

## 200MHz Current Feedback Amplifier

**élantec**

The EL400 is a wide bandwidth, fast settling monolithic amplifier built using an advanced complementary bipolar

process. This amplifier uses current-mode feedback to achieve more bandwidth at a given gain than conventional operational amplifiers. Designed for closed-loop gains of  $\pm 1$  to  $\pm 8$ , the EL400 has a 200MHz -3dB bandwidth ( $A_V = +2$ ), and 12ns settling to 0.05% while consuming only 15mA of supply current.

The EL400 is an obvious high-performance solution for video distribution and line-driving applications. With low 15mA supply current, differential gain/phase of 0.02%/0.01°, and a minimum 50mA output drive, performance in these areas is assured.

The EL400's settling to 0.05% in 12ns, low distortion, and ability to drive capacitive loads make it an ideal flash A/D driver. The wide 200MHz bandwidth and extremely linear phase allow unmatched signal fidelity. D/A systems can also benefit from the EL400, especially if linearity and drive levels are important.

## Ordering Information

PART NUMBER	TEMP. RANGE	PACKAGE	PKG. NO.
EL400CN	-40° C to +85° C	8-Pin PDIP	MDP0031
EL400CS	-40° C to +85° C	8-Pin SO	MDP0027

## Features

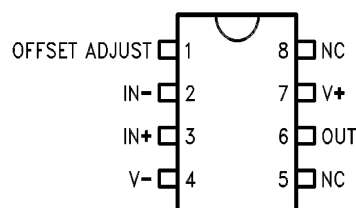
- 200MHz -3dB bandwidth,  $A_V = 2$
- 12ns settling to 0.05%
- $V_S = \pm 5V @ 15mA$
- Low distortion: HD2, HD3 @ -60dBc at 20MHz
- Differential gain 0.02% at NTSC, PAL
- Differential phase 0.01° at NTSC, PAL
- Overload/short-circuit protected
- $\pm 1$  to  $\pm 8$  closed-loop gain range
- Low cost
- Direct replacement for CLC400

## Applications

- Video gain block
- Video distribution
- HDTV amplifier
- High-speed A/D conversion
- D/A I-V conversion
- Photodiode, CCD preamps
- IF processors
- High-speed communications

## Pinout

**EL400**  
**(8-PIN PDIP, SO)**  
TOP VIEW



Manufactured under U.S. Patent No. 4,893,091

**Absolute Maximum Ratings** ( $T_A = 25^\circ\text{C}$ )

Supply Voltage ( $V_S$ ) .....  $\pm 7\text{V}$   
 Output Current .....  
 Output is short-circuit protected to ground, however, maximum reliability is obtained if  $I_{OUT}$  does not exceed 70mA.  
 Common-Mode Input Voltage .....  $\pm V_S$   
 Differential Input Voltage .....  $.5\text{V}$   
 Power Dissipation ..... See Curves

Operating Temperature .....  $-40^\circ\text{C}$  to  $+85^\circ\text{C}$   
 Pin Temperature (Soldering, 5 Seconds) .....  $300^\circ\text{C}$   
 Junction Temperature .....  $175^\circ\text{C}$   
 Storage Temperature .....  $-60^\circ\text{C}$  to  $+15^\circ\text{C}$   
 Thermal Resistance: .....  $\theta_{JA} = 95^\circ\text{C/W}$  PDIP  
 .....  $\theta_{JA} = 175^\circ\text{C/W}$  SO-8

**CAUTION:** Stresses above those listed in "Absolute Maximum Ratings" may cause permanent damage to the device. This is a stress only rating and operation of the device at these or any other conditions above those indicated in the operational sections of this specification is not implied.

**IMPORTANT NOTE:** All parameters having Min/Max specifications are guaranteed. Typical values are for information purposes only. Unless otherwise noted, all tests are at the specified temperature and are pulsed tests, therefore:  $T_J = T_C = T_A$

**Open-Loop DC Electrical Specifications**

$V_S = \pm 5\text{V}$ ,  $R_L = 100\Omega$  unless otherwise specified.

