

FEATURES

- Complete Switch Mode Power Supply
- Wide Input Voltage Range: 4.5V to 28V
- 6A DC, Typical 8A Peak Output Current
- 0.6V to 5V Output Voltage
- 1.5% Output Voltage Regulation
- Ultrafast Transient Response
- Parallel μ Module™ DC/DC Converters
- Current Mode Control
- Pin Compatible with the LTM4600 and LTM4602
- Up to 92% Efficiency
- Programmable Soft-Start
- Output Overvoltage Protection
- Optional Short-Circuit Shutdown Timer
- Pb-Free (e4) RoHS Compliant Package with Gold-Pad Finish
- Small Footprint, Low Profile (15mm × 15mm × 2.8mm) LGA Package

APPLICATIONS

- Telecom and Networking Equipment
- Servers
- Industrial Equipment
- Point of Load Regulation

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DESCRIPTION

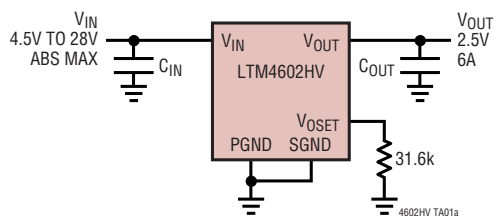
The LTM®4602HV is a complete 6A, DC/DC step down power supply with up to 28V input operation. Included in the package are the switching controller, power FETs, inductor, and all support components. Operating over an input voltage range of 4.5V to 28V, the LTM4602HV supports an output voltage range of 0.6V to 5V, set by a single resistor. This high efficiency design delivers 6A continuous current (8A peak), needing no heat sinks or airflow to meet power specifications. Only bulk input and output capacitors are needed to finish the design.

The low profile package (2.8mm) enables utilization of unused space on the bottom of PC boards for high density point of load regulation. High switching frequency and an adaptive on-time current mode architecture enables a very fast transient response to line and load changes without sacrificing stability. Fault protection features include integrated overvoltage and short circuit protection with a defeatable shutdown timer. A built-in soft-start timer is adjustable with a small capacitor.

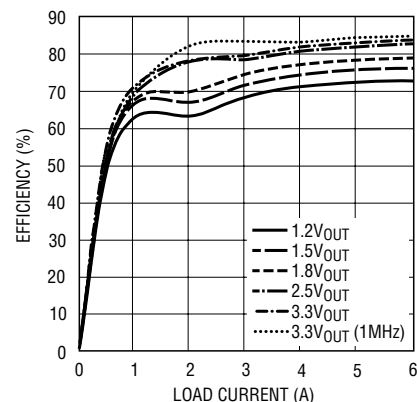
The LTM4602HV is packaged in a thermally enhanced, compact (15mm × 15mm) and low profile (2.8mm) over-molded Land Grid Array (LGA) package suitable for automated assembly by standard surface mount equipment. For the 4.5V to 20V input range version, refer to the LTM4602.

TYPICAL APPLICATION

6A μ Module Power Supply with 4.5V to 28V Input



Efficiency vs Load Current with 24V_{IN} (FCB = 0)



4602HV G03

4602hvf

ABSOLUTE MAXIMUM RATINGS

(Note 1)

FCB, EXT _V CC, PGOOD, RUN/SS, V _{OUT}	-0.3V to 6V
V _{IN} , SV _{IN} , f _{ADJ}	-0.3V to 28V
V _{OSET} , COMP.....	-0.3V to 2.7V
Operating Temperature Range (Note 2) ...	-40°C to 85°C
Junction Temperature	125°C
Storage Temperature Range.....	-55°C to 125°C

PACKAGE/ORDER INFORMATION

TOP VIEW

LGA PACKAGE
104-LEAD (15mm × 15mm × 2.8mm)
T_{JMAX} = 125°C, θ_{JA} = 15°C/W, θ_{JC} = 6°C/W,
θ_{JA} DERIVED FROM 95mm × 76mm PCB WITH 4 LAYERS
WEIGHT = 1.7g

ORDER PART NUMBER	LGA PART MARKING*
LTM4602HVEV#PBF LTM4602HVIV#PBF	LTM4602HVV LTM4602HVV

Consult LTC Marketing for parts specified with wider operating temperature ranges.
*The temperature grade is identified by a label on the shipping container.

