

# LM2743

## N-Channel FET Synchronous Buck Regulator Controller for Conversion from 3.3V

### General Description

The LM2743 is a high-speed, N-Channel synchronous buck regulator controller with a 2%, 0.6V feedback reference voltage intended to make down conversion from 3.3V to as low as 0.6V easy. A fixed-frequency voltage-mode PWM control architecture is used, that is adjustable from 50kHz to 2MHz through an external resistor. This wide range of PWM frequencies gives the power supply designer the flexibility to make tradeoffs among component size, cost, noise and efficiency. The power MOSFETs can run on a separate 1V to 16V (Input Voltage,  $V_{IN}$ ) (Note 2) rail while the regulator is biased from a 3V to 6V (IC Input Voltage,  $V_{CC}$ ), 2mA rail. A power-good flag, precision shutdown threshold and soft start features make power supply tracking and sequencing easy. The LM2743 employs output under-voltage and over-voltage flag, and current limit. Current limit is achieved by monitoring the voltage drop across the on resistance of the low-side MOSFET. The adaptive non-overlapping MOSFET gate drivers help avoid potential shoot-through problems while maintaining high efficiency. Both high-side and low-side MOSFETs are the lower cost N-Channel type, and the IC can accept a bootstrap structure to saturate the high-side MOSFET for highest efficiency.

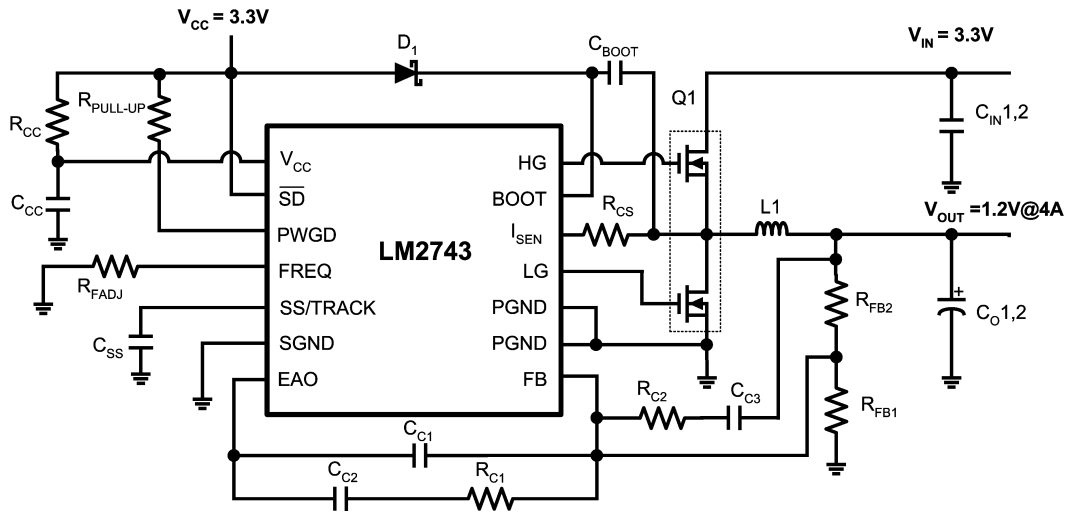
### Features

- MOSFET input voltage ( $V_{IN}$ ) from 1V to 16V (Note 2)
- IC input voltage ( $V_{CC}$ ) from 3V to 6V
- Output voltage adjustable down to 0.6V
- Power good flag and output enable
- Output over-voltage and under-voltage flag
- FB voltage: 2% over temperature
- Current limit without series sense resistor
- Adjustable soft start
- Tracking and sequencing with shutdown and soft start pins
- Switching frequency from 50 kHz to 2 MHz
- TSSOP-14 package

### Applications

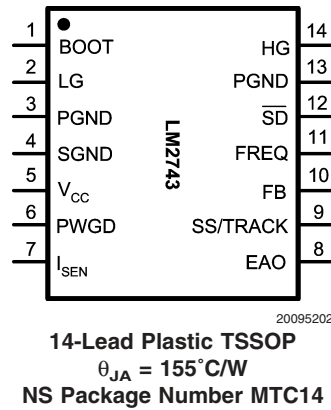
- 3.3V Buck Regulation
- Set-Top Boxes/ Home Gateways
- Core Logic Regulators
- High-Efficiency Buck Regulation

### Typical Application



20095201

## Connection Diagram



## Pin Description

**BOOT (Pin 1)** - Supply rail for the N-channel MOSFET gate drive. The voltage should be at least one gate threshold ( $V_{GS(th)}$ ) above the regulator input voltage ( $V_{IN}$ ) to properly turn on the high-side FET.

**LG (Pin 2)** - Gate drive for the low-side N-channel MOSFET. This signal is interlocked with HG (Pin 14) to avoid a shoot-through problem.

**PGND (Pins 3, 13)** - Ground for low-side FET drive circuitry. Connect to system ground.

**SGND (Pin 4)** - Ground for signal level circuitry. Connect to system ground.

**V<sub>CC</sub> (Pin 5)** Supply rail for the controller.

**PWGD (Pin 6)** - Power good pin. This is an open drain output. The pin is pulled low when the chip is in under-voltage flag (UVF), over-voltage flag (OVF), or UVLO mode. During normal operation, this pin is connected to  $V_{CC}$  or other low voltage source through a pull-up resistor ( $R_{PULL-UP}$ ).

**I<sub>SEN</sub> (Pin 7)** - Current limit threshold setting. This sources a fixed 40 $\mu\text{A}$  current. A resistor of appropriate value should be connected between this pin and the drain of the low-side FET.

**EAO (Pin 8)** - Output of the error amplifier. The voltage level on this pin is compared with an internally generated ramp signal to determine the duty cycle. This pin is necessary for compensating the control loop.

**SS (Pin 9)** - Soft start and track pin. A 10  $\mu\text{A}$  current is sourced from this pin. This pin is connected to the non-inverting input of the error amplifier during soft start, or any time the voltage is below the reference. To track power supplies connect a resistor divider (smaller than 10k $\Omega$  for better precision) from the output of the master supply directly to the SS pin. To limit the inrush current of a single power supply, place a capacitor to ground (see Application Information/Start Up for appropriate capacitance value). This pin should not be forced before  $\overline{\text{SD}}$  or  $V_{CC}$  (above the UVLO).

**FB (Pin 10)** - This is the inverting input of the error amplifier, which is used for sensing the output voltage and compensating the control loop. The FB current is negligible.

**FREQ (Pin 11)** - The switching frequency ( $F_{OSC}$ ) is set by connecting a resistor ( $R_{FADJ}$ ) between this pin and ground.

**$\overline{\text{SD}}$  (Pin 12)** - IC shutdown pin. To assure proper IC start-up the  $\overline{\text{SD}}$  pin should not be left floating. When this pin is pulled low the chip turns both, high and low, sides off. While this pin is low, the IC will not start up. This pin features a precision threshold for power supply sequencing, as well as a lower threshold to ensure minimal quiescent current.

**HG (Pin 14)** - Gate drive for the high-side N-channel MOSFET. This signal is interlocked with LG (Pin 2) to avoid a shoot-through problem.

**Absolute Maximum Ratings** (Note 1)

If Military/Aerospace specified devices are required, please contact the National Semiconductor Sales Office/Distributors for availability and specifications.

$V_{CC}$	7V
BOOT Voltage	21V
All other pins	$V_{CC} + 0.3V$
Junction Temperature	150°C
Storage Temperature	-65°C to 150°C
Soldering Information	

Lead Temperature (soldering, 10sec)	260°C
Infrared or Convection (20sec)	235°C
ESD Rating (Note 3)	2 kV

**Operating Ratings**

IC Input Voltage ( $V_{CC}$ )	3V to 6V
Junction Temperature Range	-40°C to +125°C
Thermal Resistance ( $\theta_{JA}$ )	155°C/W

**Electrical Characteristics**

$V_{CC} = 3.3V$  unless otherwise indicated. Typical and limits appearing in plain type apply for  $T_A = T_J = +25^\circ C$ . Limits appearing in boldface type apply over full Operating Temperature Range. Datasheet min/max specification limits are guaranteed by design, test, or statistical analysis.

Symbol	Parameter	Conditions	Min	Typ	Max	Units
$V_{FB}$	FB Pin Voltage	$V_{CC} = 3.3V$	<b>0.612</b>	0.6	<b>0.588</b>	V
		$V_{CC} = 5V$	<b>0.612</b>	0.6	<b>0.588</b>	
$V_{ON}$	UVLO Thresholds	Rising		2.76		V
		Falling		2.42		
$I_{Q\_VCC}$	Operating $V_{CC}$ Current	$V_{CC} = 3.3V$ , SD = 3.3V Fsw = 600kHz	<b>1</b>	1.5	<b>2.1</b>	mA
		$V_{CC} = 5V$ , SD = 3.3V Fsw = 600kHz	<b>1</b>	1.7	<b>2.1</b>	
	Shutdown $V_{CC}$ Current (Note 4)	$V_{CC} = 3.3V$ , SD = 0V	0	110	185	$\mu A$
$t_{PWGD1}$	PWGD Pin Response Time	FB Voltage Going Up		6		$\mu s$
$t_{PWGD2}$	PWGD Pin Response Time	FB Voltage Going Down		6		$\mu s$
$I_{SS-ON}$	SS Pin Source Current	SS Voltage = 0V	<b>7</b>	10	<b>14</b>	$\mu A$
$I_{SS-OC}$	SS Pin Sink Current During Over Current	SS Voltage = 0V		90		$\mu A$
$I_{SEN-TH}$	$I_{SEN}$ Pin Source Current Trip Point		<b>25</b>	40	<b>55</b>	$\mu A$

**ERROR AMPLIFIER**

GBW	Error Amplifier Unity Gain Bandwidth			9		MHz
G	Error Amplifier DC Gain			106		dB
SR	Error Amplifier Slew Rate			3.2		V/ $\mu s$
$I_{EAO}$	EAO Pin Current Sourcing and Sinking Capability	$V_{EAO} = 1.5$ , FB = 0.55V		2.6		mA
		$V_{EAO} = 1.5$ , FB = 0.65V		9.2		
$V_{EA}$	Error Amplifier Maximum Swing	Minimum		0		V
		Maximum		2		

## Electrical Characteristics (Continued)

$V_{CC} = 3.3V$  unless otherwise indicated. Typical and limits appearing in plain type apply for  $T_A = T_J = +25^\circ C$ . Limits appearing in boldface type apply over full Operating Temperature Range. Datasheet min/max specification limits are guaranteed by design, test, or statistical analysis.

Symbol	Parameter	Conditions	Min	Typ	Max	Units
<b>GATE DRIVE</b>						
$I_{Q-BOOT}$	BOOT Pin Quiescent Current	BOOTV = 12V, EN = 0		18	<b>90</b>	$\mu A$
$R_{DS1}$	Top FET Driver Pull-Up ON resistance	BOOT-SW = 5V@350mA		3		$\Omega$
$R_{DS2}$	Top FET Driver Pull-Down ON resistance			2		$\Omega$
$R_{DS3}$	Bottom FET Driver Pull-Up ON resistance			3		$\Omega$
$R_{DS4}$	Bottom FET Driver Pull-Down ON resistance			2		$\Omega$
<b>OSCILLATOR</b>						
$F_{OSC}$	PWM Frequency	$R_{FADJ} = 813.2k\Omega$		50		kHz
		$R_{FADJ} = 117.6k\Omega$		300		
		$R_{FADJ} = 54.4k\Omega$	<b>475</b>	600	<b>725</b>	
		$R_{FADJ} = 18.8k\Omega$		1400		
		$R_{FADJ} = 10.8k\Omega$		2000		
D	Max Duty Cycle	$f_{PWM} = 300kHz$ $f_{PWM} = 600kHz$		90 85		%
<b>LOGIC INPUTS AND OUTPUTS</b>						
$V_{STBY-IH}$	Standby High Trip Point	FB = 0.575V, BOOTV = 3.3V, EN = 0V to 3.3V		0.756	<b>1.1</b>	V
$V_{STBY-IL}$	Standby Low Trip Point	FB = 0.575V, BOOTV = 3.3V, EN = 3.3V to 0V	<b>0.232</b>	0.562		V
$V_{SD-IH}$	$\overline{SD}$ Pin Logic High Trip Point	FB = 0.575V, BOOTV = 3.3V, EN = 0V to 3.3V		1	<b>1.3</b>	V
$V_{SD-IL}$	$\overline{SD}$ Pin Logic Low Trip Point	FB = 0.575V, BOOTV = 3.3V, EN = 3.3V to 0V	<b>0.8</b>	1.1		V
$V_{PWGD-TH-LO}$	PWGD Pin Trip Points	FB Voltage Going Down	<b>0.408</b>	0.434	<b>0.457</b>	V
$V_{PWGD-TH-HI}$	PWGD Pin Trip Points	FB Voltage Going Up	<b>0.677</b>	0.710	<b>0.742</b>	V
$V_{PWGD-HYS}$	PWGD Hysteresis	FB Voltage Going Down FB Voltage Going Up		60 90		mV

