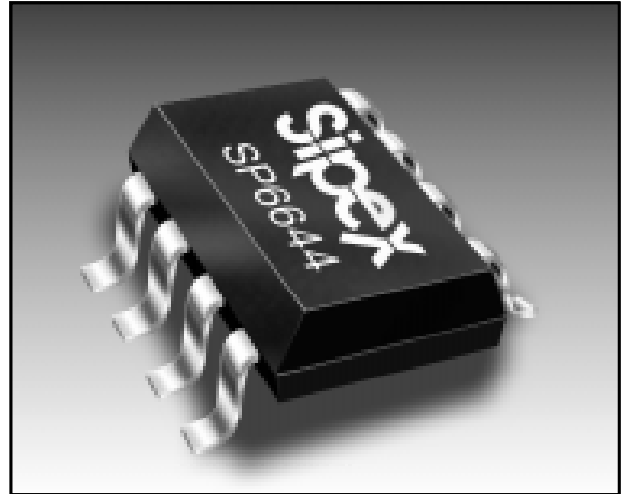


## Single/Dual Alkaline Cell, High Efficiency Boost DC-DC Regulator

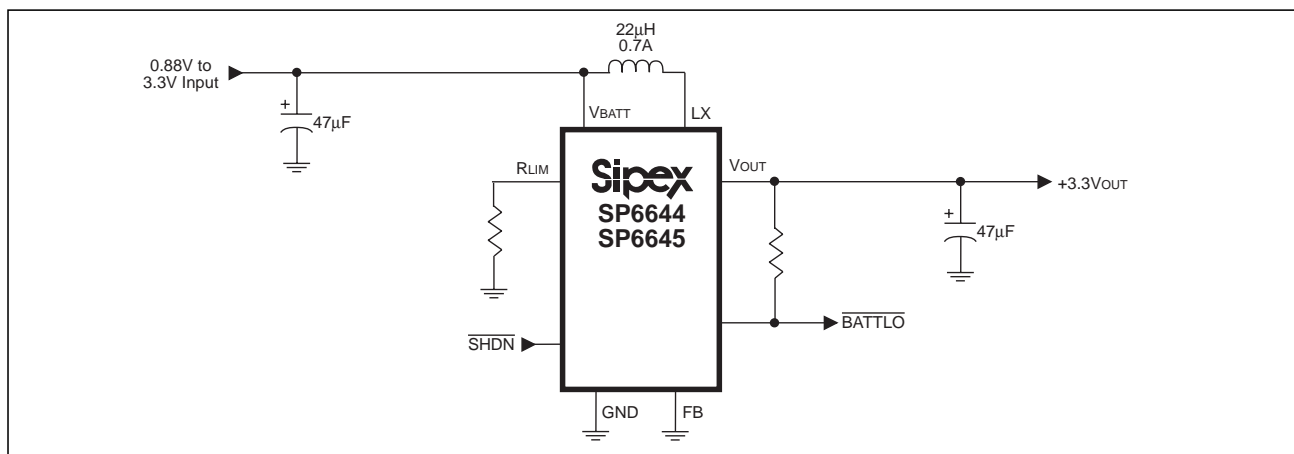
- 90mA Output Current at 1.3V Input
- 190mA Output Current at 2.6V Input
- +2V to +5.5V Output Range
- 0.88V Guaranteed Start-Up
- 92% High Efficiency
- 1.6 $\mu$ A Quiescent Supply Current at  $V_{BATT}$
- Reverse Battery Protection
- Internal Synchronous Rectifier
- 5nA Logic Controlled Shutdown Current From  $V_{BATT}$
- Low-Battery Detection Active LOW Output
- Extremely Small  $\mu$ SOIC Package
- Flexibility to Optimize Inductor Type with Programmable Peak Current Control
- No External FETs



### DESCRIPTION

The SP6644/6645 devices are high-efficiency, low-power step-up DC-DC converters ideal for single or dual alkaline cell applications such as pagers, remote controls, pointing devices, medical monitors, and other low-power portable end products. Designers can control the SP6644 device with a 1nA active LOW shutdown input. The SP6644 device features an active low output for batteries below +1.0V. The SP6645 device features an active low output for batteries below +2.0V. Both devices contain a 0.8 $\Omega$  synchronous rectifier, a 0.5 $\Omega$  N-channel MOSFET power switch, an internal voltage reference, circuitry for pulse-frequency-modulation, and an under voltage comparator. The output voltage for the SP6644/6645 devices is preset to +3.3V  $\pm$  4% or can be adjusted from +2V to +5.5V by manipulating two external resistors.

### SP6644/45 +3.3V Typical Application Circuit



## ABSOLUTE MAXIMUM RATINGS

These are stress ratings only and functional operation of the device at these ratings or any other above those indicated in the operation sections of the specifications below is not implied. Exposure to absolute maximum rating conditions for extended periods of time may affect reliability.

$V_{BATT}$ to GND.....	-0.3 to 6.0V
$V_{OUT}$ to GND.....	-0.3 to 6.0V
LX, SHDN, FB, BATTLO, to GND.....	-0.3 to 6.0V
Reverse battery Current, $T_{AMB}=+25^{\circ}\text{C}$ .....	220mA
(NOTE 1)	
$V_{BATT}$ forward current.....	0.5A
$V_{OUT}$ , LX current.....	1A
Storage Temperature Range.....	-65°C to +165°C
Lead Temperature (soldering 10s).....	+300°C
Operating Temperature.....	-40°C to +85°C

### Power Dissipation Per Package

8-pin  $\mu\text{SOIC}$  (derate 4.85mW/°C above +70°C).....390mW



**CAUTION:**  
ESD (ElectroStatic Discharge) sensitive device. Permanent damage may occur on unconnected devices subject to high energy electrostatic fields. Unused devices must be stored in conductive foam or shunts. Personnel should be properly grounded prior to handling this device. The protective foam should be discharged to the destination socket before devices are removed.

## SPECIFICATIONS

$V_{BATT} = V_{SHDN} = 1.3\text{V}$ ,  $I_{LOAD} = 0\text{mA}$ ,  $\text{FB} = \text{GND}$ ,  $T_{AMB} = -40^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ , and typical values are at  $T_{AMB} = +25^{\circ}\text{C}$  unless otherwise noted.

PARAMETER	MIN.	TYP.	MAX.	UNITS	CONDITIONS
Minimum Operating Input Voltage, $V_{BATT(MIN)}$		0.3		V	$R_L = 3\text{k}\Omega$
Maximum Operating Input Voltage, $V_{BATT(MAX)}$			3.3	V	
Start-Up Input Voltage, $V_{BATT}$	0.88	0.82		V	$R_L = 3\text{k}\Omega, T_{AMB} = +25^{\circ}\text{C}$
Start-Up Input Voltage, $V_{BATT}$ , Temperature Coefficient		-1		mV/°C	
SHDN Input Voltage $V_{IL}$ $V_{IH}$	80		20	%	% of $V_{BATT}$ % of $V_{BATT}$
SHDN Input Current		1	100	nA	
FB Input Current		1	10	nA	$V_{FB} = 1.3\text{V}$
FB Set Voltage, $V_{FB}$	1.215	1.262	1.309	V	external feedback
BATTLO Trip Voltage	0.96 1.92	1.00 2.00	1.04 2.08	V	SP6644, $V_{OUT} = 3.3\text{V}$ , hysteresis =2% SP6645, $V_{OUT} = 3.3\text{V}$ , hysteresis =2%
Output Voltage, $V_{OUT}$	3.16	3.30	3.44	V	$V_{FB} < 0.1\text{V}$
Output Voltage Range	2.0		5.5	V	external feedback
Output Current		190		mA	$V_{BATT} = 2.6\text{V}$ , $R_{LIM} = 2.5\text{k}$ , See Fig. 11
N-Channel On-Resistance		0.5	1.0	$\Omega$	$V_{OUT} = 3.3\text{V}$
P-Channel On-Resistance		0.8	1.6	$\Omega$	$V_{OUT} = 3.3\text{V}$

## SPECIFICATIONS (continued)

$V_{BATT} = V_{SHDN} = 1.3V$ ,  $I_{LOAD} = 0mA$ ,  $FB = GND$ ,  $T_{AMB} = -40^{\circ}C$  to  $+85^{\circ}C$ , and typical values are at  $T_{AMB} = +25^{\circ}C$  unless otherwise noted.