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the -40°C to 85°C temperature range, otherwise specifications are at T_A = 25°C, V_{IN} = 12V. External C_{IN} = 120μF, C_{OUT} = 200μF/Ceramic per typical application (front page) configuration.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
V _{IN(DC)}	Input DC Voltage	AbsMax 28V for Tolerance on 24V Inputs ●	4.5		28	V
V _{OUT(DC)}	Output Voltage	FCB = 0V V _{IN} = 5V or 12V, V _{OUT} = 1.5V, I _{OUT} = 0A ●	1.478 1.470	1.50 1.50	1.522 1.530	V V
Input Specifications						
V _{IN(UVLO)}	Under Voltage Lockout Threshold	I _{OUT} = 0A		3.4	4	V
I _{INRUSH(VIN)}	Input Inrush Current at Startup	I _{OUT} = 0A, V _{OUT} = 1.5V, FCB = 0 V _{IN} = 5V V _{IN} = 12V V _{IN} = 24V		0.6 0.7 0.8		A A A
I _{Q(VIN)}	Input Supply Bias Current	I _{OUT} = 0A, EXT _V CC Open V _{IN} = 12V, V _{OUT} = 1.5V, FCB = 5V V _{IN} = 12V, V _{OUT} = 1.5V, FCB = 0V V _{IN} = 24V, V _{OUT} = 2.5V, FCB = 5V V _{IN} = 24V, V _{OUT} = 2.5V, FCB = 0V Shutdown, RUN = 0.8V, V _{IN} = 12V		1.2 42 1.8 36 50	100	mA mA mA mA μA
Min On Time				100		ns
Min Off Time				400		ns
I _{S(VIN)}	Input Supply Current	V _{IN} = 12V, V _{OUT} = 1.5V, I _{OUT} = 6A V _{IN} = 12V, V _{OUT} = 3.3V, I _{OUT} = 6A V _{IN} = 5V, V _{OUT} = 1.5V, I _{OUT} = 6A V _{IN} = 24V to 3.3V at 6A, EXT _V CC = 5V		0.88 1.50 2.08 0.98		A A A A

4602hvf

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the -40°C to 85°C temperature range, otherwise specifications are at $T_A = 25^{\circ}\text{C}$, $V_{IN} = 12\text{V}$. Per typical application (front page) configuration.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS	
Output Specifications							
I_{OUTDC}	Output Continuous Current Range (See Output Current Derating Curves for Different V_{IN} , V_{OUT} and T_A)	$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$ $V_{IN} = 24\text{V}$, $V_{OUT} = 2.5\text{V}$ (Note 3)	0 0		6 6	A A	
$\frac{\Delta V_{OUT(LINE)}}{V_{OUT}}$	Line Regulation Accuracy	$V_{OUT} = 1.5\text{V}$. FCB = 0V, $I_{OUT} = 0\text{A}$, $V_{IN} = 4.5\text{V}$ to 28V	●	0.15		%	
$\frac{\Delta V_{OUT(0A-6A)}}{V_{OUT}}$	Load Regulation Accuracy	$V_{OUT} = 1.5\text{V}$. FCB = 0V, $I_{OUT} = 0\text{A}$ to 6A , $V_{IN} = 5\text{V}$, $V_{IN} = 12\text{V}$ (Note 4)	●	± 0.25 ± 0.5	± 0.5 ± 1	% %	
$V_{OUT(AC)}$	Output Ripple Voltage	$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$, FCB = 0V, $I_{OUT} = 0\text{A}$		10	15	mV _{p-p}	
f_s	Output Ripple Voltage Frequency	FCB = 0V, $I_{OUT} = 6\text{A}$, $V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$		800		kHz	
t_{START}	Turn-On Time	$V_{OUT} = 1.5\text{V}$, $I_{OUT} = 1\text{A}$ $V_{IN} = 12\text{V}$ $V_{IN} = 5\text{V}$		0.5 0.7		ms ms	
ΔV_{OUTLS}	Voltage Drop for Dynamic Load Step	$V_{OUT} = 1.5\text{V}$, Load Step: $0\text{A}/\mu\text{s}$ to $3\text{A}/\mu\text{s}$ $C_{OUT} = 22\mu\text{F}$ 6.3V, $330\mu\text{F}$ 4V Pos Cap, See Table 2		30		mV	
t_{SETTLE}	Settling Time for Dynamic Load Step $V_{IN} = 12\text{V}$	Load: 10% to 90% to 10% of Full Load		25		μs	
I_{OUTPK}	Output Current Limit	Output Voltage in Foldback $V_{IN} = 24\text{V}$, $V_{OUT} = 2.5\text{V}$ $V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$ $V_{IN} = 5\text{V}$, $V_{OUT} = 1.5\text{V}$		9 9 9		A A A	
Control Stage							
V_{OSET}	Voltage at V_{OSET} Pin	$I_{OUT} = 0\text{A}$, $V_{OUT} = 1.5\text{V}$	●	0.591 0.594	0.6 0.6	0.609 0.606	V V
$V_{RUN/SS}$	RUN ON/OFF Threshold			0.8	1.5	2	V
$I_{RUN(C)/SS}$	Soft-Start Charging Current	$V_{RUN/SS} = 0\text{V}$		-0.5	-1.2	-3	μA
$I_{RUN(D)/SS}$	Soft-Start Discharging Current	$V_{RUN/SS} = 4\text{V}$		0.8	1.8	3	μA
$V_{IN} - SV_{IN}$		$EXTV_{CC} = 0\text{V}$, FCB = 0V			100		mV
I_{EXTVCC}	Current into $EXTV_{CC}$ Pin	$EXTV_{CC} = 5\text{V}$, FCB = 0V, $V_{OUT} = 1.5\text{V}$, $I_{OUT} = 0\text{A}$			16		mA
R_{FBHI}	Resistor Between V_{OUT} and FB Pins				100		k Ω
V_{FCB}	Forced Continuous Threshold			0.57	0.6	0.63	V
I_{FCB}	Forced Continuous Pin Current	$V_{FCB} = 0.6\text{V}$			-1	-2	μA
PGOOD Output							
ΔV_{OSETH}	PGOOD Upper Threshold	V_{OSET} Rising		7.5	10	12.5	%
ΔV_{OSETL}	PGOOD Lower Threshold	V_{OSET} Falling		-7.5	-10	-12.5	%
$\Delta V_{OSET(HYS)}$	PGOOD Hysteresis	V_{OSET} Returning			2		%
V_{PGL}	PGOOD Low Voltage	$I_{PGOOD} = 5\text{mA}$			0.15	0.4	V