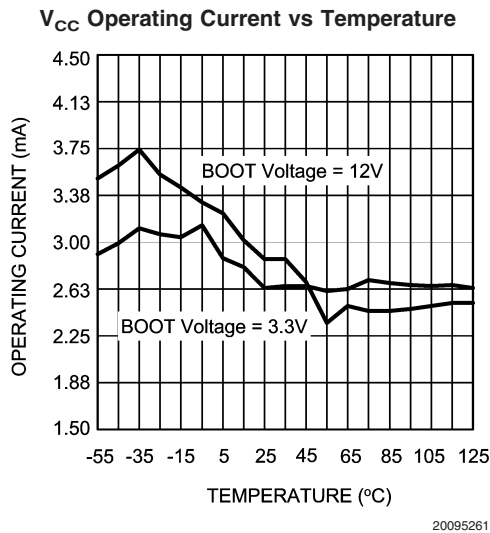
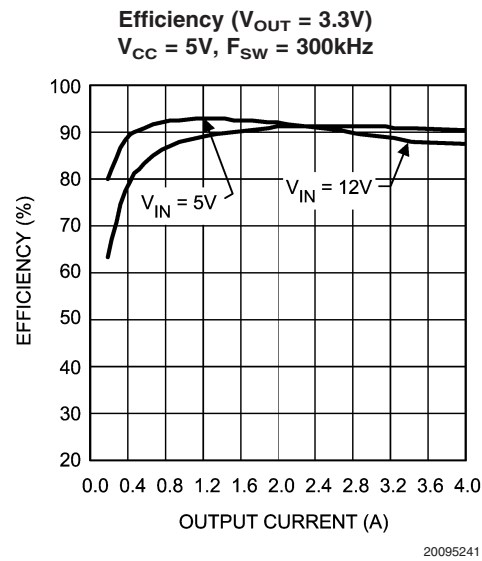
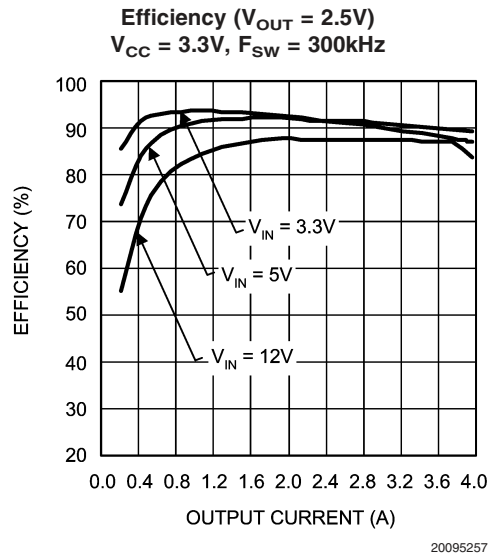
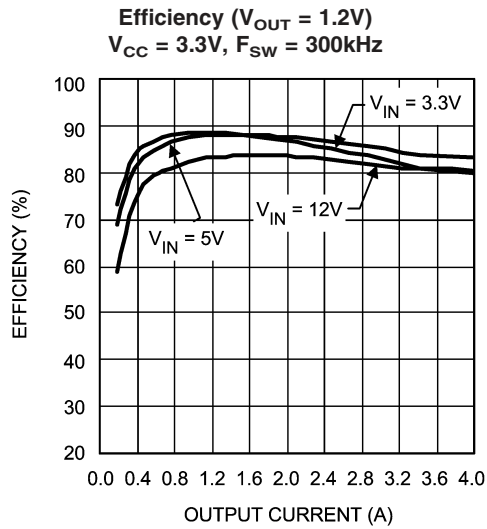
**Note 1:** Absolute maximum ratings indicate limits beyond which damage to the device may occur. **Operating ratings** indicate conditions for which the device operates correctly. **Operating Ratings** do not imply guaranteed performance limits.

**Note 2:** The power MOSFETs can run on a separate 1V to 16V rail (Input voltage,  $V_{IN}$ ). Low range of  $V_{IN}$  greatly depends on selection of the external MOSFET.

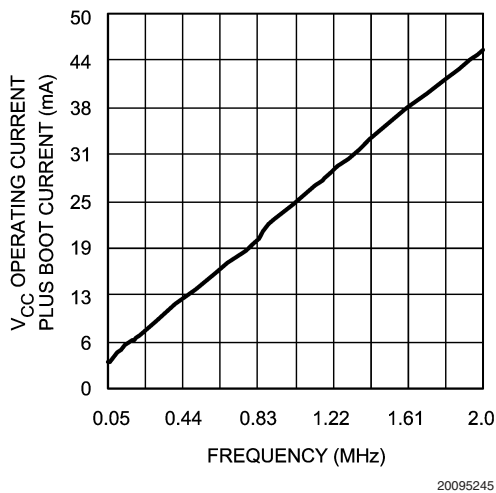
**Note 3:** The human body model is a 100pF capacitor discharged through a 1.5k resistor into each pin.

**Note 4:** Shutdown  $V_{CC}$  current goes to zero amps after 20 seconds.

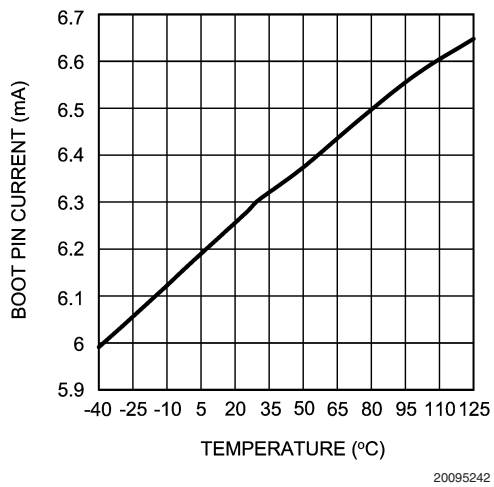
# Typical Performance Characteristics



**$V_{CC}$  Operating Current plus BOOT Current vs Frequency**  
**FDS689A FET ( $T_A = 25^\circ C$ )**

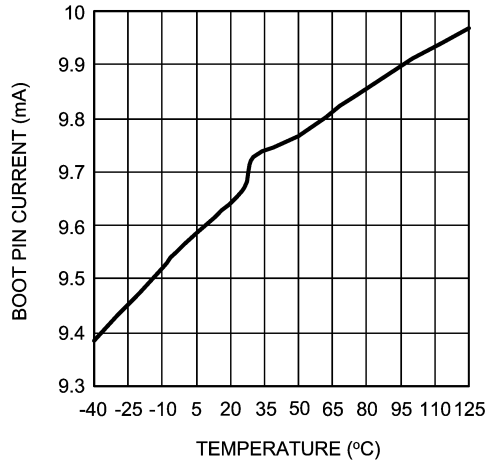


**BOOT Pin Current vs Temperature for**  
**BOOT Voltage = 3.3V**  
 $F_{SW} = 300kHz, FDS689A FET, No-Load$



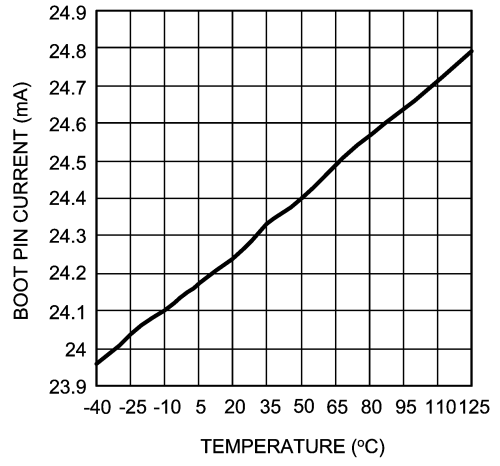
# Typical Performance Characteristics (Continued)

**BOOT Pin Current vs Temperature for  
BOOT Voltage = 5V**  
F<sub>SW</sub> = 300kHz, FDS689A FET, No-Load



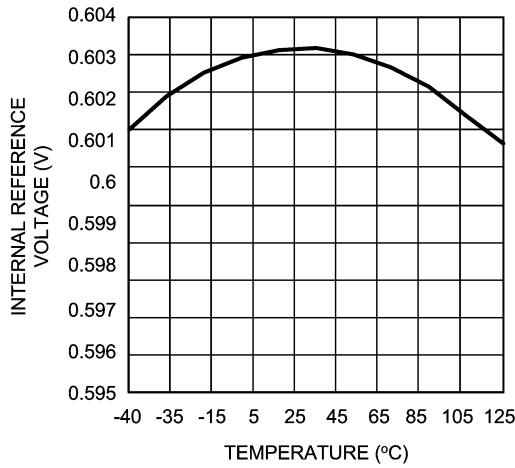
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**BOOT Pin Current vs Temperature for  
BOOT Voltage = 12V**  
F<sub>SW</sub> = 300kHz, FDS689A FET, No-Load



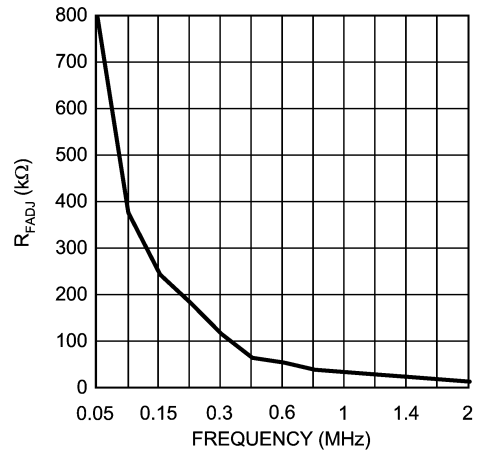
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**Internal Reference Voltage vs Temperature**



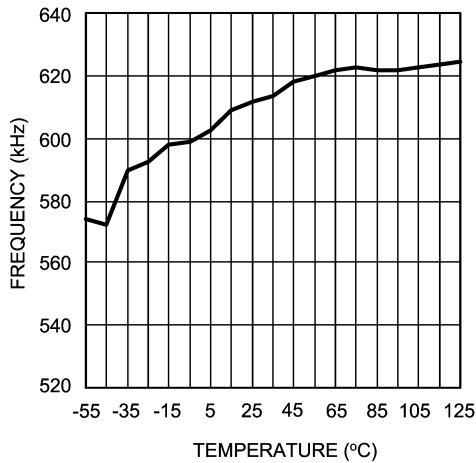
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**R<sub>FADJ</sub> vs Frequency**  
50kHz to 2MHz, T<sub>A</sub> = 25°C



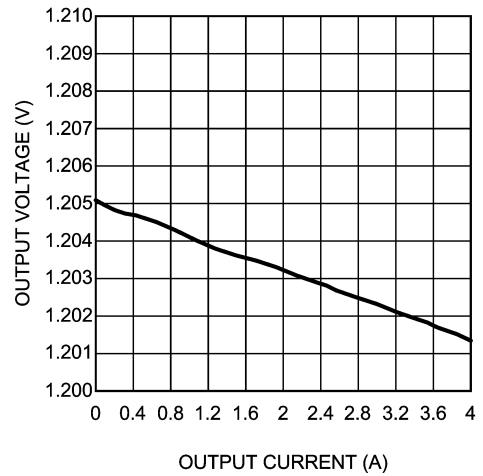
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**Frequency vs Temperature**



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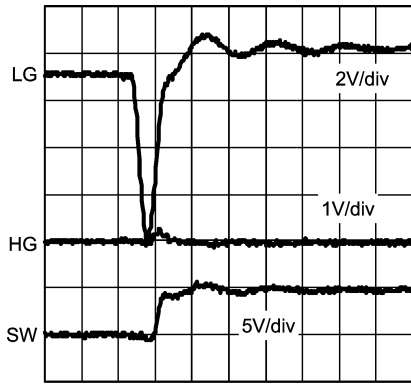
**Output Voltage vs Output Current**



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Typical Performance Characteristics (Continued)

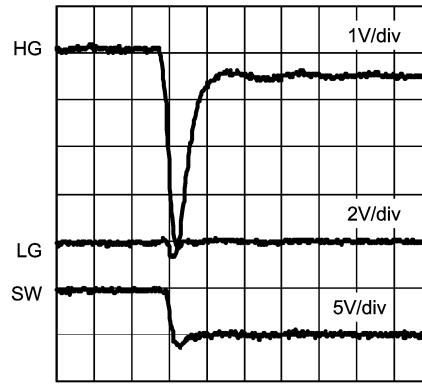
**Switch Waveforms (HG Rising)**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $I_{OUT} = 4A, C_{SS} = 12nF, F_{SW} = 300kHz$