PARAMETER	DESCRIPTION	TEST CONDITIONS	TEMP	MIN	TYP	MAX	UNIT
$V_{OS}$	Input Offset Voltage		$25^\circ\text{C}$		2.0	5.5	mV
			$T_{MIN}$			8.7	mV
			$T_{MAX}$			9.5	mV
$d(V_{OS})/dT$	Average Offset Voltage Drift	(Note 1)	All		10.0	40.0	$\mu\text{V}/^\circ\text{C}$
$+I_{IN}$	+Input Current		$25^\circ\text{C}$ , $T_{MAX}$		10.0	25.0	$\mu\text{A}$
			$T_{MIN}$			41.0	$\mu\text{A}$
$d(+I_{IN})/dT$	Average +Input Current Drift	(Note 1)	All		50.0	200.0	$\text{nA}/^\circ\text{C}$
$-I_{IN}$	-Input Current		$25^\circ\text{C}$		10.0	25.0	$\mu\text{A}$
			$T_{MIN}$			41.0	$\mu\text{A}$
			$T_{MAX}$			35.0	$\mu\text{A}$
$d(-I_{IN})/dT$	Average -Input Current Drift	(Note 1)	All		100.0	200.0	$\text{nA}/^\circ\text{C}$
PSRR	Power Supply Rejection Ratio		All	40.0	50.0		dB
CMRR	Common-Mode Rejection Ratio		All	40.0	50.0		dB
$I_S$	Supply Current—Quiescent	No Load	All		15.0	23.0	mA
$+R_{IN}$	+Input Resistance		$25^\circ\text{C}$ , $T_{MAX}$	100.0	200.0		$\text{k}\Omega$
			$T_{MIN}$	50.0			$\text{k}\Omega$
$C_{IN}$	Input Capacitance		All		0.5	2.0	pF
$R_{OUT}$	Output Impedance (DC)		All		0.1	0.2	$\Omega$
CMIR	Common-Mode Input Range	(Note 2)	$25^\circ\text{C}$ , $T_{MAX}$	2.0	2.1		V
			$T_{MIN}$	1.2			V
$I_{OUT}$	Output Current		$25^\circ\text{C}$ , $T_{MAX}$	50.0	70.0		mA
			$T_{MIN}$	35.0			mA
$V_{OUT}$	Output Voltage Swing	No Load	All	3.2	3.5		V
$V_{OUTL}$	Output Voltage Swing	$100\Omega$	$25^\circ\text{C}$	3.0	3.4		V
$R_{OL}$	Transimpedance		$25^\circ\text{C}$	30.0	125.0		V/mA
			$T_{MIN}$		80.0		V/mA
			$T_{MAX}$		140.0		V/mA