Note 1: Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

Note 2: The LTM4602HVE is guaranteed to meet performance specifications from 0°C to 85°C . Specifications over the -40°C to 85°C

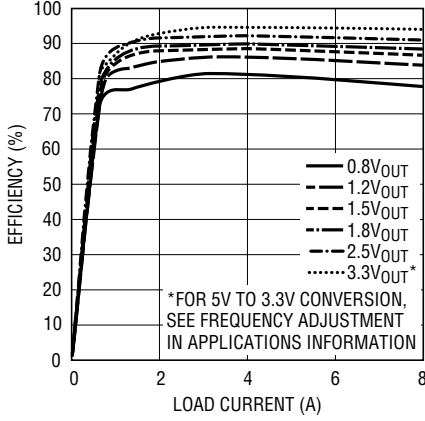
operating temperature range are assured by design, characterization and correlation with statistical process controls. The LTM4602HVI is guaranteed and tested over the -40°C to 85°C temperature range.

Note 3: Refer to current de-rating curves and thermal application note.

Note 4: Test assumes current derating verses temperature.

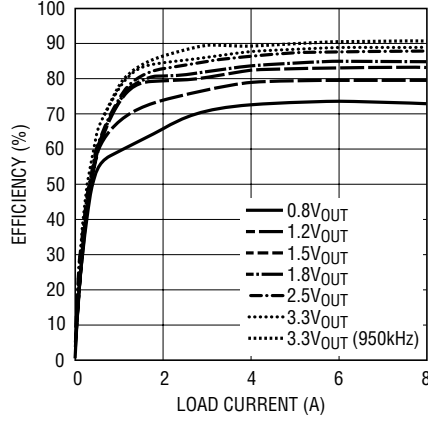
TYPICAL PERFORMANCE CHARACTERISTICS (See Figure 22 for all curves)

Efficiency vs Load Current with 5V_{IN} (FCB = 0)



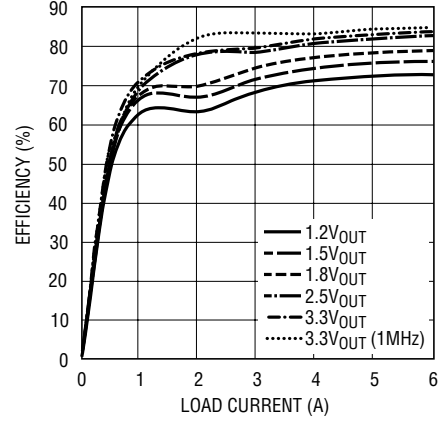
4602HV G01

Efficiency vs Load Current with 12V_{IN} (FCB = 0)



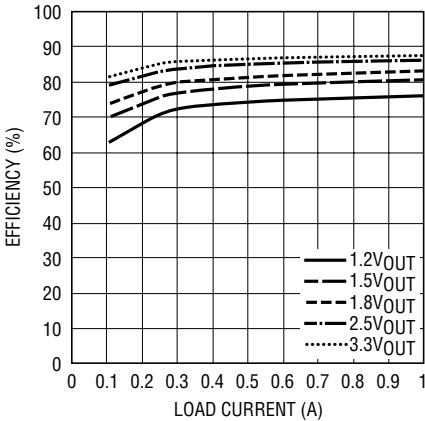
4602HV G02

Efficiency vs Load Current with 24V_{IN} (FCB = 0)