100 ns/DIV

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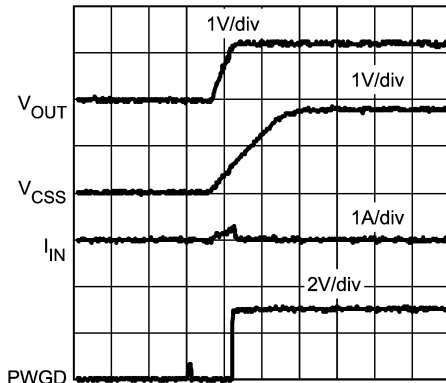
**Switch Waveforms (HG Falling)**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $I_{OUT} = 4A, C_{SS} = 12nF, F_{SW} = 300kHz$



100 ns/DIV

20095247

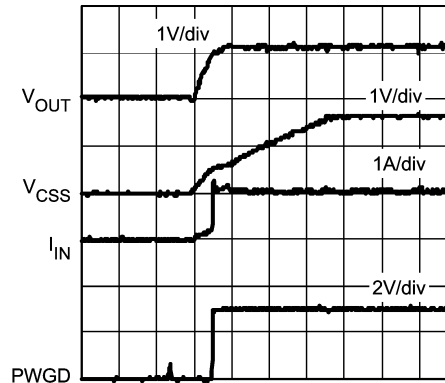
**Start-Up (No-Load)**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $I_{OUT} = 4A, C_{SS} = 12nF, F_{SW} = 300kHz$



1 ms/DIV

20095248

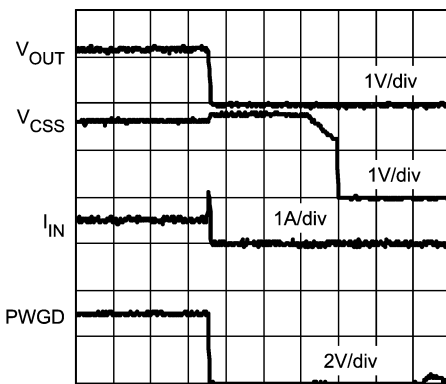
**Start-Up (Full-Load)**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $I_{OUT} = 4A, C_{SS} = 12nF, F_{SW} = 300kHz$



1 ms/DIV

20095249

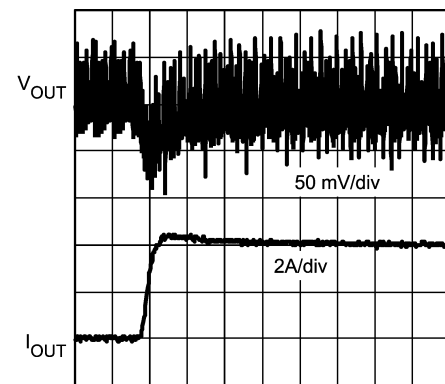
**Shutdown (Full-Load)**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $I_{OUT} = 4A, C_{SS} = 12nF, F_{SW} = 300kHz$



1 ms/DIV

20095250

**Load Transient Response ( $I_{OUT} = 0A$  to  $4A$ )**  
 $V_{CC} = 3.3V, V_{IN} = 5V, V_{OUT} = 1.2V$   
 $C_{SS} = 12nF, F_{SW} = 300kHz$



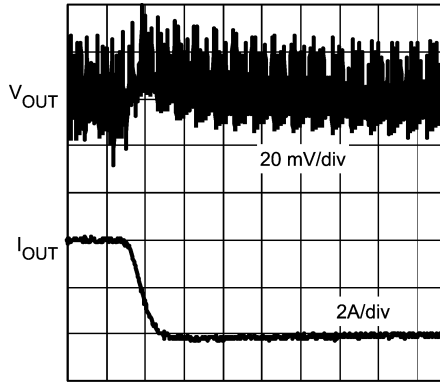
40 μs/DIV

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# Typical Performance Characteristics (Continued)

**Load Transient Response ( $I_{OUT} = 4A$  to  $0A$ )**

$V_{CC} = 3.3V$ ,  $V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$   
 $C_{SS} = 12nF$ ,  $F_{SW} = 300kHz$

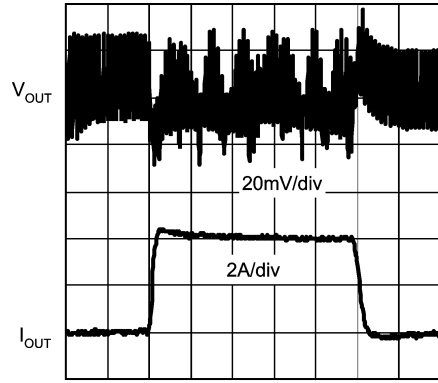


40  $\mu s$ /DIV

20095252

**Load Transient Response**

$V_{CC} = 3.3V$ ,  $V_{IN} = 5V$ ,  $V_{OUT} = 1.2V$   
 $C_{SS} = 12nF$ ,  $F_{SW} = 300kHz$

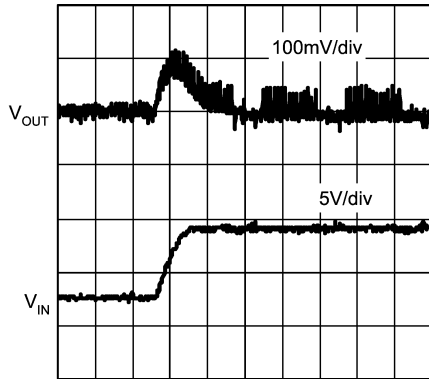


100  $\mu s$ /DIV

20095253

**Line Transient Response ( $V_{IN} = 3V$  to  $6V$ )**

$V_{CC} = 3.3V$ ,  $V_{OUT} = 1.2V$   
 $I_{OUT} = 2A$ ,  $F_{SW} = 300kHz$

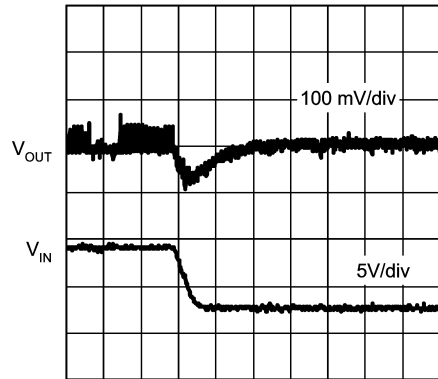


100  $\mu s$ /DIV

20095254

**Line Transient Response ( $V_{IN} = 6V$  to  $3V$ )**

$V_{CC} = 3.3V$ ,  $V_{OUT} = 1.2V$   
 $I_{OUT} = 2A$ ,  $F_{SW} = 300kHz$

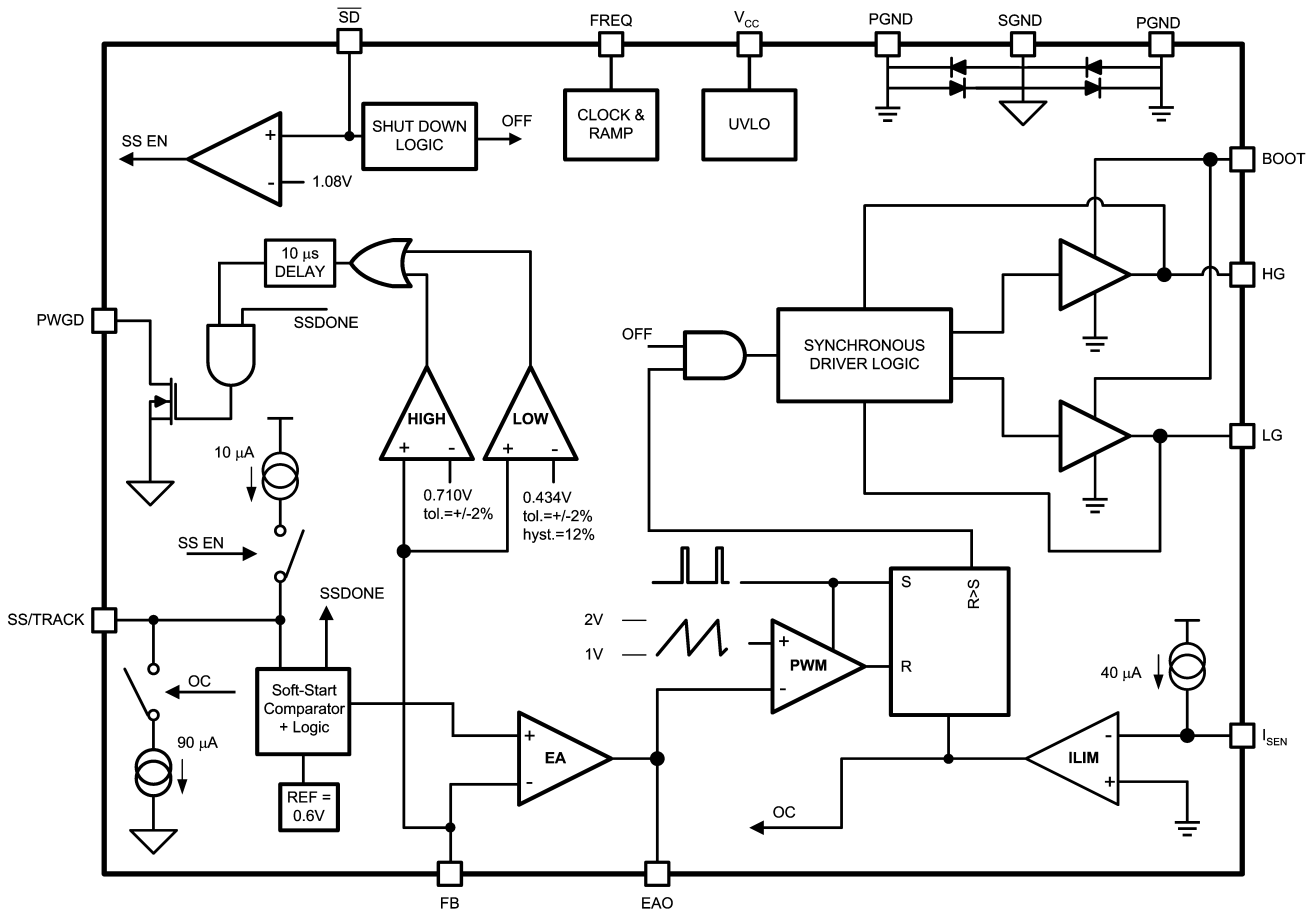


100  $\mu s$ /DIV

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## Block Diagram



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## Application Information

### THEORY OF OPERATION

The LM2743 is a voltage-mode, high-speed synchronous buck regulator with a PWM control scheme. It is designed for use in set-top boxes, thin clients, DSL/Cable modems, and other applications that require high efficiency buck converters. It has power good (PWGD) flag, output shutdown ( $\overline{SD}$ ), UVLO mode, and over-voltage flag (OVF) and under-voltage flag (UVF) features. The over-voltage and under-voltage signals are OR gated to drive the power good signal. If this signal is pulled low, the high side is off and low side if on, but only if the duty cycle is less than maximum. Current limit is achieved by sensing the voltage  $V_{DS}$  across the low side FET. During current limit the high side gate is turned off and the low side gate is turned on. A  $90\mu\text{A}$  source discharges the soft start capacitor (reducing max. duty cycle) until the current is under control.

### START UP

When  $V_{CC}$  exceeds 2.76V and the shutdown pin ( $\overline{SD}$ ) sees a logic high, the internal fixed  $10\mu\text{A}$  source begins charging the soft start capacitor. During this time the output of the error amplifier is allowed to rise with the voltage of the soft start capacitor. This capacitor,  $C_{SS}$ , determines soft start time, and can be calculated approximately by:

$$C_{SS} = \frac{t_{SS}}{4 \times 10^4}$$

During soft start the power good flag is forced low and it is released when the voltage reaches a set value as shown in *Figure 1*. At this point the chip enters normal operation mode, the power good flag is released, and the OVF and UVF functions begin to monitor  $V_{OUT}$ .