**NOTES:**

1. Measured from  $T_{MIN}$  to  $T_{MAX}$ .
2. Common-Mode Input Range for Rated Performance.

## Closed-Loop AC Electrical Specifications

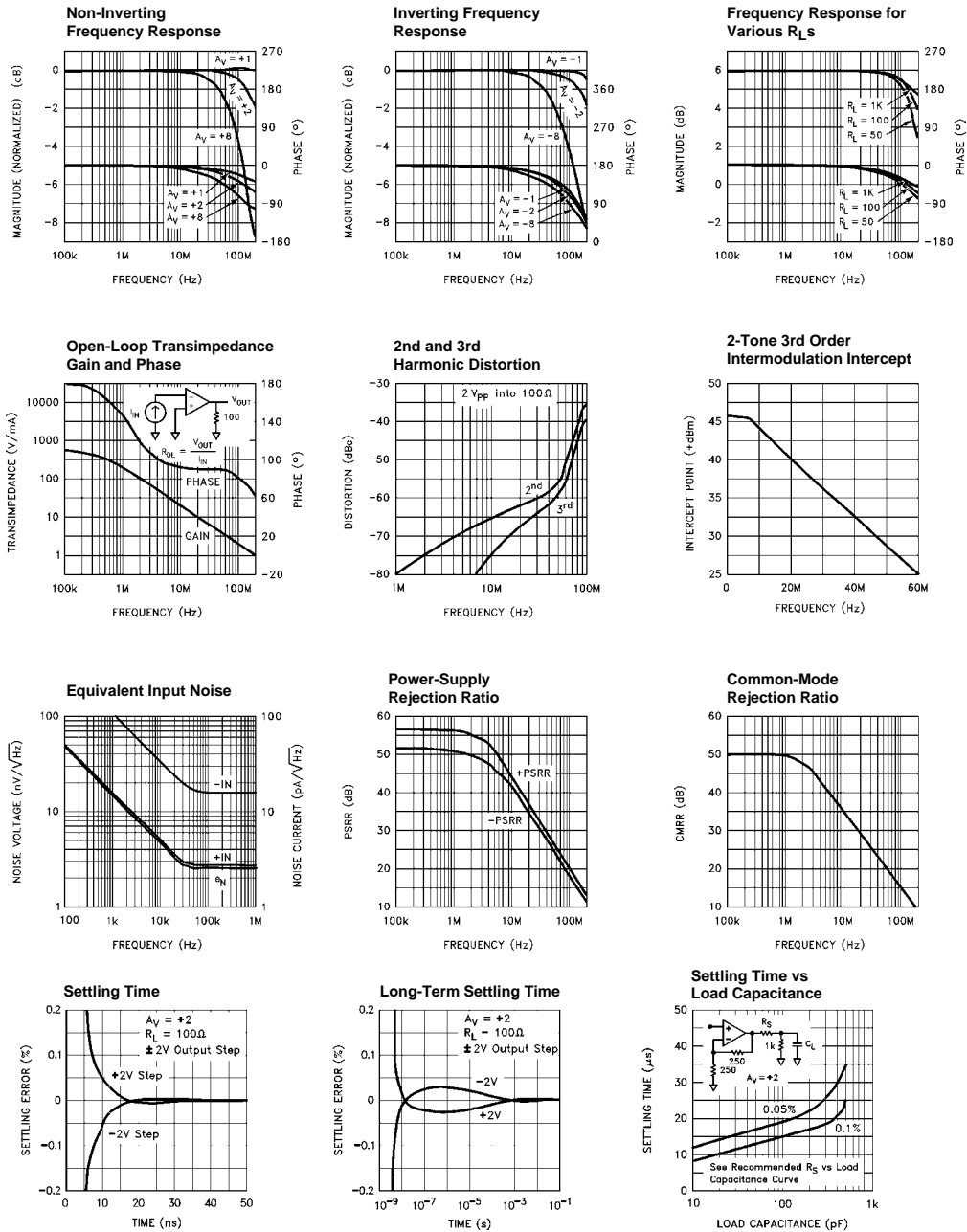
 $V_S = \pm 5V$ ,  $R_F = 250\Omega$ ,  $A_V = +2$ ,  $R_L = 100\Omega$  unless otherwise specified.