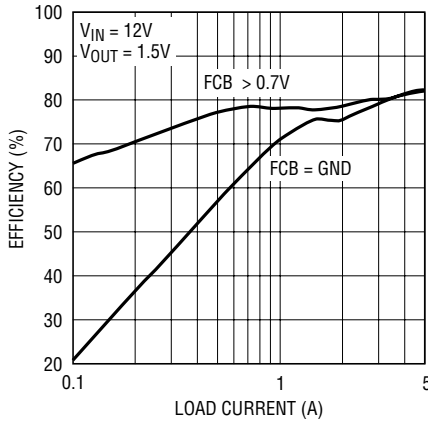
4602HV G03

Light Load Efficiency vs Load Current with 12V_{IN} (FCB > 0.7V, <5V)



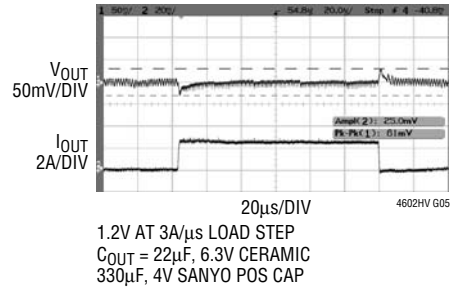
4602HV G15

Efficiency vs Load Current with Different FCB Settings



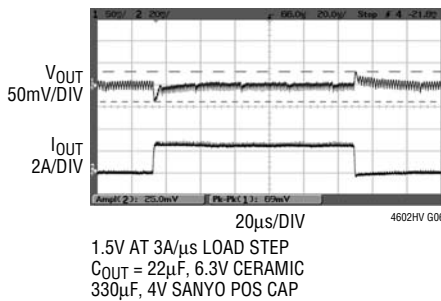
4602HV G04

1.2V Transient Response



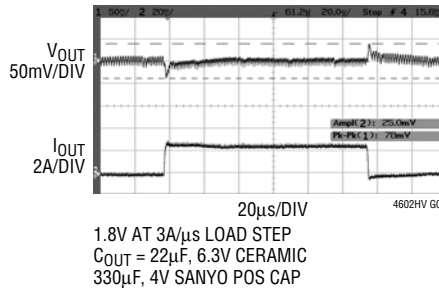
4602HV G05

1.5V Transient Response



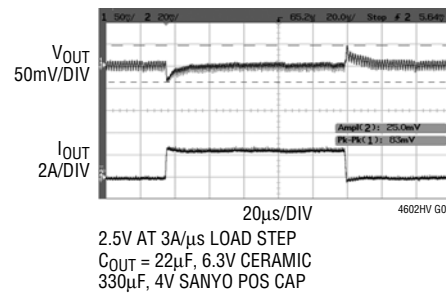
4602HV G06

1.8V Transient Response



4602HV G07

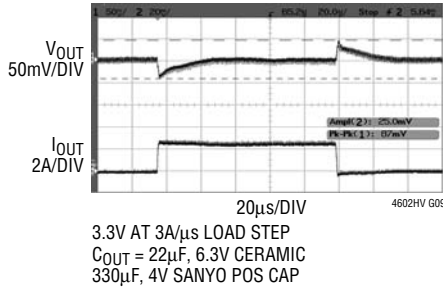
2.5V Transient Response



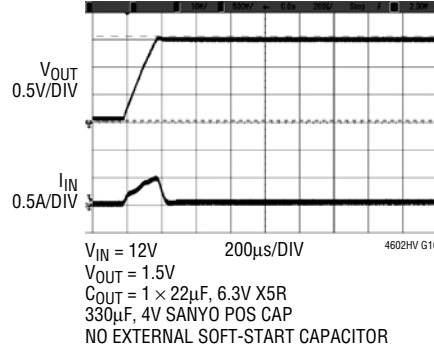
4602HV G08

TYPICAL PERFORMANCE CHARACTERISTICS (See Figure 22 for all curves)