PARAMETER	MIN.	TYP.	MAX.	UNITS	CONDITIONS
Quiescent Current into $V_{OUT}$ , $I_{QOUT}$		50	80	$\mu A$	$V_{OUT} = 3.5V$
Quiescent Current into $V_{BATT}$ , $I_{QBATT}$		1.6	3.0	$\mu A$	$V_{BATT} = 1.0V$
Shutdown Current into $V_{OUT}$ , $I_{SHDNOUT}$		0.001	0.5	$\mu A$	$V_{OUT} = 3.5V$
Shutdown Current into $V_{BATT}$ , $I_{SHDNBATT}$		0.005	0.1	$\mu A$	$V_{BATT} = 1.0V$
Low Output Voltage for $\overline{BATTLO}$ , $V_{OL}$			0.4	V	$V_{BATT} = 0.9V, V_{OUT} = +3.3V, I_{SINK} = 1mA$
Leakage Current for $\overline{BATTLO}$			1	$\mu A$	$V_{BATT} = 1.3V, V_{\overline{BATTLO}} = 3.5V$
Efficiency		89		%	$I_{LOAD} = 150mA, V_{BATT} = 2.6V$
Inductor Peak Current, $I_{PEAK}$	245	275	305	mA	$R_{LIM} = 5k\Omega$ , NOTE 4
Inductor Range	22		330	$\mu H$	
$R_{LIM}$ Range	2.5		9.3	k $\Omega$	

**NOTE 1:** The reverse battery current is measured from the Typical Operating Circuit's input terminal to GND when the battery is connected backward. A reverse current of 220mA will not exceed package dissipation limits but, if left for an extended time (more than 10 minutes), may degrade performance.

**NOTE 2:** Specifications to  $-40^{\circ}C$  are guaranteed by design, not production tested.

**NOTE 3:** Inductor Peak Current where  $I_{PEAK} = \frac{1400}{R_{LIM}}$

# PERFORMANCE CHARACTERISTICS

Refer to the circuit in Figure 28,  $T_{AMB} = +25^{\circ}\text{C}$  unless otherwise noted.

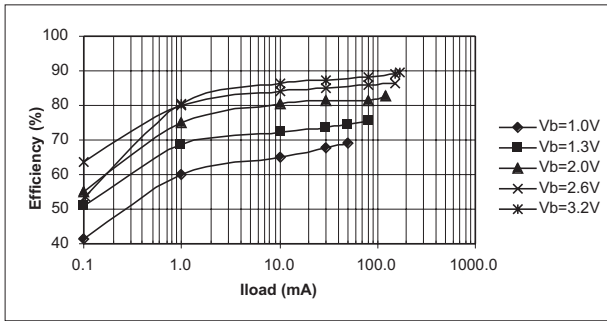


Figure 1. Efficiency vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43

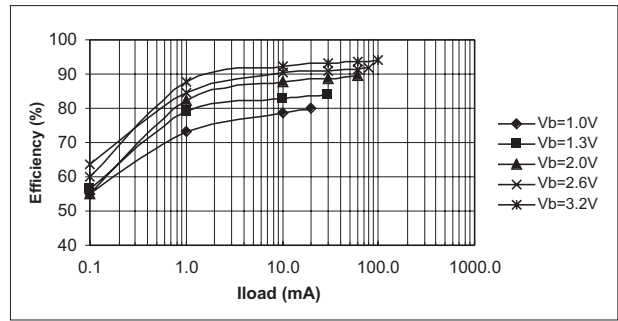


Figure 2. Efficiency vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43

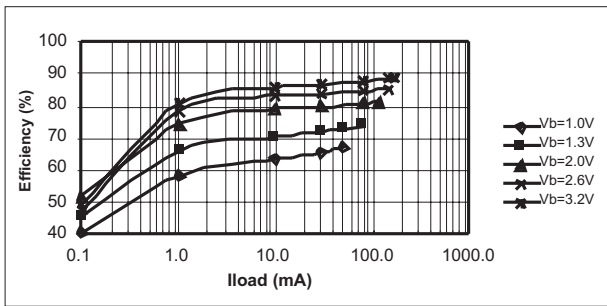


Figure 3. Efficiency vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CDRH5D18 Low Profile

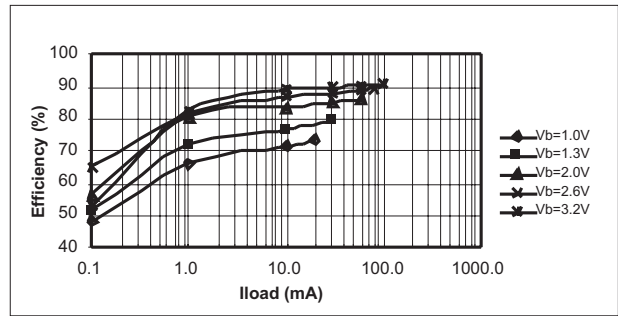


Figure 4. Efficiency vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=5\text{k}$ ,  $L_i=100\mu\text{H}$  Sumida CD54

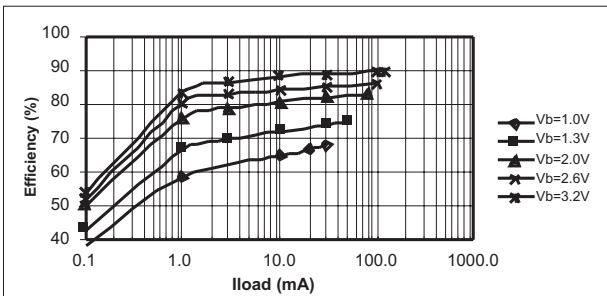


Figure 5. Efficiency vs. Output Current ( $V_{out}=5\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43, Refer to Figure 29,  $R_1=499\text{k}$ ,  $R_2=169\text{k}$

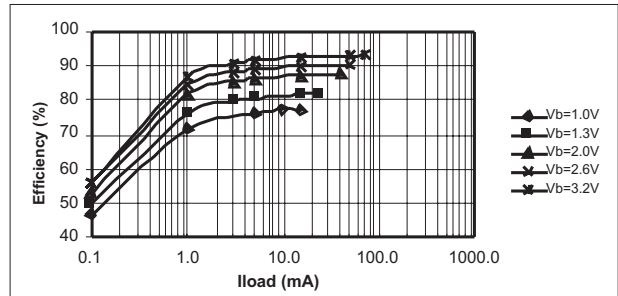


Figure 6. Efficiency vs. Output Current ( $V_{out}=5\text{V}$ ),  $R_{lim}=5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43, Refer to Figure 29,  $R_1=499\text{k}$ ,  $R_2=169\text{k}$