PARAMETER		DESCRIPTION	TEST CONDITIONS	TEMP	MIN	TYP	MAX	UNITS
Frequency Response	SSBW	-3dB Bandwidth ( $V_{OUT} < 0.5V_{PP}$ )		25°C	150.0	200.0		MHz
				$T_{MIN}$	150.0			MHz
				$T_{MAX}$	120.0			MHz
	LSBW	-3dB Bandwidth ( $V_{OUT} < 5.0V_{PP}$ )	$A_V = +5$	All	35.0	50.0		MHz
Gain Flatness	GFPL	Peaking $V_{OUT} < 0.5V_{PP}$	< 40MHz	25°C		0.0	0.3	dB
				$T_{MIN}, T_{MAX}$			0.4	dB
	GFPH	Peaking $V_{OUT} < 0.5V_{PP}$	> 40MHz	25°C		0.0	0.5	dB
				$T_{MIN}, T_{MAX}$			0.7	dB
	GFR	Rolloff $V_{OUT} < 0.5V_{PP}$	< 75MHz	25°C		0.6	1.0	dB
				$T_{MIN}$			1.0	dB
				$T_{MAX}$			1.3	dB
	LPD	Linear Phase Deviation $V_{OUT} < 0.5V_{PP}$	< 75MHz	25°C, $T_{MIN}$		0.2	1.0	°
				$T_{MAX}$			1.2	°
Time-Domain Response	$t_{R1}, t_{F1}$	Rise Time, Fall Time	0.5V Step	25°C, $T_{MIN}$		1.6	2.4	ns
				$T_{MAX}$			2.9	ns
	$t_{R2}, t_{F2}$	Rise Time, Fall Time	5.0V Step	All		6.5	10.0	ns
	$t_{S1}$	Settling Time to 0.1%	2.0V Step	All		10.0	13.0	ns
	$t_{S2}$	Settling Time to 0.05%	2.0V Step	All		12.0	15.0	ns
	OS	Overshoot	0.5V Step	25°C		0.0	10.0	%
				$T_{MIN}, T_{MAX}$			15.0	%
	SR	Slew Rate	$A_V = +2$	All	430.0	700.0		V/ $\mu$ s
			$A_V = -2$	All		1600.0		V/ $\mu$ s
Distortion	HD2	2nd Harmonic Distortion at 20MHz	2V <sub>PP</sub>	25°C		-60.0	-45.0	dBc
				$T_{MIN}$			-40.0	dBc
				$T_{MAX}$			-45.0	dBc
	HD3	3rd Harmonic Distortion at 20MHz	2V <sub>PP</sub>	25°C		-60.0	-50.0	dBc
				$T_{MIN}, T_{MAX}$			-50.0	dBc
Equivalent Input Noise	NF	Noise Floor > 100kHz	(Note 1)	25°C		-157.0	-154.0	dBm (1Hz)
				$T_{MIN}$			-154.0	dBm (1Hz)
				$T_{MAX}$			-153.0	dBm (1Hz)
	INV	Integrated Noise 100kHz to 200MHz	(Note 1)	25°C		40.0	57.0	$\mu$ V
				$T_{MIN}$			57.0	$\mu$ V
				$T_{MAX}$			63.0	$\mu$ V
Video Performance	$d_G$	Differential Gain (Note 2)	NTSC/PAL	25°C		0.02		% <sub>PP</sub>
	$d_P$	Differential Phase (Note 2)	NTSC/PAL	25°C		0.01		° <sub>PP</sub>
	$d_G$	Differential Gain (Note 2)	30MHz	25°C		0.05		% <sub>PP</sub>
	$d_P$	Differential Phase (Note 2)	30MHz	25°C		0.05		° <sub>PP</sub>
	VBW	-0.1dB Bandwidth (Note 2)		25°C		60.0		MHz

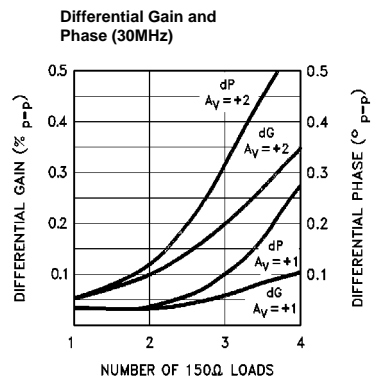
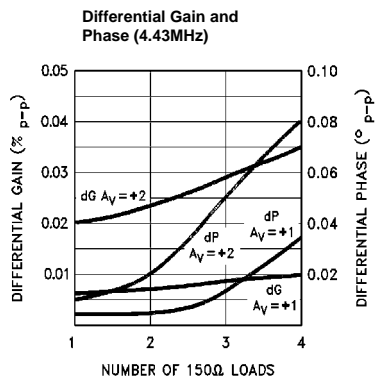
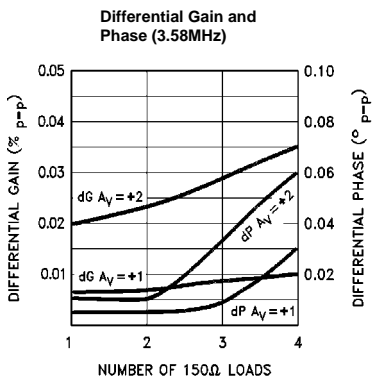
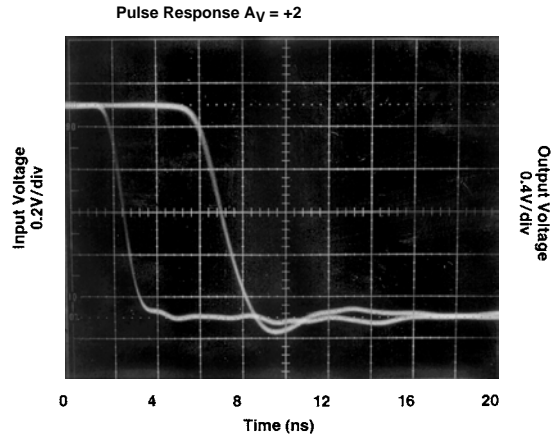
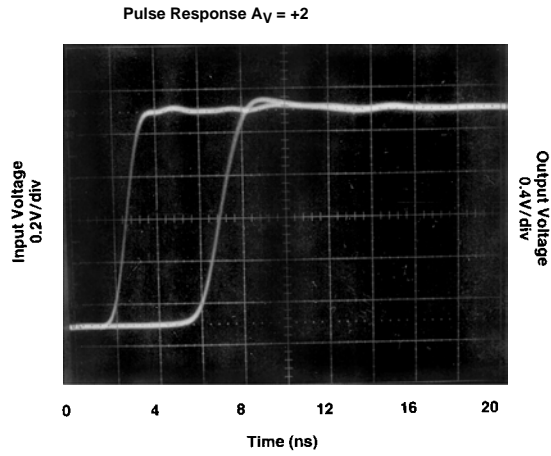
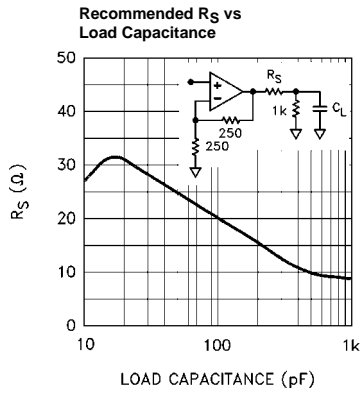
## NOTES:

- Noise Tests are Performed from 5MHz to 200MHz.
- Differential Gain/Phase Tests are  $R_L = 100\Omega$ . For other values of  $R_L$ , see curves.

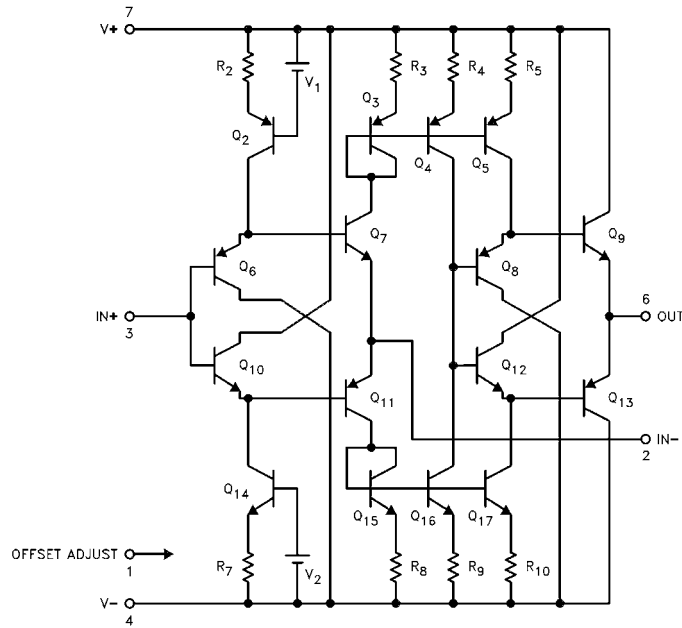
## Typical Performance Curves



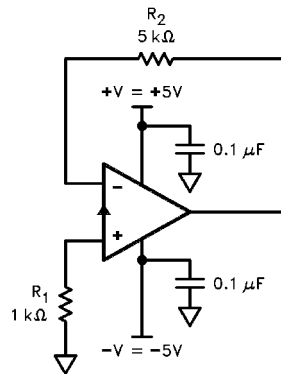
# Typical Performance Curves (Continued)



## Equivalent Circuit



## Burn-In Circuit



All Packages Use The Same Schematic.

## Applications Information

### Theory of Operation

The EL400 has a unity gain buffer from the non-inverting input to the inverting input. The error signal of the EL400 is a current flowing into (or out of) the inverting input. A very small change in current flowing through the inverting input will cause a large change in the output voltage. This current amplification is called the transimpedance ( $R_{OL}$ ) of the EL400 [ $V_{OUT} = (R_{OL}) \cdot (-I_{IN})$ ]. Since  $R_{OL}$  is very large, the

current flowing into the inverting input in the steady-state (non-slewing) condition is very small.