## Application Information (Continued)

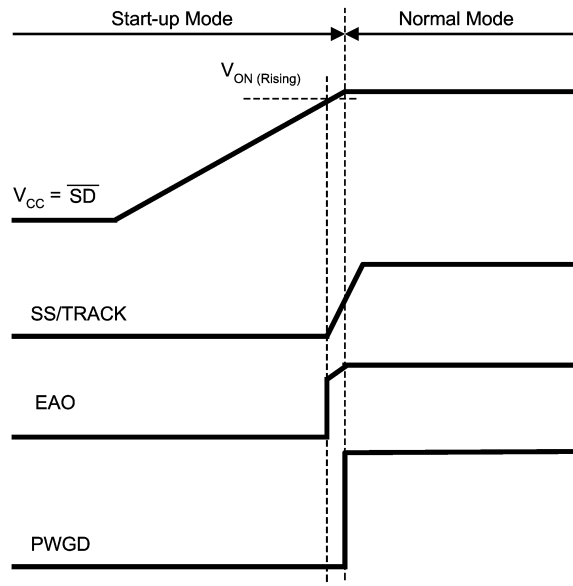


FIGURE 1. Start-Up Behavior

### NORMAL OPERATION

While in normal operation mode, the LM2743 regulates the output voltage by controlling the duty cycle of the high side and low side FETs.

The equation governing output voltage is:

$$0.6 = \frac{R_{FB1}}{R_{FB1} + R_{FB2}} V_{OUT}$$

The PWM frequency is adjustable between 50kHz and 2MHz and is set by an external resistor,  $R_{FADJ}$ , between the FREQ pin and ground. The resistance needed for a desired frequency is approximately:

$$R_{FADJ} = 10^{12} a_2 \left( \frac{1}{F_{OSC} \text{ (Hz)}} \right)^2 + 10^7 a_1 \left( \frac{1}{F_{OSC} \text{ (Hz)}} \right) + 10^2 a_0 \text{ [k}\Omega\text{]}$$

where  $a_2 = 0.206375$ ,  $a_1 = 3.691525$ ,  $a_0 = (-0.076875)$  are the coefficients,  $F_{OSC}$  is the frequency in Hz, and  $R_{FADJ}$  is the resistance in  $k\Omega$ .

### SS/TRACK

When the LM2743 is used for sequencing purposes, some care has to be taken. Once the shutdown voltage goes above  $V_{STBY-IH}$ , a  $17\mu A$  pull-up current is activated as shown in Figure 2. This current is used to create an internal hysteresis (170mV); however, high external impedances will affect the  $\overline{SD}$  pin level as well. The external impedance must be lower than  $10k\Omega$  to work properly without glitching the quiescent current of the chip. In that scenario the SS current will turn on and off during the glitching or most likely no switching will occur at all, due to the SS voltage being very low.

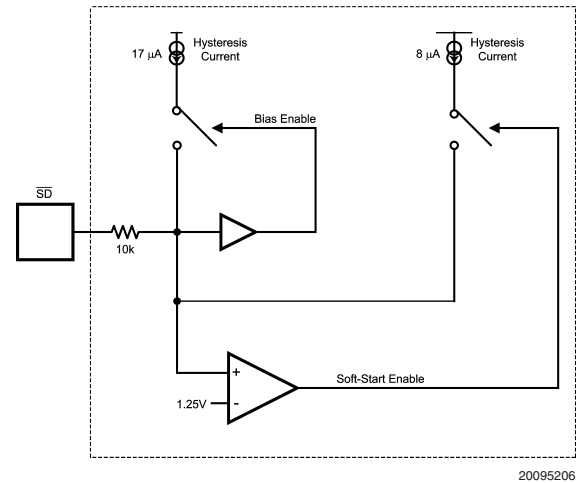


FIGURE 2.  $\overline{SD}$  Pin Logic

The LM2743 is also adequate for tracking purposes through the SS/TRACK pin. The tracking circuit, in the design examples below, contains a Master Power Supply with  $V_{OUT1} = 5V$  and an LM2743 with  $V_{OUT2} = 1.8V$ .

Three cases are described:

1. Both output voltages,  $V_{OUT1}$  and  $V_{OUT2}$ , rise together, reaching their final values at the same time,
2. Both output voltages rise together at the same rate until  $V_{OUT2} = 1.8V$ , and finally
3. Output voltage  $V_{OUT2}$  starts rising 3.24ms after  $V_{OUT1}$  starts.

The calculation of the feedback resistors Figure 3 for all cases is based on the Tracking Equation. Since  $V_{FB} = 0.6V$ ,  $V_{OUT2} = 1.8V$ , and  $R_{FB2} = 10k\Omega$ , then the  $R_{FB1}$  becomes  $5k\Omega$ .

### Case 1: Rise together

Both,  $V_{OUT1}$  and  $V_{OUT2}$ , start rising, and reach their nominal values at the same time as shown in Figure 4. This means that  $V_{OUT2}$  rises at slower rate than  $V_{OUT1}$ .

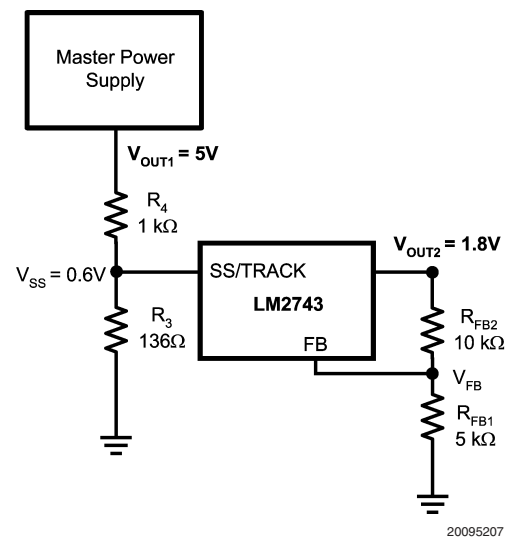


FIGURE 3. Block Diagram of Case 1

$$V_{SS} = V_{OUT1} * (R_3 / (R_3 + R_4))$$

## Application Information (Continued)

$$V_{FB} = V_{OUT2} * (R_{FB2} / (R_{FB1} + R_{FB2}))$$

Since  $V_{SS} = V_{FB} = 0.6V$ , then

### Tracking Equation

$$V_{OUT2} = V_{OUT1} * \frac{R_3}{R_3 + R_4} * \frac{R_{FB1} + R_{FB2}}{R_{FB2}}$$

The total value of the track resistor divider (Figure 3),  $R_3$  and  $R_4$ , should be set below  $10k\Omega$  for better precision. Let  $R_4 = 1K$ , for  $V_{OUT1} = 5V$  and  $V_{OUT2} = 1.8V$ ,  $R_3 = 136\Omega$ .

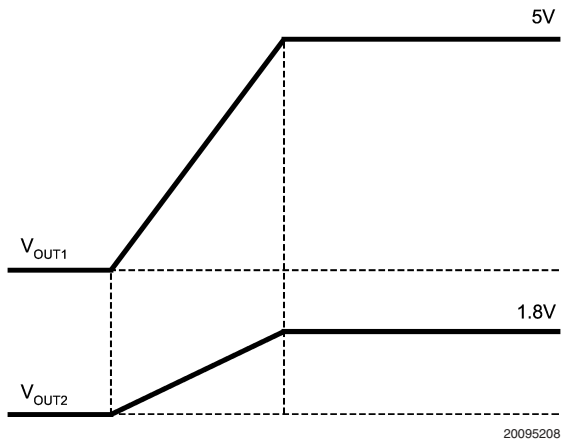


FIGURE 4. Timing Behavior of Case 1

### Case 2: Rise together until $V_{OUT2} = 1.8V$

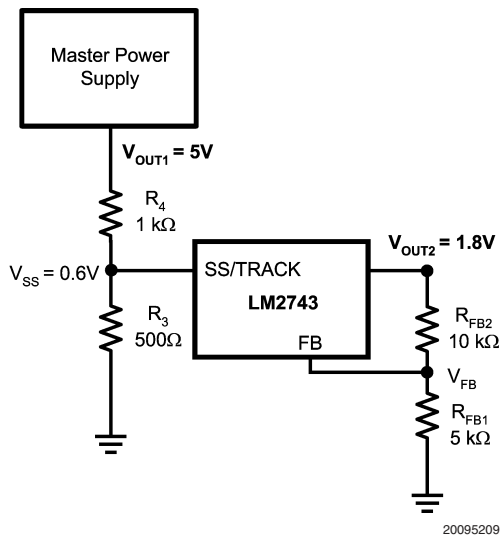


FIGURE 5. Block Diagram of Case 2

$$V_{SS} = V_{FB} = 0.6V,$$

$$V_{OUT1} = V_{OUT2} = 1.8V$$

For  $R_4 = 1k\Omega$ ,  $R_3 = 500\Omega$  (from Tracking Equation).

The soft start reaches 0.6V at  $V_{OUT1}$  equal 1.8V.

For  $V_{OUT1} > 1.8V$ ,  $V_{OUT2}$  stays in regulation at 1.8V.

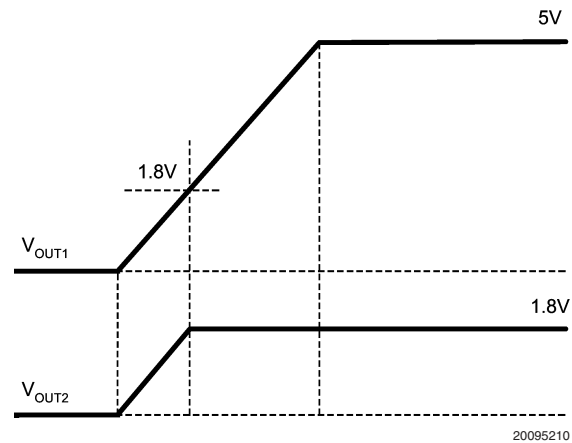


FIGURE 6. Timing Behavior of Case 2

### Case 3: $V_{OUT2}$ starts rising 3.0ms after $V_{OUT1}$

Assuming  $V_{OUT1}$  slew rate  $SR_{VSD} = 1V/ms$  and voltage divider ratio 1:3 ( $R_3 = 500\Omega$  and  $R_4 = 1k\Omega$ ), the  $V_{SD}$  slew rate equals  $SR_{VSD} = 0.333V/ms$ . During the delay time  $V_{SD}$  raises to 1.0V ( $V_{SD-IH}$ ) as shown in Figure 8. The delay time is calculated from:

$$t_{DELAY} = V_{SD-IH}^- / SR_{VSD}$$

$$t_{DELAY} = 1.0(V) / 0.333(V/ms) = 3.0ms$$

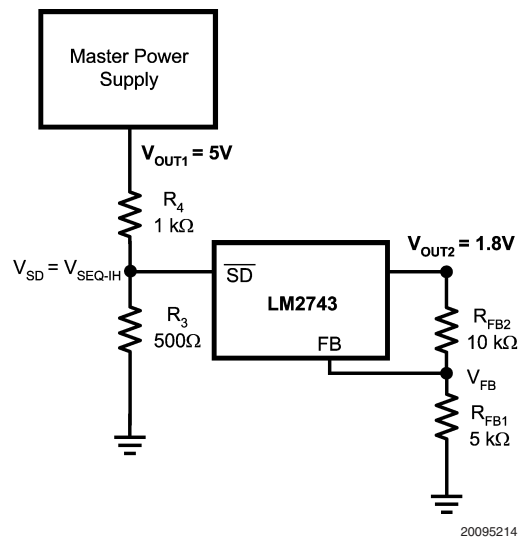
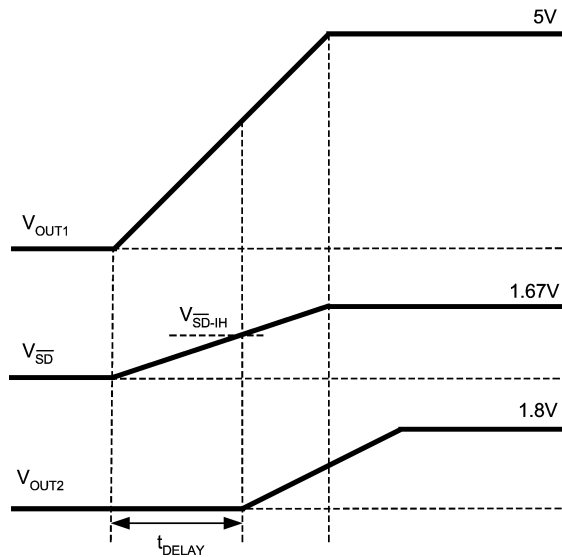


FIGURE 7. Block Diagram of Case 3

## Application Information (Continued)



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**FIGURE 8. Timing Behavior of Case 3**

If the tracking through SS/TRACK pin is not used, a capacitor to ground is needed to limit the inrush current.