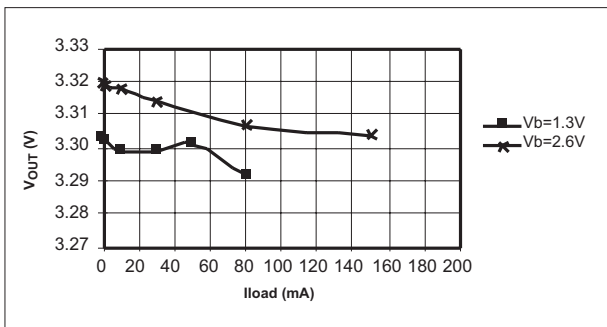


Figure 7. Line/Load Rejection vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43

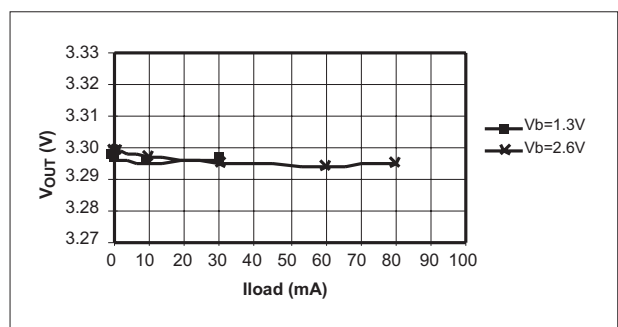


Figure 8. Line/Load Rejection vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43

# PERFORMANCE CHARACTERISTICS

Refer to the circuit in Figure 28,  $T_{AMB} = +25^{\circ}\text{C}$  unless otherwise noted.

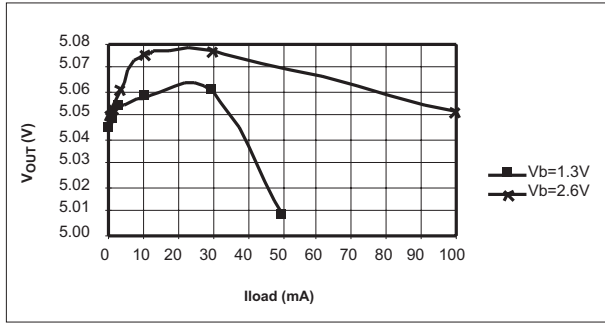


Figure 9. Line/Load vs. Output Current ( $V_{out}=5\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43, Refer to figure 29,  $R_1=499\text{k}$ ,  $R_2=169\text{k}$

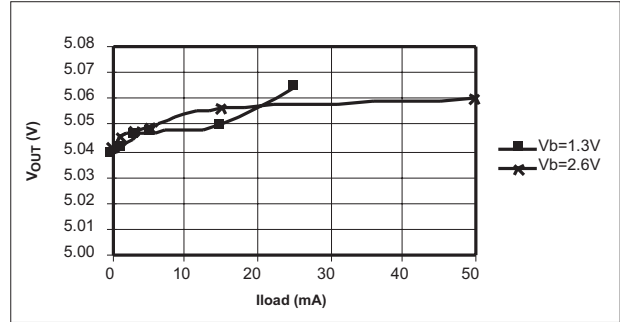


Figure 10. Line/Load vs. Output Current ( $V_{out}=5\text{V}$ ),  $R_{lim}=5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD43, Refer to figure 29,  $R_1=499\text{k}$ ,  $R_2=169\text{k}$

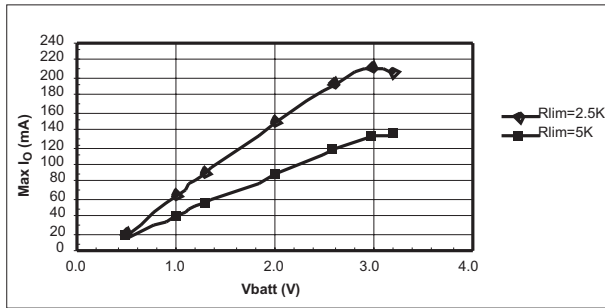


Figure 11. Maximum Load Current vs.  $V_{batt}$  ( $V_{out}=3.3\text{V}$ ),  $L_i=22\mu\text{H}$  Sumida CD43

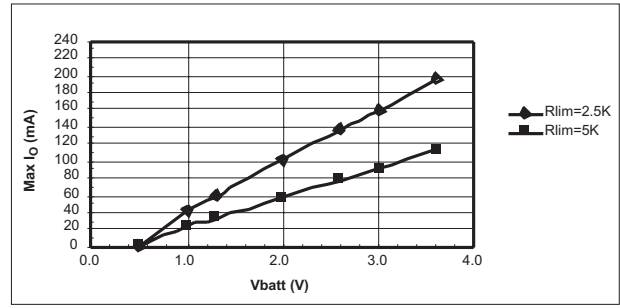


Figure 12. Maximum Load Current vs.  $V_{batt}$  ( $V_{out}=5\text{V}$ ),  $L_i=22\mu\text{H}$  Sumida CD43, Refer to Figure 29,  $R_1=499\text{k}$ ,  $R_2=169\text{k}$

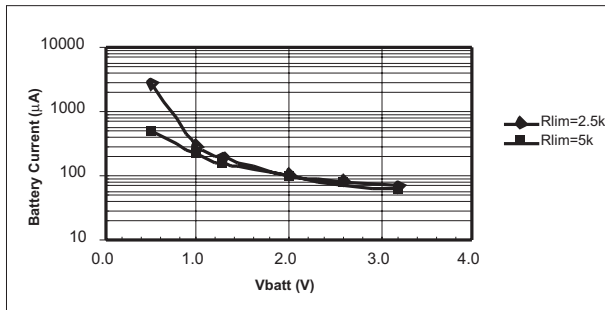


Figure 13. No Load Battery Current vs.  $V_{batt}$  ( $V_{out}=3.3\text{V}$ ),  $L_i=22\mu\text{H}$  Sumida CD43

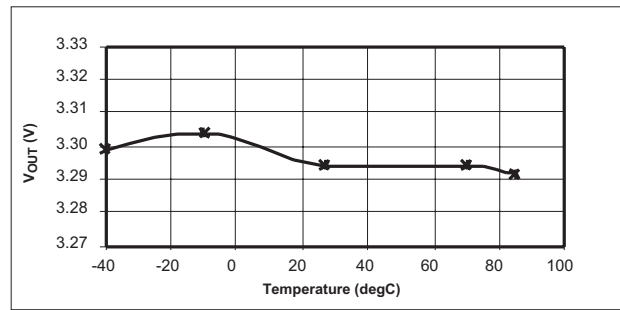


Figure 14. Output Voltage vs. Temperature,  $R_{lim}=2.5\text{k}$ ,  $R_{load}=3\text{k}$ , ( $V_{out}=3.3\text{V}$ ),  $L_i=22\mu\text{H}$  Sumida CD43