Therefore we can still use op-amp assumptions as a first-order approximation for circuit analysis, namely that:

1. The voltage across the inputs is approximately 0V.
2. The current into the inputs is approximately 0mA.

### Resistor Value Selection and Optimization

The value of the feedback resistor (and an internal capacitor) sets the AC dynamics of the EL400. The nominal value for

the feedback resistor is  $250\Omega$ , which is the value used for production testing. This value guarantees stability. For a given closed-loop gain the bandwidth may be increased by decreasing the feedback resistor and, conversely, the bandwidth may be decreased by increasing the feedback resistor.

Reducing the feedback resistor too much will result in overshoot and ringing, and eventually oscillations. Increasing the feedback resistor results in a lower -3dB frequency. Attenuation at high frequency is limited by a zero in the closed-loop transfer function which results from stray capacitance between the inverting input and ground. Consequently, it is very important to keep stray capacitance to a minimum at the inverting input.

### **Differential Gain/Phase**

An industry-standard method of measuring the distortion of a video component is to measure the amount of differential gain and phase error it introduces. To measure these, a 40 IRE<sub>pp</sub> reference signal is applied to the device with 0V DC offset (0IRE) at 3.58MHz for NTSC, 4.43MHz for PAL, and 30MHz for HDTV. A second measurement is then made with a 0.714V DC offset (100IRE). Differential Gain is a measure of the change in amplitude of the sine wave, and is measured in percent. Differential Phase is a measure of the change in phase, and is measured in degrees. Typically, the maximum positive and negative deviations are summed to give peak values.

In general, a back terminated cable ( $75\Omega$  in series at the drive end and  $75\Omega$  to ground at the receiving end) is preferred since the impedance match at both ends will absorb any reflections. However, when double-termination is used, the received signal is reduced by half; therefore a gain of 2 configuration is typically used to compensate for the attenuation. In a gain of 2 configuration, with output swing of  $2V_{PP}$  with each back-terminated load at  $150\Omega$ . The EL400 is capable of driving up to 4 back-terminated loads with excellent video performance. Please refer to the typical curves for more information on video performance with respect to frequency, gain, and loading.

### **Capacitive Feedback**

The EL400 relies on its feedback resistor for proper compensation. A reduction of the impedance of the feedback element results in less stability, eventually resulting in oscillation. Therefore, circuit implementations which have capacitive feedback should not be used because of the capacitor's impedance reduction with frequency. Similarly, oscillations can occur when using the technique of placing a capacitor in parallel with the feedback resistor to compensate for shunt capacitances from the inverting input to ground.

### **Offset Adjustment Pin**

Output offset voltage of the EL400 can be nulled by tying a 10k potentiometer between  $+V_S$  and  $-V_S$  with the slider attached to pin 1. A full-range variation of the voltage at pin 1 to  $\pm 5V$  results in an offset voltage adjustment of at least  $\pm 10mV$ . For best settling performance pin 1 should be bypassed to ground with a ceramic capacitor located near to the package, even if the offset voltage adjustment feature is not being used.

### **Printed Circuit Layout**

As with any high frequency device, good PCB layout is necessary for optimum performance. Ground plane construction is a requirement, as is good power-supply and Offset Adjust bypassing close to the package. The inverting input is sensitive to stray capacitance, therefore connections at the inverting input should be minimal, close to the package, and constructed with as little coupling the ground plane as possible.

Capacitance at the output node will reduce stability, eventually resulting in peaking, and finally oscillation if the capacitance is large enough. The design of the EL400 allows a larger capacitive load than comparable products, yet there are occasions when a series resistor before the capacitance may be needed. Please refer to the graphs to determine the proper resistor value needed.