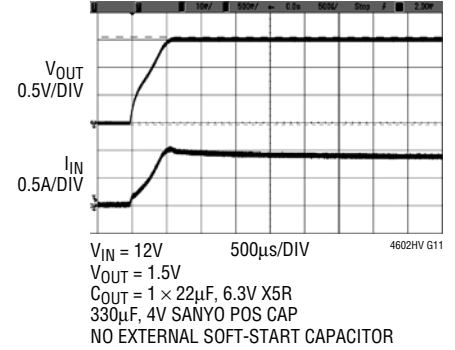
3.3V Transient Response



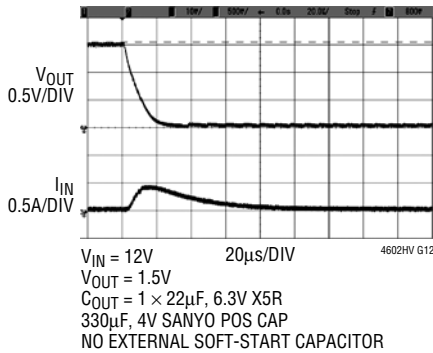
Start-Up, $I_{OUT} = 0A$



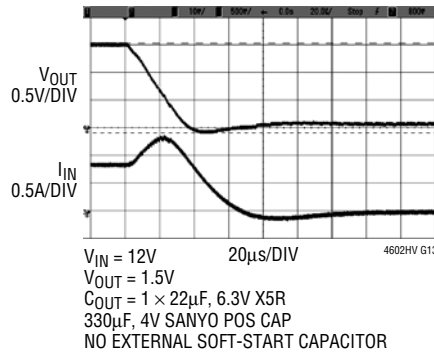
**Start-Up, $I_{OUT} = 6A$
(Resistive Load)**



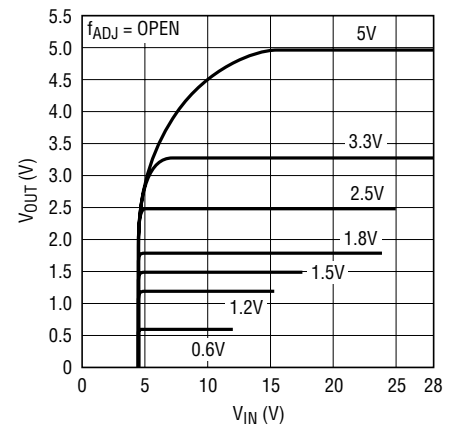
**Short-Circuit Protection,
 $I_{OUT} = 0A$**



**Short-Circuit Protection,
 $I_{OUT} = 6A$**



V_{IN} to V_{OUT} Stepdown Ratio



SEE FREQUENCY ADJUSTMENT DISCUSSION FOR $12V_{IN}$ TO $5V_{OUT}$ AND $5V_{IN}$ TO $3.3V_{OUT}$ CONVERSION

4602HV G14

PIN FUNCTIONS (See Package Description for Pin Assignment)

V_{IN} (Bank 1): Power Input Pins. Apply input voltage between these pins and PGND pins. Recommend placing input decoupling capacitance directly between V_{IN} pins and PGND pins.

f_{ADJ} (Pin A15): A 110k resistor from V_{IN} to this pin sets the one-shot timer current, thereby setting the switching frequency. The LTM4602HV switching frequency is typically 850kHz. An external resistor to ground can be selected to reduce the one-shot timer current, thus lower the switching frequency to accommodate a higher duty cycle step down requirement. See the applications section.

SV_{IN} (Pin A17): Supply Pin for Internal PWM Controller. Leave this pin open or add additional decoupling capacitance.

$EXTV_{CC}$ (Pin A19): External 5V supply pin for controller. If left open or grounded, the internal 5V linear regulator will power the controller and MOSFET drivers. For high input voltage applications, connecting this pin to an external 5V will reduce the power loss in the power module. The $EXTV_{CC}$ voltage should never be higher than V_{IN} .

V_{OSET} (Pin A21): The Negative Input of The Error Amplifier. Internally, this pin is connected to V_{OUT} with a 100k precision resistor. Different output voltages can be programmed with additional resistors between the V_{OSET} and SGND pins.

COMP (Pin B23): Current Control Threshold and Error Amplifier Compensation Point. The current comparator threshold increases with this control voltage. The voltage ranges from 0V to 2.4V with 0.8V corresponding to zero sense voltage (zero current).

SGND (Pin D23): Signal Ground Pin. All small-signal components should connect to this ground, which in turn connects to PGND at one point.