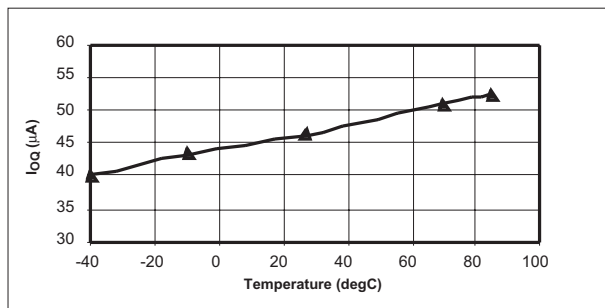


Figure 15.  $I_o$  Pin Quiescent Current vs. Temperature, ( $V_{out}=3.3\text{V}$ )

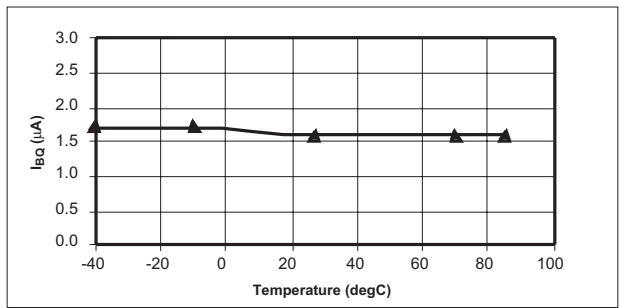


Figure 16.  $I_{batt}$  Pin Quiescent Current vs. Temperature, ( $V_{out}=3.3\text{V}$ ),  $V_{batt}=1.0\text{V}$

# PERFORMANCE CHARACTERISTICS

Refer to the circuit in Figure 28,  $T_{AMB} = +25^{\circ}\text{C}$  unless otherwise noted.

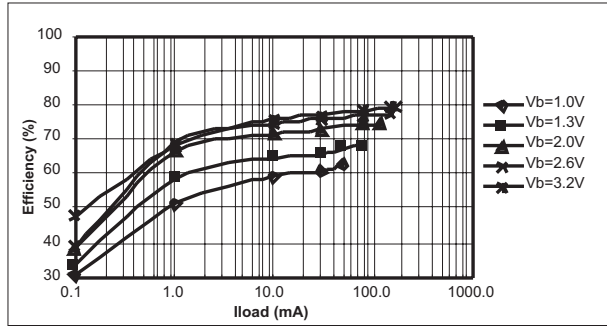


Figure 17. SP6644/6201 DC/DC LDO Combination Efficiency vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43, Refer to Figure 30

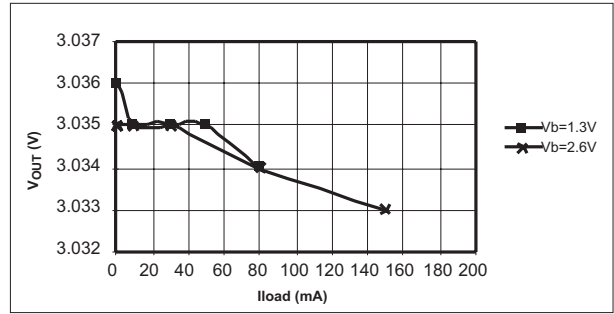


Figure 18. SP6644/6201 LDO Line/Load Rejection vs. Output Current ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43, Refer to Figure 30

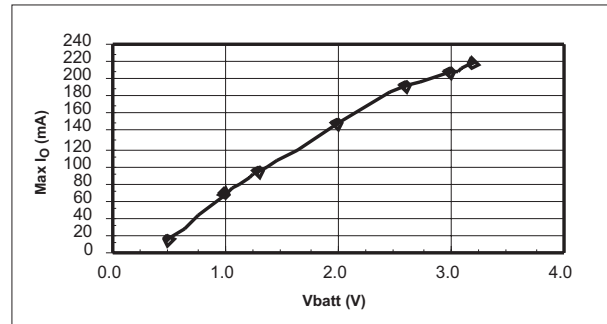


Figure 19. SP6644/6201 DC/DC LDO Maximum Load Current vs.  $V_{batt}$  ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43, Refer to Figure 30

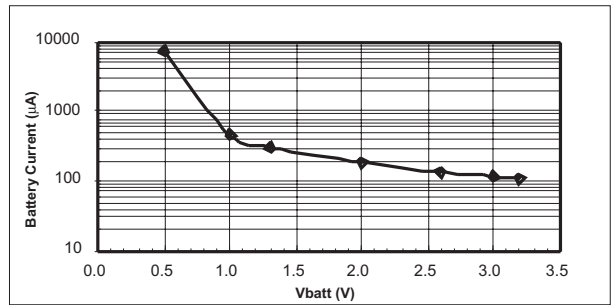


Figure 20. SP6644/6201 DC/DC LDO No-Load  $I_{batt}$  vs.  $V_{batt}$  ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43, Refer to Figure 30

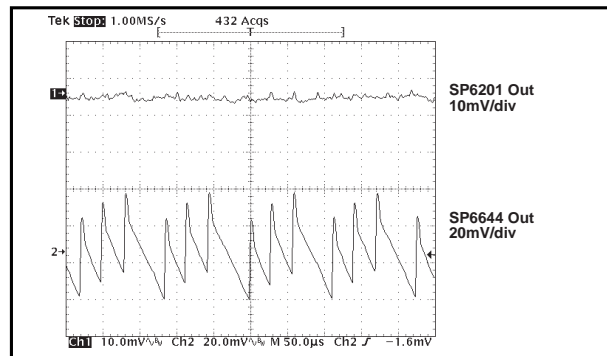


Figure 21. SP6644/6201 DC/DC LDO Output Ripple Voltage ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43, Refer to Figure 30

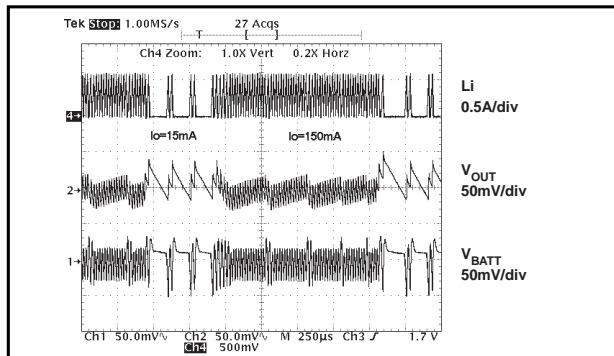


Figure 22. Load Transient Response,  $V_{batt}=1.3\text{V}$ , ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43

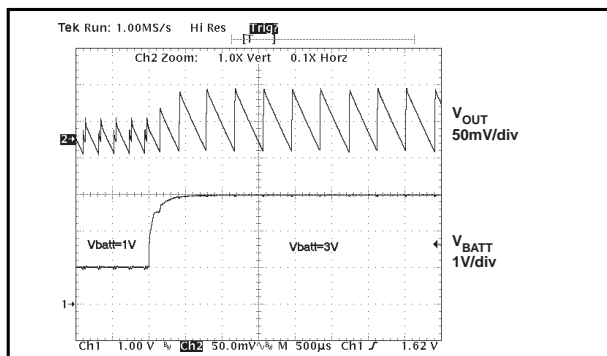


Figure 23. Line Transient Response, ( $V_{out}=3.3\text{V}$ ),  $R_{lim}=2.5\text{k}$ ,  $I_{load}=22\mu\text{H}$  Sumida CD-43

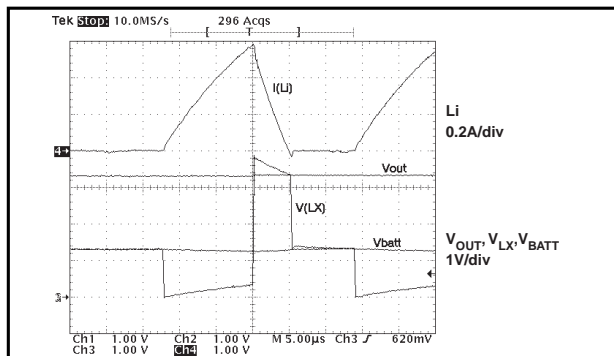


Figure 24. Switching Waveforms, ( $V_{out}=3.3\text{V}$ ),  $V_{batt}=1.3\text{V}$ ,  $R_{lim}=2.5\text{k}$ ,  $I_{load}=10\text{mA}$ ,  $L_i=22\mu\text{H}$  Sumida CD-43

## PERFORMANCE CHARACTERISTICS (continued)

Refer to the circuit in Figure 28,  $T_{AMB} = +25^{\circ}\text{C}$ , unless otherwise noted.