**EL400 Macromodel**

\* Revision A. March 1992

\* Enhancements include PSRR, CMRR, and Slew Rate Limiting

\* Connections: +input

\* | -input

\* | | +Vsupply

\* | | | -Vsupply

\* | | | | output

\* | | | | |  
 .subckt M400 3 2 7 4 6

\* Input Stage

\*  
 e1 10 0 3 0 1.0

vis 10 9 0V

h2 9 12 vxx 1.0

r1 2 11 50

l1 11 12 48nH

iinp 3 0 8μA

iinm 2 0 8μA

\*  
 \* Slew Rate Limiting

h1 13 0 vis 600

r2 13 14 1K

d1 14 0 dclamp

d2 0 14 dclamp

\*  
 \* High Frequency Pole

\*e2 30 0 14 0 0.001666666666

l3 30 17 0.1μH

c5 17 0 0.1pF

r5 17 0 500

\*  
 \* Transimpedance Stage

g1 0 18 17 0 1.0

rol 18 0 150K

cdp 18 0 2.8pF

\*  
 \* Output Stage

q1 4 18 19 qp

q2 7 18 20 qn

q3 7 19 21 qn

q4 4 20 22 qp

r7 21 6 2

r8 22 6 2

ios1 7 19 2.5mA

ios2 20 4 2.5mA

\*  
 \* Supply Current

ips 7 4 9mA

\*  
 \* Error Terms

ivos 0 23 5mA

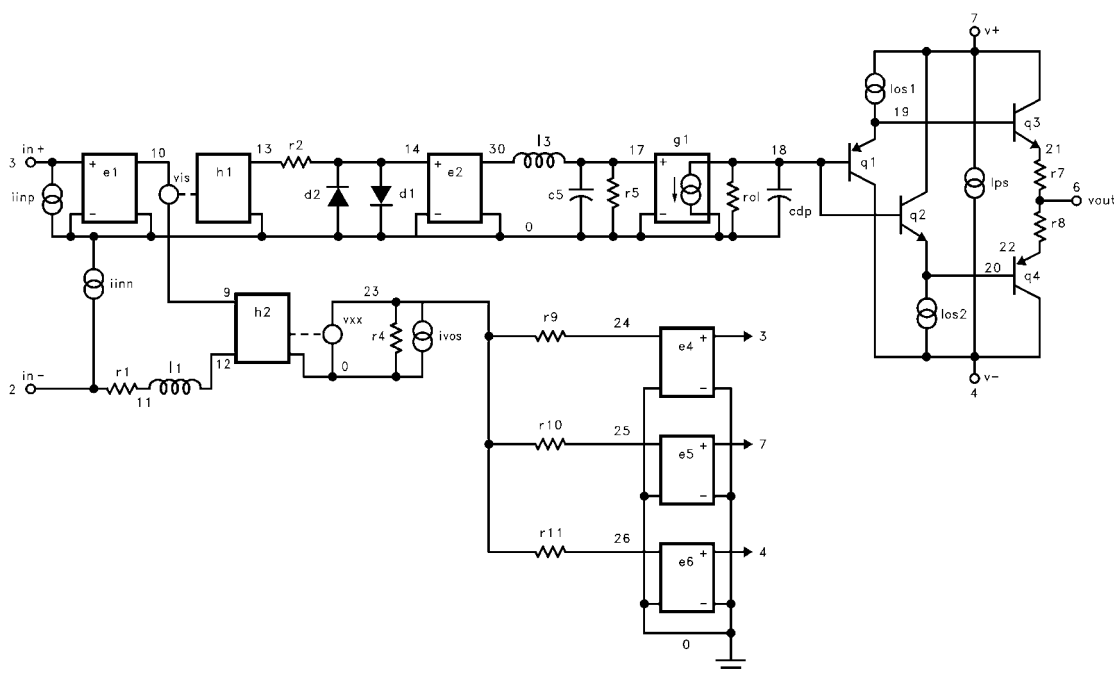


**EL400 Macromodel** (Continued)

```
vxx 23 0 0V
e4 24 0 3 0 1.0
e5 25 0 7 0 1.0
e6 26 0 4 0 1.0
r9 24 23 3K
r10 25 23 1K
r11 26 23 1K
```

## \* Models

```
.model qn npn (is=5e-15 bf=200 tf=0.5nS)
.model qp npn (is=5e-15 bf=200 tf=0.5nS)
.model dclamp d(is=1e-30 ibv=0.266 bv=1.3 n=4)
.ends
```



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