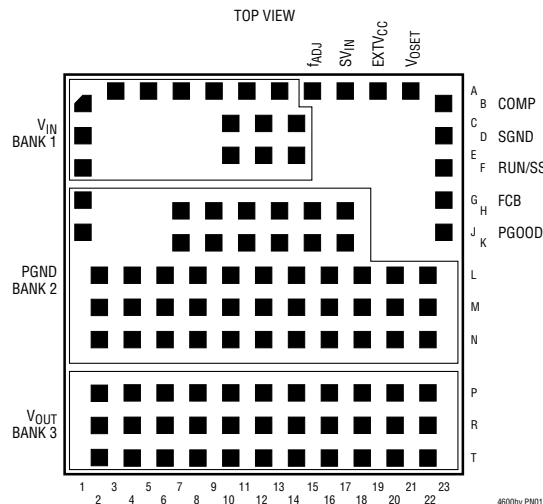
RUN/SS (Pin F23): Run and Soft-Start Control. Forcing this pin below 0.8V will shut down the power supply. Inside the power module, there is a 1000pF capacitor which provides approximately 0.7ms soft-start time with 200 μ F output capacitance. Additional soft-start time can be achieved by adding additional capacitance between the RUN/SS and SGND pins. The internal short-circuit lathoff can be disabled by adding a resistor between this pin and the V_{IN} pin. This resistor must supply a minimum 5 μ A pull up current.

FCB (Pin G23): Forced Continuous Input. Grounding this pin enables forced continuous mode operation regardless of load conditions. Tying this pin above 0.63V enables discontinuous conduction mode to achieve high efficiency operation at light loads. There is an internal 10k resistor between the FCB and SGND pins.

PGOOD (Pin J23): Output Voltage Power Good Indicator. When the output voltage is within 10% of the nominal voltage, the PGOOD is open drain output. Otherwise, this pin is pulled to ground.

PGND (Bank 2): Power ground pins for both input and output returns.

V_{OUT} (Bank 3): Power Output Pins. Apply output load between these pins and PGND pins. Recommend placing High Frequency output decoupling capacitance directly between these pins and PGND pins.



SIMPLIFIED BLOCK DIAGRAM

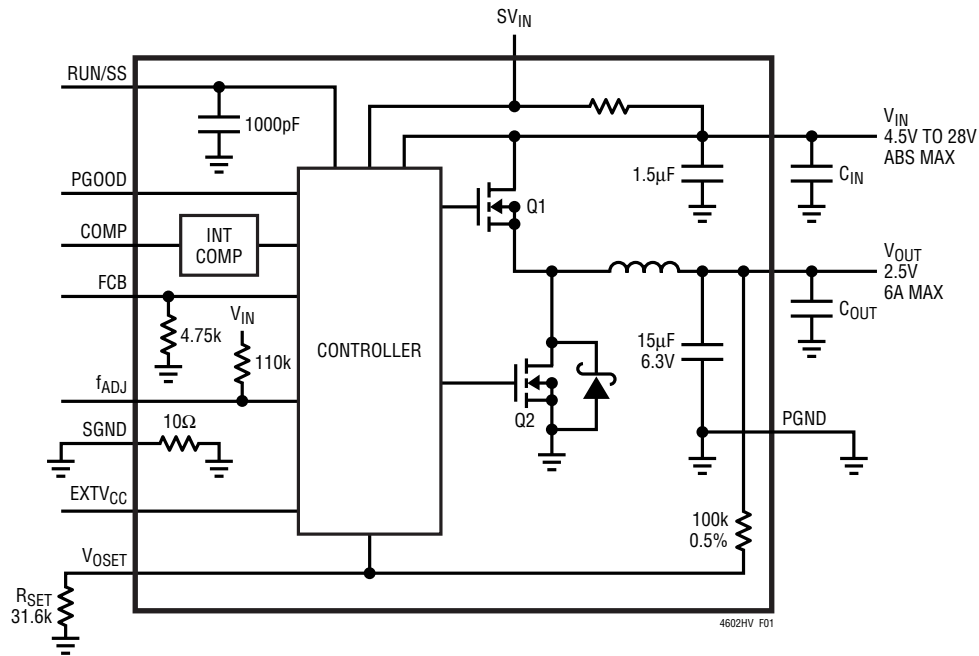


Figure 1. Simplified LTM4602HV Block Diagram

DECOUPLING REQUIREMENTS

$T_A = 25^\circ\text{C}$, $V_{IN} = 12\text{V}$. Use Figure 1 configuration.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
C_{IN}	External Input Capacitor Requirement ($V_{IN} = 4.5\text{V to } 28\text{V}$, $V_{OUT} = 2.5\text{V}$)	$I_{OUT} = 6\text{A}$, 2x 10 μF 35V Ceramic Taiyo Yuden GDK316BJ106ML	20			μF
C_{OUT}	External Output Capacitor Requirement ($V_{IN} = 4.5\text{V to } 28\text{V}$, $V_{OUT} = 2.5\text{V}$)	$I_{OUT} = 6\text{A}$, Refer to Table 2 in the Applications Information Section	100	200		μF

OPERATION

µModule Description

The LTM4602HV is a standalone non-isolated synchronous switching DC/DC power supply. It can deliver up to 6A of DC output current with only bulk external input and output capacitors. This module provides a precisely regulated output voltage programmable via one external resistor from $0.6V_{DC}$ to $5.0V_{DC}$. The input voltage range is 4.5V to 28V. A simplified block diagram is shown in Figure 1 and the typical application schematic is shown in Figure 21.