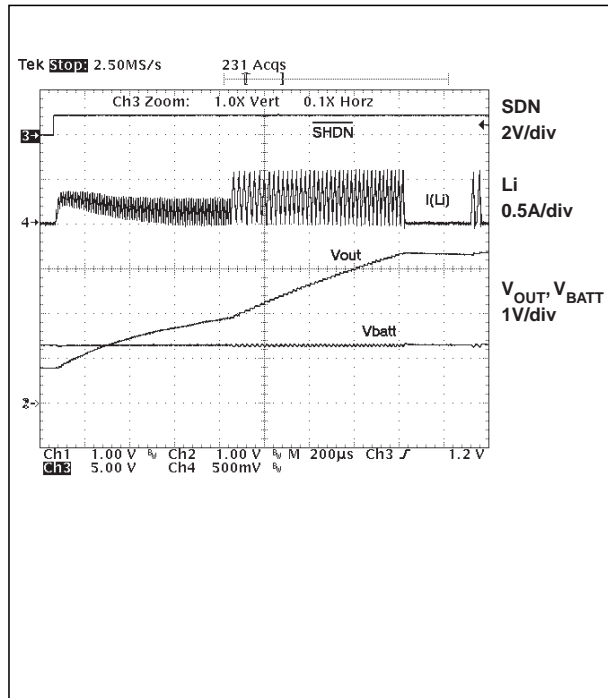


Figure 25. Shutdown Response and Inductor Current,  $V_{out}=3.3\text{V}$ ,  $V_{batt}=1.3\text{V}$ ,  $R_{lim}=2.5\text{k}$ ,  $R_{load}=550\ \Omega$ ,  $L_i=22\ \mu\text{H}$  Sumida CD43

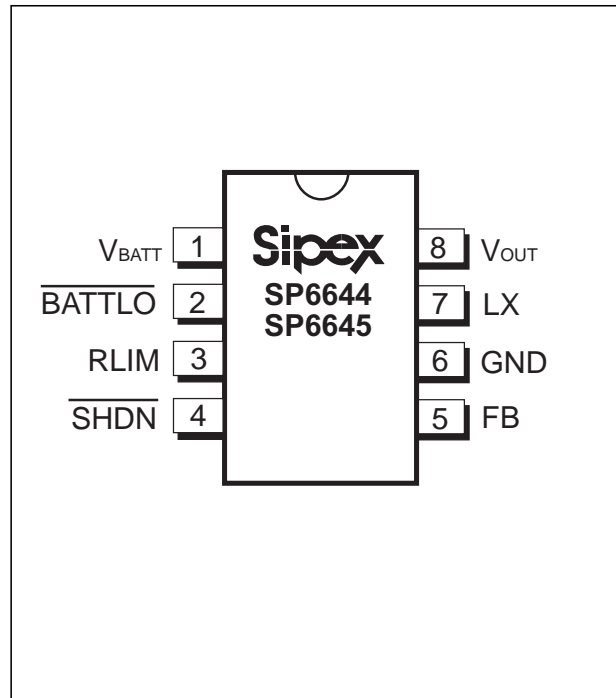


Figure 26. Pinout for the SP6644/6645

NAME	FUNCTION	PIN NO.
$V_{BATT}$	Battery Supply. This pin ties to the sensor input of the BATTLO comparator.	1
$\overline{\text{BATTLO}}$	Open-Drain Battery Low Output. When the voltage drops below 1V for the <b>SP6644</b> or 2V for the <b>SP6645</b> , BATTLO sinks current.	2
$R_{LIM}$	Resistor Programmable Inductor Peak Current. Connecting a resistor from this pin to ground programs the inductor peak current where $I_{PEAK} = \frac{1400}{R_{LIM}}$	3
$\overline{\text{SHDN}}$	Active-LOW Shutdown Input. Connect to $V_{BATT}$ for normal operation.	4
FB	Feedback Input. Input for adjustable-output operation. Connect this input pin to an external resistor voltage divider between $V_{OUT}$ and GND. Connect to GND for fixed-output operation.	5
GND	Connect to the lowest circuit potential, typically ground.	6
LX	Coil. An inductor is connected from $V_{BATT}$ to the N-Channel MOSFET switch drain and the P-Channel synchronous-rectifier drain through this pin.	7
$V_{OUT}$	Power Output. Feedback input for fixed 3.3V operation and IC power input. Connect filter capacitor close to $V_{OUT}$ .	8

Table 1. SP6644/6645 Pin Descriptions



## DESCRIPTION

The SP6644/6645 devices are high-efficiency, low-power step-up DC-DC converters ideal for single or dual alkaline cell applications such as pagers, remote controls, and other low-power portable end products.

The SP6644/6645 devices feature a 5nA logic-controlled shutdown mode and a dedicated low-battery detector circuitry. Both devices contain a  $0.8\Omega$  synchronous rectifier, a  $0.5\Omega$  N-channel MOSFET power switch, an internal voltage reference, circuitry for pulse-frequency-modulation, and an under voltage comparator. The output voltage for the SP6644/6645 devices can be adjusted from +2V to +5.5V by manipulating two external resistors. The output voltage is preset to +3.3V.

## THEORY OF OPERATION

The SP6644/6645 devices are ideal for end products that function with a single or dual alkaline cell, such as remote controls, pagers, and other portable consumer products. Designers can implement the SP6644/6645 devices into applications with the following power management operating states: 1. where the primary battery is good and the load is active, and 2. where the primary battery is good and the load is sleeping.

In the first operating state where the primary supply is good and the load is active, the SP6644/6645 devices typically offer 88% efficiency, drawing tens of milliamps.

Applications will predominantly operate in the second state where the primary supply is good and the load is sleeping. The SP6644/6645 devices draw a very low quiescent current while the load in its disabled state will draw typically hundreds of microamps.

The pulse-frequency-modulation (PFM) circuitry provides higher efficiencies at low to moderate output loads than traditional PWM converters are capable of delivering.

In a state where the error comparator detects that the output voltage at  $V_{OUT}$  is too low, the internal N-channel MOSFET switch is turned on until the

peak inductor current is satisfied. This is indicated by the falling edge of the I-Charge comparator output. The approximate inductor charging time is defined by:

$$t_{CHARGE} \cong L \times I_{PEAK} / V_{BATT}$$

where  $t_{CHARGE}$  [s] is the approximate inductor charging time,  $L$  [H] is the inductance,  $I_{PEAK}$  [A] is the peak inductor current, and  $V_{BATT}$  [V] is the input voltage to the device.