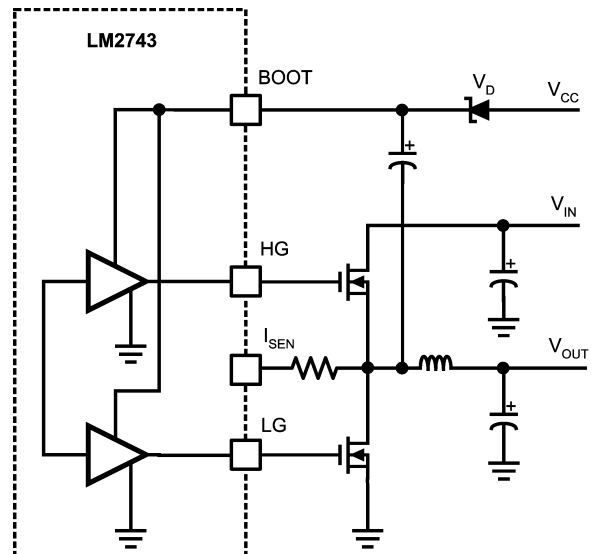
### MOSFET GATE DRIVERS

The LM2743 has two gate drivers designed for driving N-channel MOSFETs in a synchronous mode. Power for the drivers is supplied through the BOOT pin. For the high side gate (HG), to fully turn the top FET on, the BOOT voltage must be at least one  $V_{GS(th)}$  greater than  $V_{IN}$  ( $V_{BOOT} \geq 2V + V_{IN}$ ). This voltage can be supplied from a separate voltage source or from a local charge pump structure, the bootstrap.

A charge pump can be built using a diodes and small capacitors, as shown in the below figures. The capacitor serves to maintain enough voltage between the top FET gate and source to control the device even when the top FET is on and its source has risen up to the input voltage level.

The LM2743 gate drives use a BiCMOS design. Unlike some other bipolar control ICs, the gate drivers have rail-to-rail swing, ensuring no spurious turn-on due to capacitive coupling.

The LM2743 can operate its internal circuitry at the  $V_{CC}$  range from 3.0V to 6.0V. However, the external FETs may operate more efficiently with higher gate drive voltage. *Figure 9* shows a typical bootstrap method where the voltage applied to the FETs is  $V_{CC} - V_D$ .

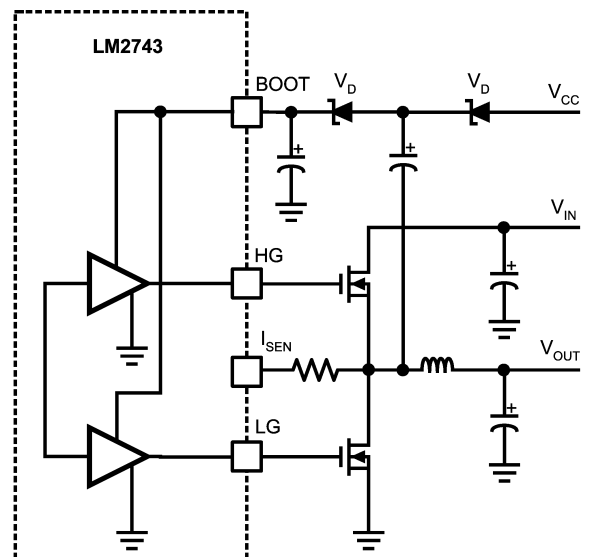


20095212

**FIGURE 9. Bootstrap Configuration 1**

This means that if  $V_{CC}$  is 3.0V, the gate drive for the FETs is approximately 2.5V. This voltage could be too low to fully turn the FET on. As a result  $I^2R$  losses could be higher than expected.

In the next bootstrap configuration (*Figure 10*) the voltage applied to the high side FET is  $V_{CC} - 2V_D$  and to the low side FET is  $V_{CC} - 2V_D + V_{IN}$ .



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**FIGURE 10. Bootstrap Configuration 2**

If  $V_{CC}$  and  $V_{IN}$  are both 3.0V, then 5V is developed at BOOT pin and the low side FET can be driven fully on. The high side FET however may have difficulty turning on since the applied gate drive is only 2V in this case.

The *Figure 11* shows next example of bootstrap configuration. In this case the low gate drive voltage on the top FET is resolved. Now the gate drive on both, the low and high, side FETs is  $V_{CC} - 3V_D + V_{IN}$ .

## Application Information (Continued)

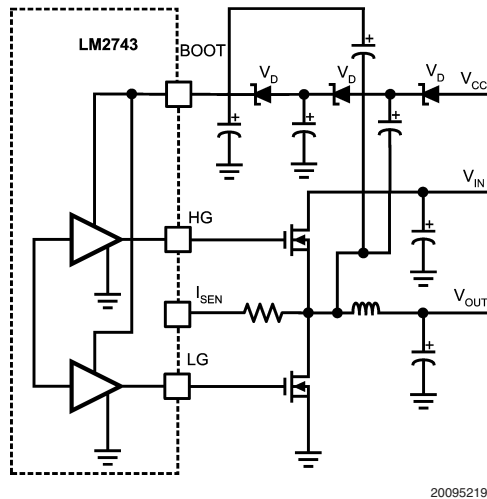


FIGURE 11. Bootstrap Configuration 3

At an input voltage of 3V both, the high and low, side FETs are driven with about 4.5V.

The decision on which configuration to use depends on the desired output current and operating frequency. At high currents and low frequencies, configuration 3 (Figure 11) is recommended. For low currents and high frequencies, configuration 1 (Figure 9) may work well.

### POWER GOOD SIGNAL

The power good signal is the OR-gated flag representing over-voltage and under-voltage conditions. If the feedback pin (FB) voltage is about 18% over its nominal value ( $V_{PWGD-TH-HI} = 0.710V$ ) or falls about 30% below its nominal value ( $V_{PWGD-TH-LO} = 0.434V$ ) the power good flag goes low. At about 118% of  $V_{FB}$  the converter turns off the high side gate and turns on the low side gate. However, at about 70% of  $V_{FB}$  the converter goes to maximum duty cycle and the high and low sides are still switching. The power good flag will return to logic high whenever the feedback pin voltage is between 70% and 118% of 0.6V.

### UVLO

The 2.76V turn-on threshold on  $V_{CC}$  has a built in hysteresis of 400mV. Therefore, if  $V_{CC}$  drops below 2.42V, the chip enters UVLO mode. UVLO consists of turning off the top and bottom FETs, and remaining in that condition until  $V_{CC}$  rises above 2.76V. As with shutdown, the soft start capacitor is discharged through a FET, ensuring that the next start-up will be smooth.

### CURRENT LIMIT

Current limit is realized by sensing the voltage across the low side FET while it is on. The  $R_{DS(ON)}$  of the FET is a known value, and the voltage across the FET can be found from:

$$V_{DS} = I_{DS} * R_{DS(ON)}$$

The current limit is determined by an external resistor,  $R_{CS}$ , connected between the switch node and the  $I_{SEN}$  pin. A constant current of 40 $\mu$ A is forced through  $R_{CS}$ , causing a fixed voltage drop. This fixed voltage is compared against

$V_{DS}$  and if the latter is higher, the current limit of the chip has been reached. The  $R_{CS}$  can be found by using the following:

$$R_{CS} = R_{DS(ONLOW)} (\Omega) \times \frac{I_{LIM}(A)}{40 \mu(A)}$$

where resistance  $R_{DS(ON)}$  is taken from MOSFET's datasheet ( $R_{DS(ON LOW)} = 13m\Omega$ ) and current limit ( $I_{LIM}$ ) value is calculated from equation.

$$I_{LIM} = I_{OUT} + 0.5 \frac{(V_{CC} - V_{OUT}) \times V_{OUT}}{L \times V_{CC} \times F_{OSC}}$$

where: L is the inductance and  $F_{OSC}$  is the PWM frequency. Because current sensing is done across the low side FET, no minimum high side on-time is necessary. In the current limit mode the LM2743 will turn the high side off and the keep low side on for a time as long as necessary. The chip also discharges the soft start capacitor through a fixed 90 $\mu$ A source. This way, smooth ramping up of the output voltage as with a normal soft start is ensured. The output of the LM2743 internal error amplifier is limited by the voltage on the soft start capacitor. Hence, discharging the soft start capacitor reduces the maximum duty cycle (D) of the controller. During severe current limit, this reduction in duty cycle will reduce the output voltage if the current limit conditions last for an extended period of time.

### UVF/OVF

The output under-voltage flag (UVF) and over-voltage flag (OVF) mechanisms engage at about 70% and 118% of the target output voltage, respectively. In the UVF case, the LM2743 will turn off the high side switch and turn on the low side switch and discharge the soft start capacitor through the MOSFET switch. However, in the OVF the converter goes to maximum duty cycle and the high and low sides are still switching. The chip remains in this state until the shutdown pin has been pulled to a logic low and then released. The UVF function is masked only during the initial charge of the soft start capacitor, when voltage is first applied to the  $V_{CC}$  pin. The power good flag goes low during this time, giving a logic-level warning signal.

### SHUT DOWN

To assure proper IC start-up, shutdown pin ( $\overline{SD}$ ) should not be left floating. For Normal Operation this pin should be connected to  $V_{CC}$  or other low voltage source (see Electrical Characteristics table).

If the shutdown pin  $\overline{SD}$  is pulled low, the LM2743 discharges the soft start capacitor through a MOSFET switch. The high and the low side switches are turned off. The LM2743 remains in this state until  $\overline{SD}$  is released.

### DESIGN CONSIDERATIONS

The following is a design procedure for all the components needed to create the Typical Application Circuit. The designed 3.3V ( $V_{CC}$ ) to 1.2V ( $V_{OUT}$ ) converter is capable of delivering 4A with an efficiency of 89% at switching frequency of 300kHz. The same procedures can be followed to create many other designs with varies input and output voltages, and load current.

## Application Information (Continued)

### Input Capacitor

The input capacitors in a Buck switching converter are subjected to high stress due to the input current square waveform. Hence input capacitors are selected for their ripple current capability and their ability to withstand the heat generated as that ripple current runs through their ESR. Input rms ripple current is approximately:

$$I_{\text{RMS\_RIP}} = I_{\text{OUT}} \times \sqrt{D(1-D)}$$

where D is the duty cycle.

The power dissipated by each input capacitor is:

$$P_{\text{CAP}} = \frac{(I_{\text{RMS\_RIP}})^2 \times \text{ESR}}{n^2}$$

where, n is the number of capacitors, and ESR is the equivalent series resistance of  $C_{\text{IN1}}$ .

The equation indicates that power loss in each capacitor decreases rapidly as the number of input capacitors increases. The worst-case ripple for a Buck converter occurs during full load and when the duty cycle (D) is 0.5. For design 3.3V ( $V_{\text{CC}}$ ) to 1.2V ( $V_{\text{OUT}}$ ) the duty cycle is 0.364. With a 4A maximum load the ripple current is around 2A. The Sanyo 20SP120M aluminum electrolytic capacitor works fine here. It has a ripple current rating of 3A and maximum ESR of 24m $\Omega$  at 100kHz. The power dissipated by the Sanyo's capacitor is then 0.088W. Other options for input and output capacitors include MLCC, Tantalum, OSCON, SP, and POSCAPS.

### Support Components: Capacitors ( $C_{\text{IN2}}$ , $C_{\text{CC}}$ , $C_{\text{BOOT}}$ , $C_{\text{SS}}$ ), Resistors ( $R_{\text{CC}}$ , $R_{\text{CS}}$ , $R_{\text{FADJ}}$ , $R_{\text{PULL-UP}}$ ), and Schottky Diode ( $D_1$ )

$C_{\text{IN2}}$  - the MOSFET's input capacitor is high frequency bypass device designed to filter harmonics of the switching frequency and input noise. 0.1 $\mu$ F - 1 $\mu$ F ceramic capacitor with a sufficient voltage rating will work well in almost any case.

$R_{\text{CC}}$ ,  $C_{\text{CC}}$ , and  $C_{\text{BOOT}}$  - bypass resistor and bypass capacitors are standard filter components designed to ensure smooth DC voltage for the chip supply and for the bootstrap structure, if it is used. Recommended values:  $R_{\text{CC}} = 10\Omega$ ,  $C_{\text{CC}} = 0.1\mu\text{F}$ , and  $C_{\text{BOOT}} = 0.1\mu\text{F}$ .

$R_{\text{PULL-UP}}$  - this is a standard pull-up resistor for the open-drain power good signal (PWGD). The recommended value: 100 $\Omega$ : connected to  $V_{\text{CC}}$ . If this feature is not necessary, the resistor can be omitted.

$D_1$  - Schottky diode should be used for the bootstrap. It allows the minimum drop for both, high and low side drivers. The MBR0520 works well here.