The LTM4602HV contains an integrated LTC constant on-time current-mode regulator, ultra-low $R_{DS(ON)}$ FETs with fast switching speed and integrated Schottky diode. The typical switching frequency is 800kHz at full load. With current mode control and internal feedback loop compensation, the LTM4602HV module has sufficient stability margins and good transient performance under a wide range of operating conditions and with a wide range of output capacitors, even all ceramic output capacitors (X5R or X7R).

Current mode control provides cycle-by-cycle fast current limit. In addition, foldback current limiting is provided in an over-current condition while V_{FB} drops. Also, the LTM4602HV has defeatable short circuit latch off. Internal overvoltage and undervoltage comparators pull the open-drain PGOOD output low if the output feedback voltage exits a $\pm 10\%$ window around the regulation point. Furthermore,

in an overvoltage condition, internal top FET Q1 is turned off and bottom FET Q2 is turned on and held on until the overvoltage condition clears.

Pulling the RUN/SS pin low forces the controller into its shutdown state, turning off both Q1 and Q2. Releasing the pin allows an internal $1.2\mu A$ current source to charge up the softstart capacitor. When this voltage reaches 1.5V, the controller turns on and begins switching.

At low load current the module works in continuous current mode by default to achieve minimum output voltage ripple. It can be programmed to operate in discontinuous current mode for improved light load efficiency when the FCB pin is pulled up above 0.8V and no higher than 6V. The FCB pin has a 10k resistor to ground, so a resistor to V_{IN} can set the voltage on the FCB pin.

When $EXTV_{CC}$ pin is grounded or open, an integrated 5V linear regulator powers the controller and MOSFET gate drivers. If a minimum 4.7V external bias supply is applied on the $EXTV_{CC}$ pin, the internal regulator is turned off, and an internal switch connects $EXTV_{CC}$ to the gate driver voltage. This eliminates the linear regulator power loss with high input voltage, reducing the thermal stress on the controller. The maximum voltage on $EXTV_{CC}$ pin is 6V. The $EXTV_{CC}$ voltage should never be higher than the V_{IN} voltage. Also $EXTV_{CC}$ must be sequenced after V_{IN} . Recommended for 24V operation to lower temperature in the µModule.

APPLICATIONS INFORMATION

The typical LTM4602HV application circuit is shown in Figure 20. External component selection is primarily determined by the maximum load current and output voltage.

Output Voltage Programming and Margining

The PWM controller of the LTM4602HV has an internal $0.6V \pm 1\%$ reference voltage. As shown in the block diagram, a $100k/0.5\%$ internal feedback resistor connects V_{OUT} and FB pins. Adding a resistor R_{SET} from V_{OSET} pin to SGND pin programs the output voltage:

$$V_O = 0.6V \cdot \frac{100k + R_{SET}}{R_{SET}}$$

Table 1 shows the standard values of 1% R_{SET} resistor for typical output voltages:

Table 1

R_{SET} (k Ω)	Open	100	66.5	49.9	43.2	31.6	22.1	13.7
V_O (V)	0.6	1.2	1.5	1.8	2	2.5	3.3	5

Voltage margining is the dynamic adjustment of the output voltage to its worst case operating range in production testing to stress the load circuitry, verify control/protection functionality of the board and improve the system reliability. Figure 2 shows how to implement margining function with the LTM4602HV. In addition to the feedback resistor R_{SET} , several external components are added. Turn off both transistor Q_{UP} and Q_{DOWN} to disable the margining. When Q_{UP} is on and Q_{DOWN} is off, the output

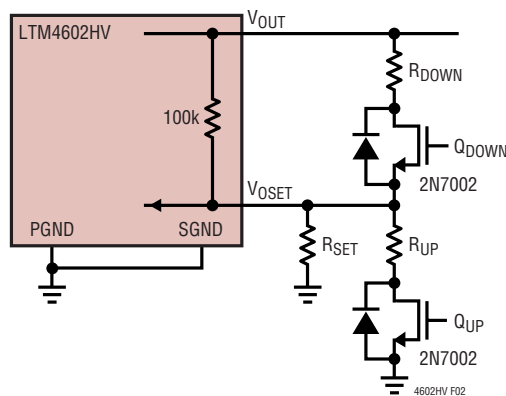


Figure 2

voltage is margined up. The output voltage is margined down when Q_{DOWN} is on and Q_{UP} is off. If the output voltage V_O needs to be margined up/down by $\pm M\%$, the resistor values of R_{UP} and R_{DOWN} can be calculated from the following equations:

$$\frac{(R_{SET} \parallel R_{UP}) \cdot V_O \cdot (1 + M\%)}{(R_{SET} \parallel R_{UP}) + 100k\Omega} = 0.6V$$

$$\frac{R_{SET} \cdot V_O \cdot (1 - M\%)}{R_{SET} + (100k\Omega \parallel R_{DOWN})} = 0.6V$$