The peak inductor current,  $I_{PEAK}$ , is programmed externally by putting a resistor between the  $R_{LIM}$  pin and ground. This is defined by:

$$I_{PEAK} = \frac{1400}{R_{LIM}}$$

where  $I_{PEAK}$  [A] is the peak inductor current and  $R_{LIM}$  [ $\Omega$ ] is the value of the resistor connected from pin  $R_{LIM}$  to ground.

When the charging N MOSFET turns off, the discharging P MOSFET turns on and the inductor current flows into the output capacitor and the load recharging the output. When the current through the discharging P MOSFET approaches zero, the I-Discharge comparator indicates to the logic to turn off the P MOSFET. The approximate time for discharging the inductor current can be determined by:

$$t_{DCHG} \cong \frac{L \times I_{PEAK}}{V_{OUT} - V_{BATT}}$$

where  $t_{DCHG}$  [s] is the time to discharge the inductor,  $L$  [H] is the inductance,  $I_{PEAK}$  [A] is the peak inductor current,  $V_{OUT}$  [V] is the output voltage, and  $V_{BATT}$  [V] is the input voltage to the device.

The output filter capacitor stores charge while current from the inductor is high and holds the output voltage high until the discharge phase of the next switching cycle, smoothing power flow to the load. Between switching cycles, the inductor damping switch is closed suppressing the ringing caused by the inductor and the parasitic capacitance on the LX node.



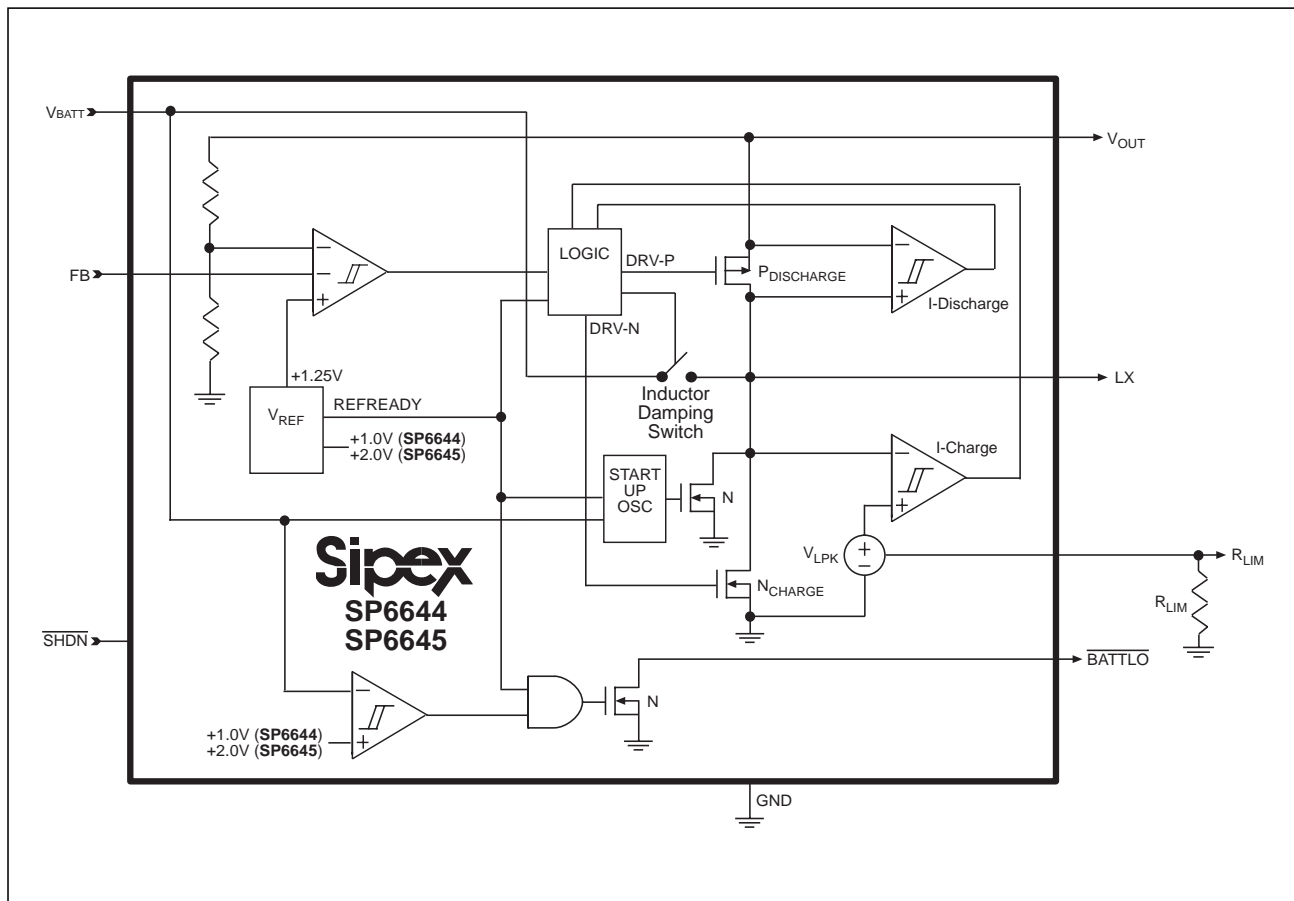


Figure 27. Internal Block Diagram of the SP6644/6645

## Internal Bootstrap Circuitry

The internal bootstrap circuitry contains a low-voltage start-up oscillator that pumps up the output voltage to approximately 1.9V so the main DC-DC converter can function. At lower battery supply voltages, the circuitry can start up with low-load conditions. Designers can reduce the load as needed to allow start-up with input voltages below 1V. Refer to *Figures 10 to 13*. Once started, the output voltage can maintain the load as the battery voltage decreases below the initial start-up voltage. The start-up oscillator is powered by  $V_{BATT}$  driving a charge pump and NMOS switch. During start-up, the P-channel synchronous rectifier remains off and either its body diode or an external diode is used as an output rectifier.

## BATTLO Circuitry

The SP6644 device has an internal comparator for low-battery detection. If  $V_{BATT}$  drops below 1V,  $\overline{BATTLO}$  will sink current.  $\overline{BATTLO}$  is an open-drain output. The SP6645 operates in the same manner with a threshold voltage of 2V.

## Shutdown for the SP6644

A logic LOW at  $\overline{SHDN}$  will drive the SP6644 into a shutdown mode where  $\overline{BATTLO}$  goes into a high-impedance state, the internal switching MOSFET turns off, and the synchronous rectifier turns off to prevent reverse current from flowing from the output back to the input. Designers should note that in shutdown, the output can drift to one diode drop below  $V_{BATT}$  because there is still a forward current path through the synchronous-rectifier body diode from the input to the output. To disable the shutdown feature, designers can connect  $\overline{SHDN}$  to  $V_{BATT}$ .

## Adjustable Output Voltage

Driving FB to ground (logic LOW) will drive the output voltage to the fixed-voltage operation of  $+3.3V \pm 4\%$ . Connecting FB to a voltage divider between  $V_{OUT}$  and ground will select an adjustable output voltage between +2V and +5.5V. Refer to *Figure 28*. FB regulates to +1.25V.