$R_{\text{CS}}$  - resistor used to set the current limit. Since the design calls for a peak current magnitude ( $I_{\text{OUT}} + 0.5 \times \Delta I_{\text{OUT}}$ ) of 4.8A, a safe setting would be 6A. (This is below the saturation current of the output inductor, which is 7.8 A.) Following the equation from the Current Limit section, use a 1.5k $\Omega$  resistor.

$R_{\text{FADJ}}$  - this resistor is used to set the switching frequency ( $F_{\text{OSC}}$ ) of the chip. The resistor value is calculated from equation in Normal Operation section. To obtain the switching frequency of 300kHz, 110k $\Omega$ , 1% resistor is needed.

$C_{\text{SS}}$  - the soft start capacitor depends on the user requirements and is calculated based on the equation from the Start Up section. For a 7ms delay, a 12nF capacitor will be suitable.

### Output Inductor

The output inductor forms the first half of the power stage in a Buck converter. It is responsible for smoothing the square wave created by the switching action and for controlling the output current ripple ( $\Delta I_{\text{OUT}}$ ). The inductance is chosen by selecting between tradeoffs in efficiency and response time. The smaller the output inductor, the more quickly the converter can respond to transients in the load current. However, as shown in the efficiency calculations, a smaller inductor requires a higher switching frequency to maintain the same level of output current ripple. An increase in frequency can mean increasing loss in the FETs due to the charging and discharging of the gates. Generally the switching frequency is chosen so that conduction loss outweighs switching loss. The equation for output inductor selection is:

$$L = \frac{V_{\text{CC}} - V_{\text{OUT}}}{\Delta I_{\text{OUT}} \times F_{\text{OSC}}} \times D$$

$$L = \frac{3.3\text{V} - 1.2\text{V}}{0.4\text{A} \times 4\text{A} \times 300\text{kHz}} \times \frac{1.2\text{V}}{3.3\text{V}}$$

$$L = 16\mu\text{H}$$

Plugging in the values for output current ripple, input voltage, output voltage, switching frequency, and assuming a 40% peak-to-peak output current ripple yields an inductance of 1.6 $\mu$ H. The output inductor must be rated to handle the peak current (also equal to the peak switch current), which is ( $I_{\text{OUT}} + 0.5 \times \Delta I_{\text{OUT}}$ ) 4.8A for a 4A design. The Coilcraft DO3316P-222P is 2.2 $\mu$ H, is rated to 7.4A rms, and has a direct current resistance ( $\text{DCR}_{\text{IOUT}}$ ) of 11m $\Omega$ .

### Output Capacitor

The output capacitor forms the second half of the power stage of a Buck switching converter. It is used to control the output voltage ripple ( $\Delta V_{\text{OUT}}$ ) and to supply load current during fast load transients.

In this example the output current is 4A and the expected type of capacitor is an aluminum electrolytic, as with the input capacitors. Other possibilities include ceramic, tantalum, and solid electrolyte capacitors, however the ceramic type often do not have the large capacitance needed to supply current for load transients, and tantalums tend to be more expensive than aluminum electrolytic. Aluminum capacitors tend to have very high capacitance and fairly low ESR, meaning that the ESR zero, which affects system stability, will be much lower than the switching frequency. The large capacitance means that at switching frequency, the ESR is dominant, hence the type and number of output capacitors is selected on the basis of ESR. One simple formula to find the maximum ESR based on the desired output voltage ripple,  $\Delta V_{\text{OUT}}$  and the designed output current ripple,  $\Delta I_{\text{OUT}}$ , is:

$$\text{ESR}_{\text{MAX}} = \frac{\Delta V_{\text{OUT}}}{\Delta I_{\text{OUT}}}$$

## Application Information (Continued)

In this example, in order to maintain a 2% peak-to-peak output voltage ripple and a 40% peak-to-peak inductor current ripple, the required maximum ESR is 15mΩ. The Sanyo 4SP560M aluminum electrolytic capacitor will give an equivalent ESR of 14mΩ. The capacitance of 560μF is enough to supply even severe load transients.

### MOSFETs

MOSFETs are the critical parts of any switching controller. Both, the control high side FET and the synchronous low side FET, have a direct impact on the system efficiency.

In this case the target efficiency for typical application circuit is about 89%. This variable will determine which MOSFET is acceptable to use for the design.

Loss from the capacitors, inductors, and IC come to about 0.27W. This leaves about 0.33W for the FET switching, conduction, and gate charging losses to meet the target efficiency. All the losses are detailed in the Efficiency section.

The switching loss is particularly difficult to estimate because it depends on many factors. When the load current is more than about 1 or 2 amps, conduction losses outweigh the switching and gate charging losses. This allows FET selection based on the  $R_{DS(ON)}$  of the FET. After adding the FET switching and gate charging losses about 0.27W leaves for conduction losses. When plugged MOSFET, the FDS6898A with a typical  $R_{DS(ON)}$  of 13mΩ, into the equation from Efficiency section for  $P_{CND}$  the loss come to be about 0.27W.

### Control Loop Components

The Typical Application Circuit has been compensated to improve the DC gain and bandwidth. The result of this compensation is better line and load transient responses. For the LM2743, the top feedback divider resistor,  $R_{FB2}$ , is also a part of the compensation. For the 3.3V to 1.2V at 4A design, the values are:

$$C_{C1} = 27\text{pF}, C_{C2} = 1200\text{nF}, C_{C3} = 3300\text{pF}, R_{C1} = 40.2\text{k}\Omega, R_{C2} = 2.55\text{k}\Omega, R_{FB2} = 10\text{k}\Omega.$$

These values give a phase margin of 53° and a bandwidth of 80kHz.

### EFFICIENCY CALCULATIONS

A reasonable estimation of the efficiency of a switching buck controller can be obtained by adding together the Output Power ( $P_{OUT}$ ) loss and the Total Power ( $P_{TOTAL}$ ) loss:

$$\eta = \frac{P_{OUT}}{P_{OUT} + P_{TOTAL}} \times 100\%$$

The Output Power ( $P_{OUT}$ ) for the Typical Application Circuit design is (1.2V \* 4A) = 4.8W. The Total Power ( $P_{TOTAL}$ ), with an efficiency calculation to complement the design, is shown below.

The majority of the power losses are due to low and high side of MOSFET's losses. The losses in any MOSFET are group of switching ( $P_{SW}$ ) and conduction losses ( $P_{CND}$ ).

$$P_{FET} = P_{SW} + P_{CND} = 61.38\text{mW} + 270\text{mW}$$

$$P_{FET} = 331.4\text{mW}$$

### FET Switching Loss ( $P_{SW}$ )

$$P_{SW} = P_{SW(ON)} + P_{SW(OFF)}$$

$$P_{SW} = 0.5 * V_{CC} * I_{OUT} * (t_r + t_f) * F_{OSC}$$

$$P_{SW} = 0.5 * 3.3\text{V} * 4\text{A} * 300\text{kHz} * 31\text{ns}$$

$$P_{SW} = 61.38\text{mW}$$

The FDS6898A has a typical turn-on rise time  $t_r$  and turn-off fall time  $t_f$  of 15ns and 16ns, respectively. The switching losses for this type of dual N-Channel MOSFETs are 0.061W.

### FET Conduction Loss ( $P_{CND}$ )

$$P_{CND} = P_{CND1} + P_{CND2}$$

$$P_{CND1} = I_{OUT}^2 * R_{DS(ON)} * k * D$$

$$P_{CND2} = I_{OUT}^2 * R_{DS(ON)} * k * (1-D)$$

$R_{DS(ON)} = 13\text{m}\Omega$  and the factor is a constant value ( $k = 1.3$ ) to account for the increasing  $R_{DS(ON)}$  of a FET due to heating.

$$P_{CND1} = (4\text{A})^2 * 13\text{m}\Omega * 1.3 * 0.364$$

$$P_{CND2} = (4\text{A})^2 * 13\text{m}\Omega * 1.3 * (1 - 0.364)$$

$$P_{CND} = 98.42\text{mW} + 172\text{mW} = 270\text{mW}$$

There are few additional losses that are taken into account:

### IC Operating Loss ( $P_{IC}$ )

$$P_{IC} = I_{Q-VCC} * V_{CC}$$

where  $I_{Q-VCC}$  is the typical operating  $V_{CC}$  current

$$P_{IC} = 1.5\text{mA} * 3.3\text{V} = 4.95\text{mW}$$

### FET Gate Charging Loss ( $P_{GATE}$ )

$$P_{GATE} = n * V_{CC} * Q_{GS} * F_{OSC}$$

$$P_{GATE} = 2 * 3.3\text{V} * 3\text{nC} * 300\text{kHz}$$

$$P_{GATE} = 5.94\text{mW}$$

The value  $n$  is the total number of FETs used and  $Q_{GS}$  is the typical gate-source charge value, which is 3nC. For the FDS6898A the gate charging loss is 5.94mW.

### Input Capacitor Loss ( $P_{CAP}$ )

$$P_{CAP} = \frac{(I_{RMS\_RIP})^2 * ESR}{n^2}$$

Where,

$$I_{RMS\_RIP} = I_{OUT} * \sqrt{D(1-D)}$$

$n$  is the number of capacitors, and ESR is equivalent series resistance.

$$P_{CAP} = \frac{(1.924\text{A})^2 * 24\text{m}\Omega}{1^2}$$

$$P_{CAP} = 88.8\text{mW}$$

### Output Inductor Loss ( $P_{IND}$ )

$$P_{IND} = I_{OUT}^2 * DCR_{IOUT}$$

where  $DCR_{IOUT}$  is the direct current resistance

$$P_{IND} = (4\text{A})^2 * 11\text{m}\Omega$$

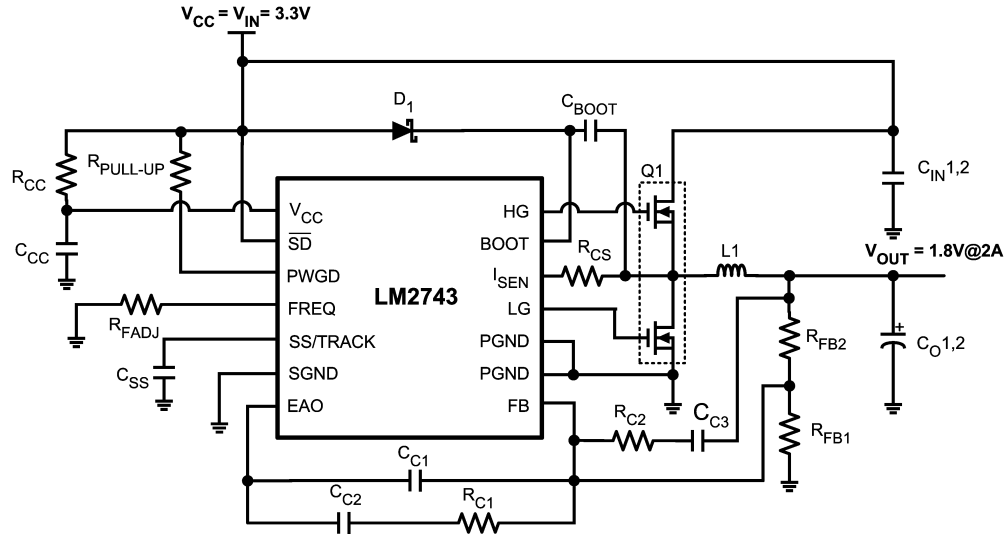
$$P_{IND} = 176\text{mW}$$

### Total System Efficiency

$$\eta = \frac{P_{OUT}}{P_{OUT} + P_{TOTAL}} \times 100\%$$

$$\eta = \frac{4.8\text{W}}{4.8\text{W} + 0.6\text{W}} = 89\%$$

## Example Circuits



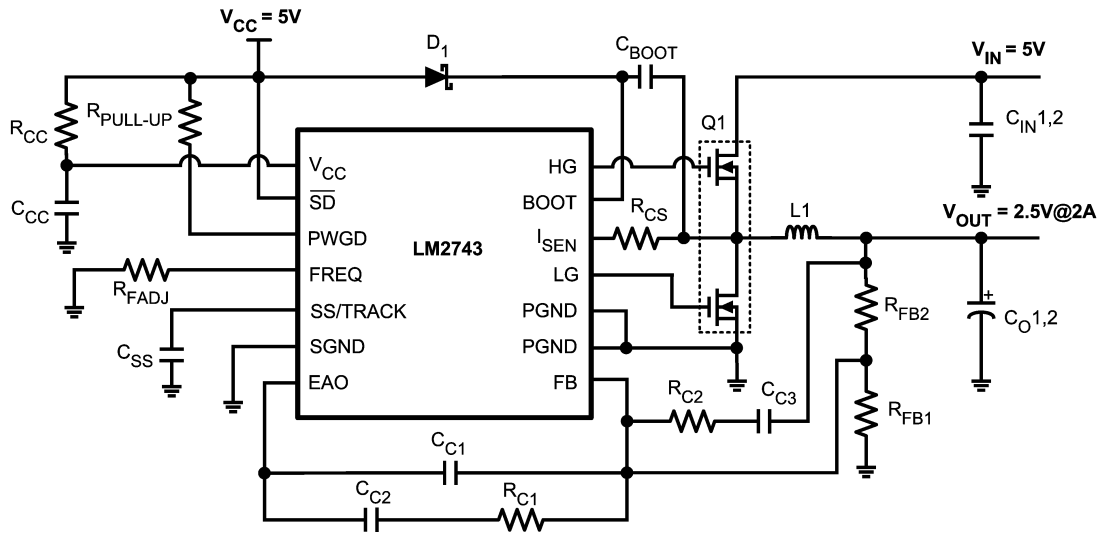
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FIGURE 12. 3.3V to 1.8V @ 2A,  $F_{sw} = 300\text{kHz}$ 