Since the FB leakage current is 10nA maximum, designers should select the feedback resistor R2 in the 100k $\Omega$  to 1M $\Omega$  range. R1 can be determined with the following equation:

$$R1 = R2 \times \left[ \frac{V_{OUT}}{V_{REF}} - 1 \right]$$

where R1 [ $\Omega$ ] and R2 [ $\Omega$ ] are the feedback resistors in *Figure 29*,  $V_{OUT}$  [V] is the output voltage, and  $V_{REF}$  [V] is 1.25V.

## Battery Reversal Protection

The SP6644/6645 devices will tolerate single-cell battery reversal up to the package power-dissipation limits noted in the **ABSOLUTE MAXIMUM RATINGS** section. An internal diode in series with an internal 5 $\Omega$  resistor limits any reverse current to less than 220mA preventing damage to the devices. Prolonged operation above 220mA reverse-battery current can degrade performance of the devices.

## The Inductor

The programmable peak inductor current feature of the SP6644/6645 devices affords a great deal of flexibility in choosing an inductor. The most important point to consider when choosing an inductor is to insure that the peak inductor current is programmed below the saturation rating of the inductor. If the inductor goes into saturation, the internal switches and the inductor will be stressed due to current peaking, potentially leading to reliability problems with the application circuit.

The peak inductor current is programmed by putting a resistor between the  $R_{LIM}$  pin and ground. The usable current range is between 150mA and 560mA. This is defined by:

$$I_{PEAK} = \frac{1400}{R_{LIM}}$$

where  $I_{PEAK}$  [A] is the peak inductor current, and  $R_{LIM}$  [ $\Omega$ ] is the value of the resistor connected from pin  $R_{LIM}$  to ground.

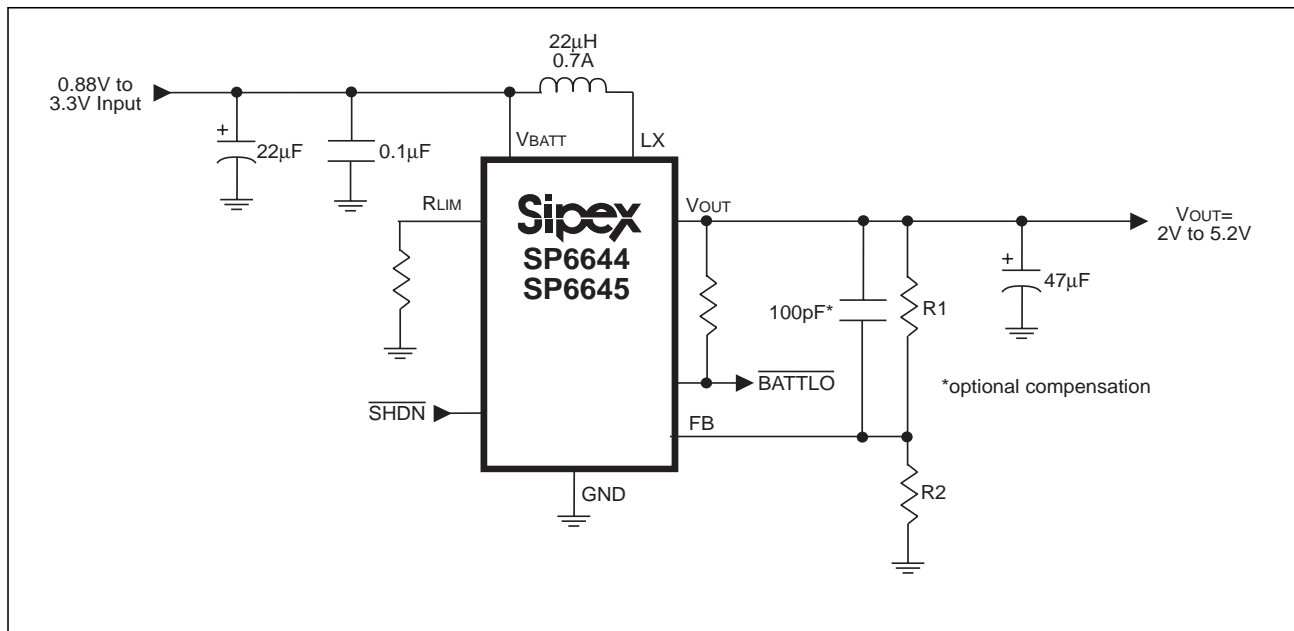


Figure 28. Adjustable Output Voltage Circuitry

With an external resistor tolerance of  $\pm 1\%$ , the peak current tolerance will be  $\pm 6\%$ . To make sure that the SP6644/6645 internal circuitry adequately controls the inductor current, it is recommended that values equal to or greater than  $22\mu\text{H}$  ( $\pm 10\%$ ) be used.

The SP6644/6645 devices control algorithm delivers an average maximum load current in regulation as defined by:

$$I_{\text{LOAD-MAX}} = \frac{E \times I_{\text{PEAK}} \times V_{\text{BATT}}}{2 \times V_{\text{OUT}}}$$

where  $I_{\text{LOAD-MAX}}$  [A] is the maximum load current, E is the efficiency factor (generally between 0.8 and 0.9),  $I_{\text{PEAK}}$  [A] is the programmed peak inductor current,  $V_{\text{BATT}}$  [V] is the input voltage to the device, and  $V_{\text{OUT}}$  [V] is the output voltage.

Given the minimum input voltage, output voltage, and maximum average load current, the value of  $I_{\text{PEAK}}$  can be solved for and an appropriate inductor can be chosen. It is good design practice to use the lowest peak current possible to reduce possible EMI and output ripple voltage. A closed-core inductor, such as a toroid or shielded bobbin, will minimize any fringe magnetic fields or EMI.

## APPLICATION NOTES

Printed circuit board layout is a critical part of design. Poor designs can result in excessive EMI on the voltage gradients and feedback paths on the ground planes with applications involving high switching frequencies and large peak currents. Excessive EMI can result in instability or regulation errors.

All power components should be placed on the PC board as closely as possible with the traces kept short, direct, and wide ( $\geq 50\text{mils}$  or  $1.25\text{mm}$ ). Extra copper on the PC board should be integrated into ground as a pseudo-ground plane. On a multilayer PC board, route the star ground using component-side copper fill, then connect it to the internal ground plane using vias.

For the SP6644/6645 devices, the inductor and input and output filter capacitors should be soldered with their ground pins as close together as possible in a star-ground configuration. The  $V_{\text{OUT}}$  pin must be bypassed directly to ground as close to the SP6644/6645 devices as possible (within  $0.2\text{in}$  or  $5\text{mm}$ ). The DC-DC converter and any digital circuitry should be placed on the opposite corner of the PC board as far away from sensitive RF and analog input stages. The external voltage-feedback network should be placed very close to the FB pin as well as the  $R_{\text{LIM}}$  resistor (within  $0.2\text{in}$  or  $5\text{mm}$ ). Any

noisy traces, such as from the LX pin, should be kept away from the voltage-feedback network and separated from it using grounded copper to minimize EMI.

Capacitor equivalent series resistance is a major contributor to output ripple, usually greater than 60%. Low ESR capacitors are recommended. Ceramic capacitors have the lowest ESR. Low-ESR tantalum capacitors may be a more acceptable solution having both a low ESR and lower cost than ceramic capacitors. Designers should select input and output capacitors with a rating exceeding the peak inductor current. Do not allow tantalum capacitors to exceed their ripple-current ratings. A 22 $\mu$ F, 6V, low-ESR, surface-mount tantalum output filter capacitor typically provides 60mV output ripple when stepping up from 1.3V to 3.3V at 20mA. An input filter capacitor can reduce peak currents drawn from the battery and improve efficiency. Low-ESR aluminum electrolytic capacitors are acceptable in some applications but standard aluminum electrolytic capacitors are not recommended.