PART	PART NUMBER	TYPE	PACKAGE	DESCRIPTION	VENDOR
U <sub>1</sub>	LM2743	Synchronous Controller	TSSOP-14		NSC
Q <sub>1</sub>	FDS6898A	Dual N-MOSFET	SO-8	20V, 10mΩ@ 4.5V, 16nC	Fairchild
D <sub>1</sub>	MBR0520LT1	Schottky Diode	SOD-123		
L <sub>1</sub>	DO3316P-472	Inductor		4.7μH, 4.8Arms 18mΩ	Coilcraft
C <sub>IN1</sub>	16SP100M	Aluminum Electrolytic		100μF, 16V, 2.89Arms	Sanyo
C <sub>O1</sub>	6SP220M	Aluminum Electrolytic		220μF, 6.3V 3.1Arms	Sanyo
C <sub>CC</sub> , C <sub>BOOT</sub> , C <sub>IN2</sub> , C <sub>O2</sub>	VJ1206Y104KXXA	Capacitor	1206	0.1μF, 10%	Vishay
C <sub>C3</sub>	VJ805Y332KXXA	Capacitor	805	3300pF, 10%	Vishay
C <sub>SS</sub>	VJ0805Y123KXXA	Capacitor	805	12nF, 10%	Vishay
C <sub>C2</sub>	VJ1805A821KXAA	Capacitor	805	820pF 10%	Vishay
C <sub>C1</sub>	VJ0805A220KXAA	Capacitor	805	22pF, 10%	Vishay
R <sub>FB2</sub>	CRCW08051002F	Resistor	805	10.0kΩ 1%	Vishay
R <sub>FB1</sub>	CRCW08054991F	Resistor	805	4.99kΩ1%	Vishay
R <sub>FADJ</sub>	CRCW08051103F	Resistor	805	110kΩ 1%	Vishay
R <sub>C2</sub>	CRCW08052101F	Resistor	805	2.1kΩ 1%	Vishay
R <sub>CS</sub>	CRCW08057500F	Resistor	805	750Ω 1%	Vishay
R <sub>CC</sub>	CRCW080510R0F	Resistor	805	10.0Ω 1%	Vishay
R <sub>C1</sub>	CRCW08055492F	Resistor	805	54.9kΩ 1%	Vishay
R <sub>PULL-UP</sub>	CRCW08051003J	Resistor	805	100kΩ 5%	Vishay



## Example Circuits (Continued)

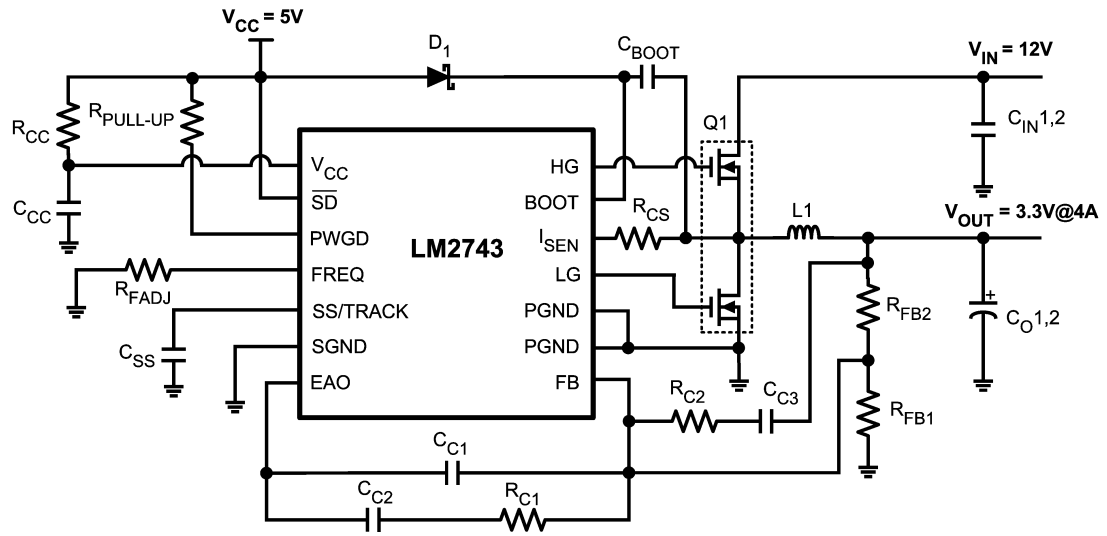


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FIGURE 13. 5V to 2.5V @ 2A,  $F_{sw} = 300\text{kHz}$

PART	PART NUMBER	TYPE	PACKAGE	DESCRIPTION	VENDOR
U <sub>1</sub>	LM2743	Synchronous Controller	TSSOP-14		NSC
Q <sub>1</sub>	FDS6898A	Dual N-MOSFET	SO-8	20V, 10mΩ@ 4.5V, 16nC	Fairchild
D <sub>1</sub>	MBR0520LTI	Schottky Diode	SOD-123		
L <sub>1</sub>	DO3316P-682	Inductor		6.8μH, 4.4Arms, 27mΩ	Coilcraft
C <sub>IN1</sub>	16SP100M	Aluminum Electrolytic		100μF, 16V, 2.89Arms	Sanyo
C <sub>O1</sub>	10SP56M	Aluminum Electrolytic		56μF, 10V 1.7Arms	Sanyo
C <sub>CC</sub> , C <sub>BOOT</sub> , C <sub>IN2</sub> , C <sub>O2</sub>	VJ1206Y104KXXA	Capacitor	1206	0.1μF, 10%	Vishay
C <sub>C3</sub>	VJ0805A182KXAA	Capacitor	805	1800pF, 10%	Vishay
C <sub>SS</sub>	VJ0805Y123KXXA	Capacitor	805	12nF, 10%	Vishay
C <sub>C2</sub>	VJ1805A821KXAA	Capacitor	805	820pF 10%	Vishay
C <sub>C1</sub>	VJ0805A330KXAA	Capacitor	805	33pF, 10%	Vishay
R <sub>FB2</sub>	CRCW08051002F	Resistor	805	10.0kΩ 1%	Vishay
R <sub>FB1</sub>	CRCW08053161F	Resistor	805	3.16kΩ 1%	Vishay
R <sub>FADJ</sub>	CRCW08051103F	Resistor	805	110kΩ 1%	Vishay
R <sub>C2</sub>	CRCW08051301F	Resistor	805	1.3kΩ 1%	Vishay
R <sub>CS</sub>	CRCW08057870F	Resistor	805	787Ω 1%	Vishay
R <sub>CC</sub>	CRCW080510R0F	Resistor	805	10.0Ω 1%	Vishay
R <sub>C1</sub>	CRCW08053322F	Resistor	805	33.2kΩ 1%	Vishay
R <sub>PULL-UP</sub>	CRCW08051003J	Resistor	805	100kΩ 5%	Vishay

## Example Circuits (Continued)

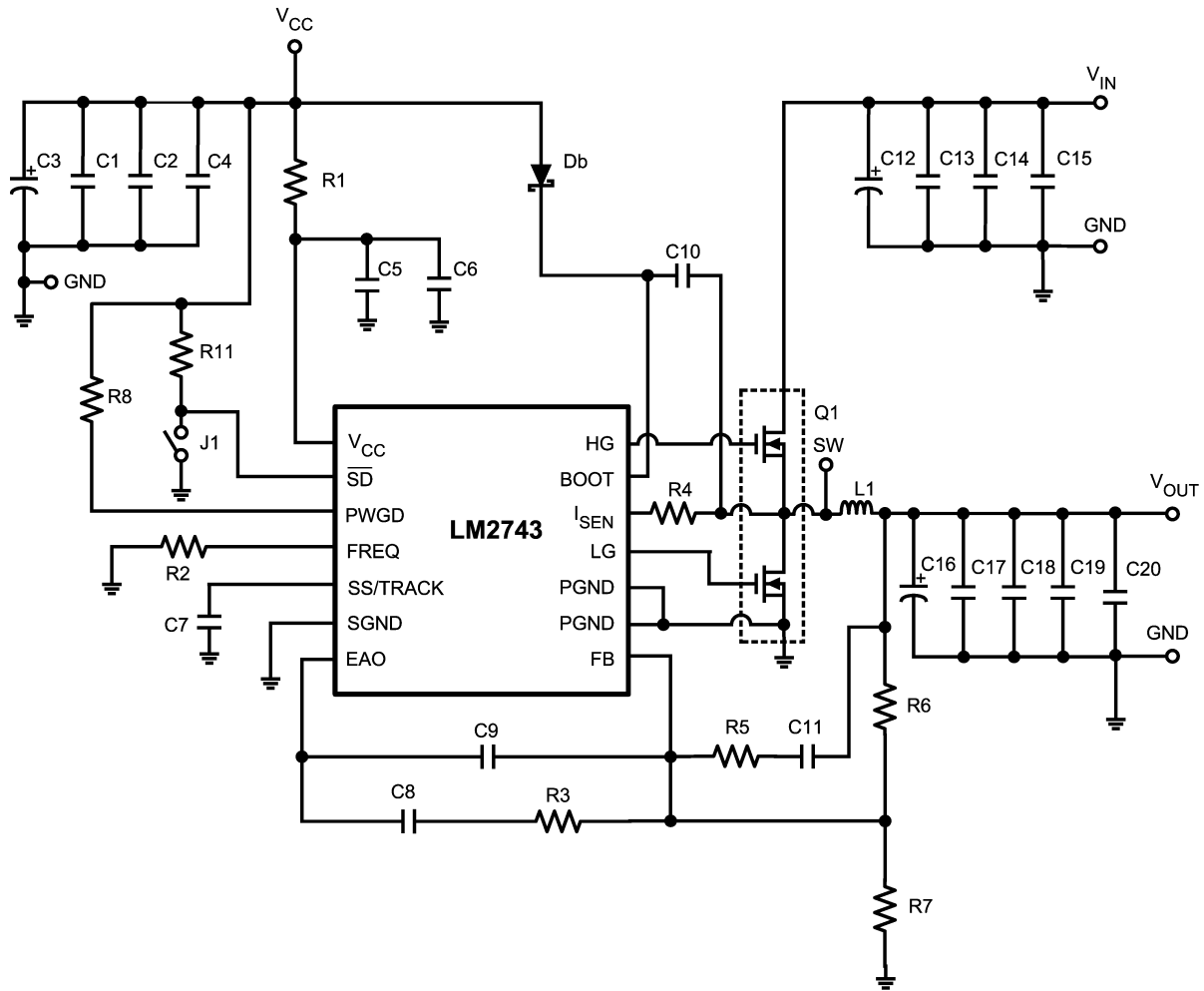


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FIGURE 14. 5V to 3.3V @ 4A,  $F_{sw} = 300\text{kHz}$ 