Designers should add LC pi filters, linear post-regulators, or shielding in applications necessary to address excessive noise, voltage ripple, or EMI concerns. The LC pi filter's cutoff frequency should be at least a decade or two below the DC-DC converters's switching frequency for the specified load and input voltage.

A small SOT23-5pin 200mA Low Drop Out linear regulator can be used at the SP6644/6645 output to reduce output noise and ripple. The schematic in figure 29 illustrates this circuit with the SP6644 3.3V output followed by the Sipex SP6201 3.0V output Low Drop Out linear regulator. Compare in Figure 21 the SP6644 ripple of 40-50mVpp with the SP6201 ripple of about 3mVpp and you can see the amount of noise reduction obtained. Additional performance characteristics for the SP6644/6201 combination can be seen in figures 17 to 20.

Inductance ( $\mu$ H)	Manufacturer/Part No.	Inductor Specification	
		Resistance (ohms)	Isat (mA)
22	Sumida CD43-220	0.38 (max)	680
	Sumida CDRH5D18-220	0.28 (max)	760
	Coilcraft DO1608C-223	0.32 (typ)	700
47	Sumida CD43-470	0.84 (max)	440
	Coilcraft DO1608C-473	0.56 (typ)	500
100	Sumida CD54-101	0.7 (max)	520
	Coilcraft DO1608C-104	1.1 (typ)	310

**Table 1. Surface-Mount Inductor Information**

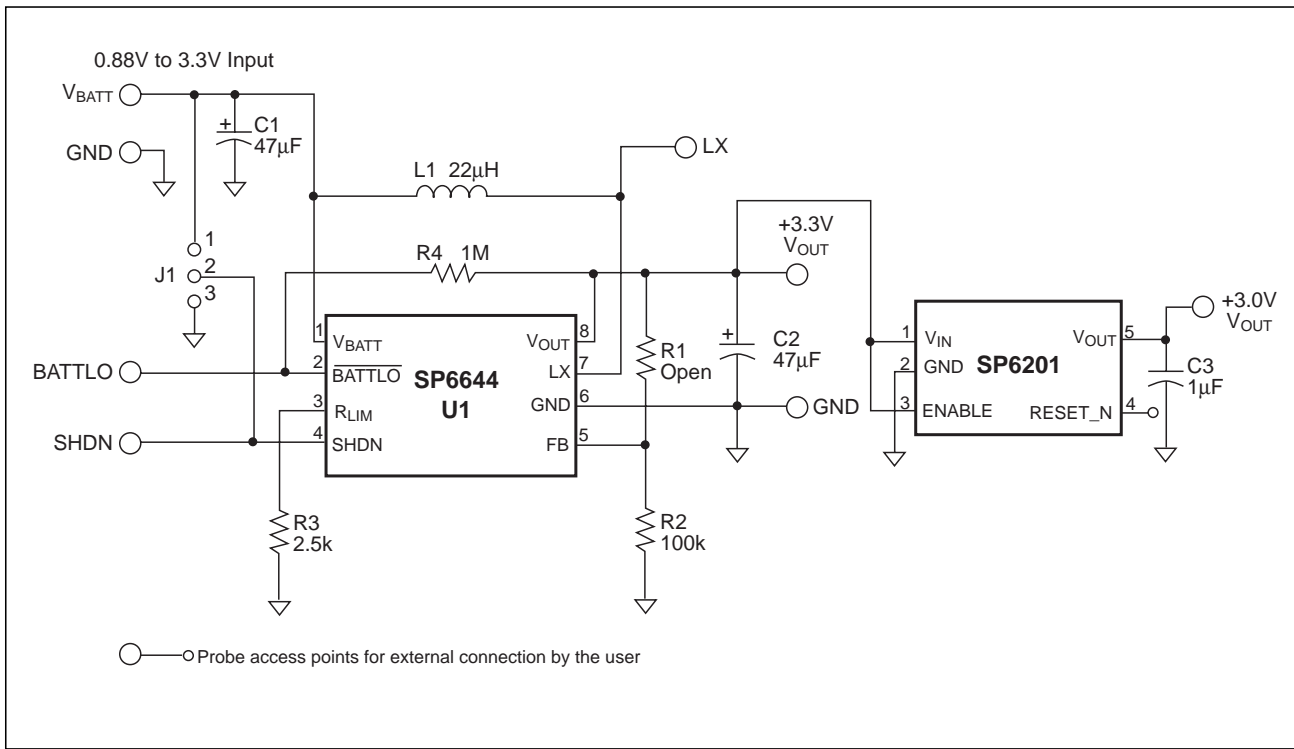
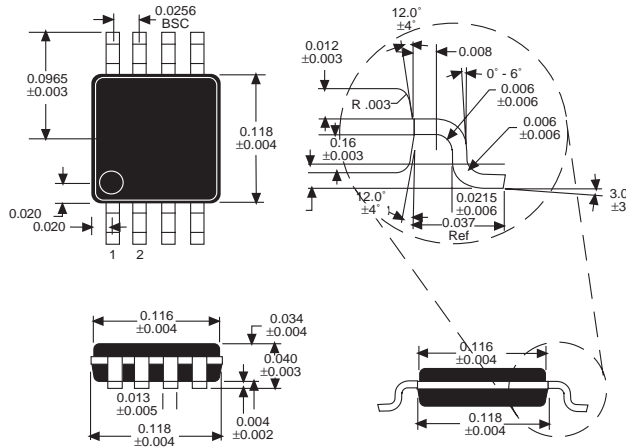
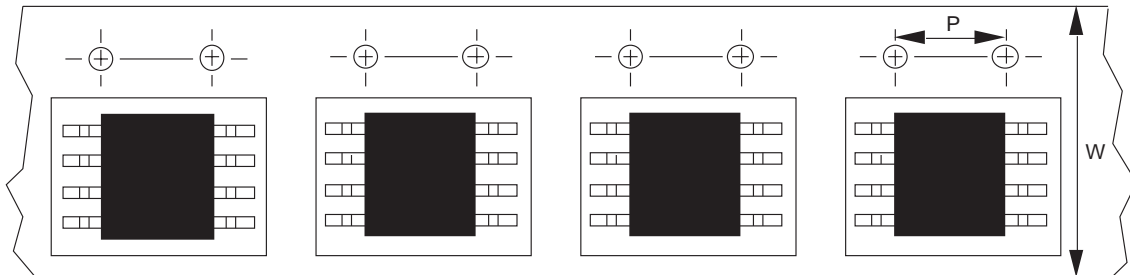


Figure 29. Schematic SP6644/6201 DC/DC LDO Combination

All package dimensions in inches



50  $\mu$ SOIC devices per tube



**8-pin  $\mu$ SOIC 13" reels: P = 8mm, W = 12mm**

pkg	min qty per reel	std qty per reel	max qty per reel
EU	500	2500	3000

## ORDERING INFORMATION

Model	Temperature Range	Package Type
SP6644EU .....	-40°C to +85°C .....	8-Pin $\mu$ SOIC
SP6645EU .....	-40°C to +85°C .....	8-Pin $\mu$ SOIC

Please consult the factory for pricing and availability on a Tape-On-Reel option.



SIGNAL PROCESSING EXCELLENCE

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