PART	PART NUMBER	TYPE	PACKAGE	DESCRIPTION	VENDOR
U <sub>1</sub>	LM2743	Synchronous Controller	TSSOP-14		NSC
Q <sub>1</sub>	FDS6898A	Dual N-MOSFET	SO-8	20V, 10mΩ@ 4.5V, 16nC	Fairchild
D <sub>1</sub>	MBR0520LTI	Schottky Diode	SOD-123		
L <sub>1</sub>	DO3316P-332	Inductor		3.3µH, 5.4Arms 15mΩ	Coilcraft
C <sub>IN1</sub>	16SP100M	Aluminum Electrolytic		100µF, 16V 2.89Arms	Sanyo
C <sub>O1</sub>	6SP220M	Aluminum Electrolytic		220µF, 6.3V 3.1Arms	Sanyo
C <sub>CC</sub> , C <sub>BOOT</sub> , C <sub>IN2</sub> , C <sub>O2</sub>	VJ1206Y104KXXA	Capacitor	1206	0.1µF, 10%	Vishay
C <sub>C3</sub>	VJ805Y222KXXA	Capacitor	805	2200pF, 10%	Vishay
C <sub>SS</sub>	VJ0805Y123KXXA	Capacitor	805	12nF, 10%	Vishay
C <sub>C2</sub>	VJ805Y332KXXA	Capacitor	805	3300pF 10%	Vishay
C <sub>C1</sub>	VJ0805A820KXAA	Capacitor	805	82pF, 10%	Vishay
R <sub>FB2</sub>	CRCW08051002F	Resistor	805	10.0kΩ 1%	Vishay
R <sub>FB1</sub>	CRCW08052211F	Resistor	805	2.21kΩ 1%	Vishay
R <sub>FADJ</sub>	CRCW08051103F	Resistor	805	110kΩ 1%	Vishay
R <sub>C2</sub>	CRCW08052611F	Resistor	805	2.61kΩ 1%	Vishay
R <sub>C3</sub>	CRCW08057870F	Resistor	805	787Ω 1%	Vishay
R <sub>CC</sub>	CRCW080510R0F	Resistor	805	10.0Ω 1%	Vishay
R <sub>C1</sub>	CRCW08051272F	Resistor	805	12.7kΩ 1%	Vishay
R <sub>PULL-UP</sub>	CRCW08051003J	Resistor	805	100kΩ 5%	Vishay

### Evaluation Board Schematic



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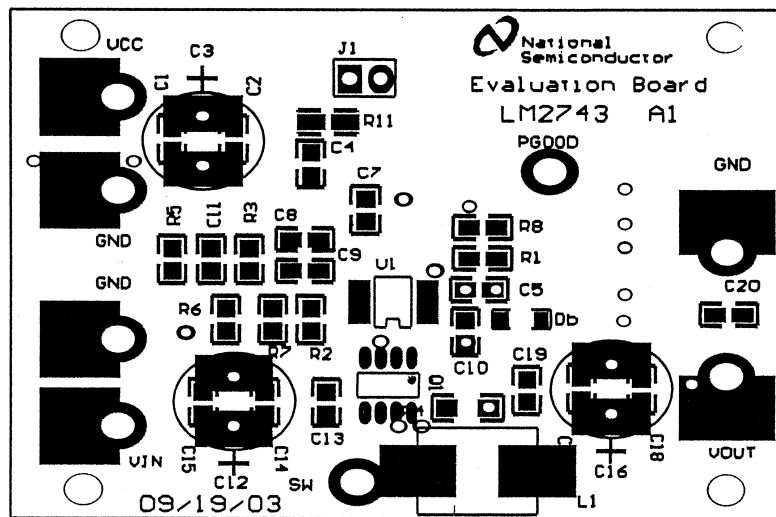
FIGURE 15. 3.3V to 1.2V @ 4A,  $F_{sw} = 300kHz$

PART	PART NUMBER	TYPE	PACKAGE	DESCRIPTION	VENDOR
U <sub>1</sub>	LM2743	Synchronous Controller	TSSOP-14		NSC
Q <sub>1</sub>	FDS6898A	Dual N-MOSFET	SO-8	20V, 10mΩ@ 4.5V, 16nC	Fairchild
D <sub>1</sub>	MBR0520LT1	Schottky Diode	SOD-123		
L <sub>1</sub>	DO3316P-222	Inductor		2.2μH, 6.1Arms 12mΩ	Coilcraft
J <sub>1</sub>	NOT USED				
C12	20SP120M	Aluminum Electrolytic		120μF, 20V 3.1Arms	Sanyo
C16	4SP560M	Aluminum Electrolytic		560μF, 4V 4Arms	Sanyo
C4,C5,C10, C13,C19	VJ1206Y104KXXA	Capacitor	1206	0.1μF, 10%	Vishay
C11	VJ805Y332KXXA	Capacitor	805	3300pF 10%	Vishay
C7	VJ0805Y123KXXA	Capacitor	805	12nF, 10%	Vishay

## Evaluation Board Schematic (Continued)

PART	PART NUMBER	TYPE	PACKAGE	DESCRIPTION	VENDOR
C8	VJ1206Y122KXXA	Capacitor	1206	1200pF 10%	Vishay
C9	VJ0805A270KXAA	Capacitor	805	27pF, 10%	Vishay
C1, C2, C3, C6, C14, C15, C17, C18, C20	NOT USED				
R6	CRCW08051002F	Resistor	805	10.0k $\Omega$ 1%	Vishay
R7	CRCW08051002F	Resistor	805	10.0k $\Omega$ 1%	Vishay
R2	CRCW08051103F	Resistor	805	110k $\Omega$ 1%	Vishay
R5	CRCW08052551F	Resistor	805	2.55k $\Omega$ 1%	Vishay
R4	CRCW08051501F	Resistor	805	1.50k $\Omega$ 1%	Vishay
R1	CRCW080510R0F	Resistor	805	10.0 $\Omega$ 1%	Vishay
R3	CRCW08054022F	Resistor	805	40.2k $\Omega$ 1%	Vishay
R11	CRCW08050R00F	Resistor	805	0 $\Omega$ 1%	Vishay
R8	CRCW08051003J	Resistor	805	100k $\Omega$ 5%	Vishay

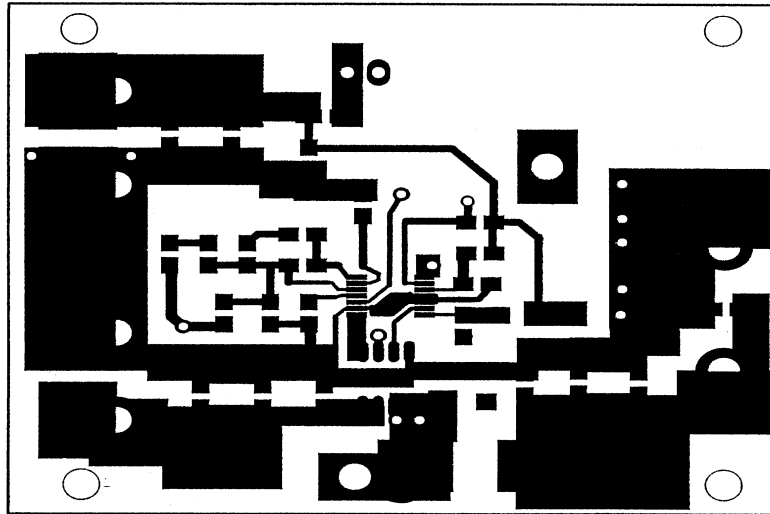
## PCB Layout for the Evaluation Board



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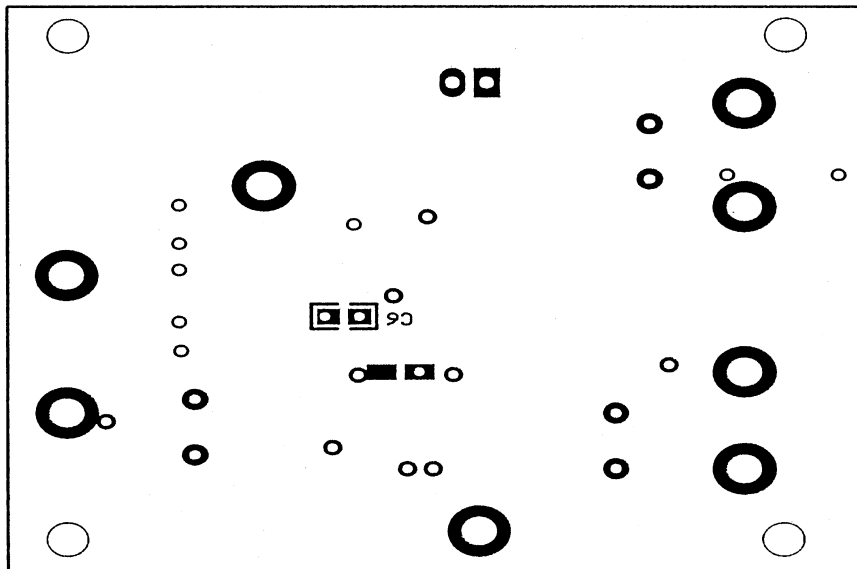
Top Silkscreen

# PCB Layout for the Evaluation Board (Continued)



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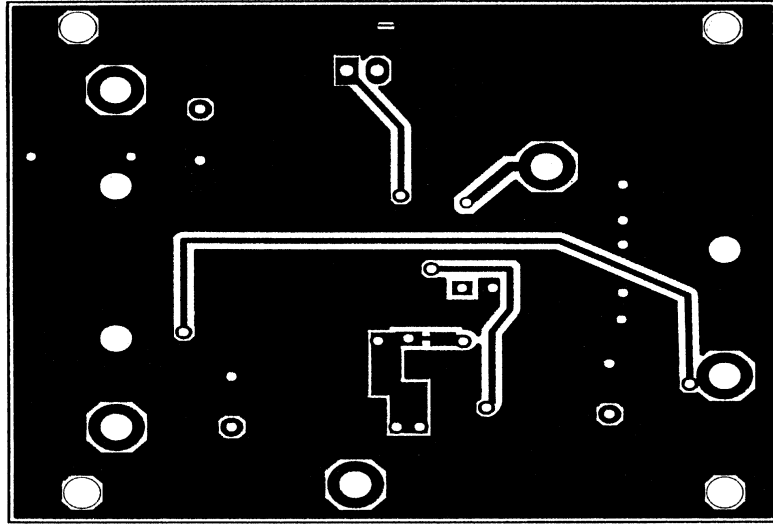
Top Copper



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Bottom Silkscreen

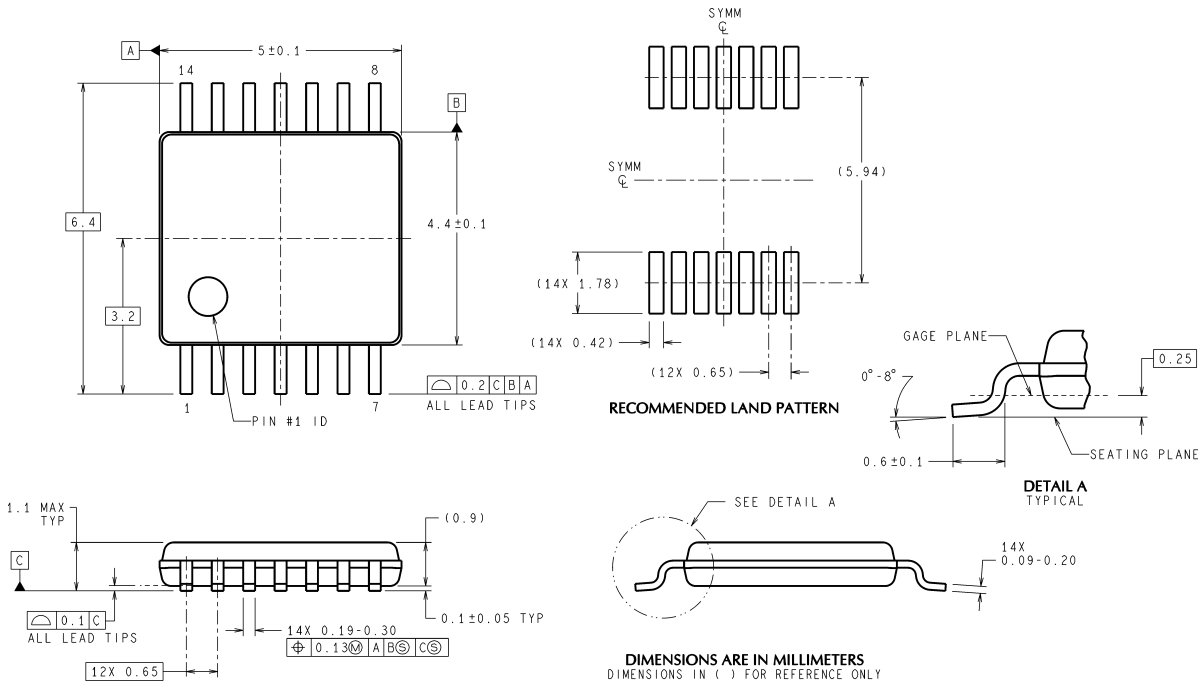
# PCB Layout for the Evaluation Board (Continued)



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Bottom Copper

**Physical Dimensions** inches (millimeters) unless otherwise noted



**TSSOP-14 Pin Package**  
**NS Package Number MTC14**

MTC14 (Rev D)


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