Input Capacitors

The LTM4602HV μ Module should be connected to a low ac-impedance DC source. High frequency, low ESR input capacitors are required to be placed adjacent to the module. In Figure 20, the bulk input capacitor C_{IN} is selected for its ability to handle the large RMS current into the converter. For a buck converter, the switching duty-cycle can be estimated as:

$$D = \frac{V_O}{V_{IN}}$$

Without considering the inductor current ripple, the RMS current of the input capacitor can be estimated as:

$$I_{CIN(RMS)} = \frac{I_{O(MAX)}}{\eta\%} \cdot \sqrt{D \cdot (1 - D)}$$

In the above equation, $\eta\%$ is the estimated efficiency of the power module. C_1 can be a switcher-rated electrolytic aluminum capacitor, OS-CON capacitor or high volume ceramic capacitors. Note the capacitor ripple current ratings are often based on only 2000 hours of life. This makes it advisable to properly derate the input capacitor, or choose a capacitor rated at a higher temperature than required. Always contact the capacitor manufacturer for derating requirements.

In Figure 16, the input capacitors are used as high frequency input decoupling capacitors. In a typical 6A output application, 1-2 pieces of very low ESR X5R or X7R, $10\mu F$ ceramic capacitors are recommended. This decoupling capacitor should be placed directly adjacent the module input pins

APPLICATIONS INFORMATION

in the PCB layout to minimize the trace inductance and high frequency AC noise.

Output Capacitors

The LTM4602HV is designed for low output voltage ripple. The bulk output capacitor C_{OUT} is chosen with low enough effective series resistance (ESR) to meet the output voltage ripple and transient requirements. C_{OUT} can be low ESR tantalum capacitor, low ESR polymer capacitor or ceramic capacitor (X5R or X7R). The typical capacitance is 200 μ F if all ceramic output capacitors are used. The internally optimized loop compensation provides sufficient stability margin for all ceramic capacitors applications. Additional output filtering may be required by the system designer, if further reduction of output ripple or dynamic transient spike is required. Refer to Table 2 for an output capacitance matrix for each output voltage Droop, peak to peak deviation and recovery time during a 3A/ μ s transient with a specific output capacitance.

Fault Conditions: Current Limit and Over current Foldback

The LTM4602HV has a current mode controller, which inherently limits the cycle-by-cycle inductor current not only in steady state operation, but also in transient.

To further limit current in the event of an over load condition, the LTM4602HV provides foldback current limiting. If the output voltage falls by more than 50%, then the maximum output current is progressively lowered to about one sixth of its full current limit value.

Soft-Start and Latchoff with the RUN/SS pin

The RUN/SS pin provides a means to shut down the LTM4602HV as well as a timer for soft-start and over-current latchoff. Pulling the RUN/SS pin below 0.8V puts the LTM4602HV into a low quiescent current shutdown ($I_Q \leq 75\mu$ A). Releasing the pin allows an internal 1.2 μ A current source to charge up the timing capacitor C_{SS} . Inside LTM4602HV, there is an internal 1000pF capacitor from RUN/SS pin to ground. If RUN/SS pin has an external capacitor C_{SS_EXT} to ground, the delay before starting is about:

$$t_{DELAY} = \frac{1.5V}{1.2\mu A} \cdot (C_{SS_EXT} + 1000pF)$$

When the voltage on RUN/SS pin reaches 1.5V, the LTM4602HV internal switches are operating with a clamping of the maximum output inductor current limited by the RUN/SS pin total soft-start capacitance. As the RUN/SS pin voltage rises to 3V, the soft-start clamping of the inductor current is released.

V_{IN} to V_{OUT} Stepdown Ratios

There are restrictions in the maximum V_{IN} to V_{OUT} step down ratio that can be achieved for a given input voltage. These constraints are shown in the Typical Performance Characteristics curves labeled “ V_{IN} to V_{OUT} Stepdown Ratio”. Note that additional thermal de-rating may apply. See the Thermal Considerations and Output Current De-Rating sections of this data sheet.

APPLICATIONS INFORMATION

Table 2. Output Voltage Response Versus Component Matrix (Refer to Figure 17), 0A to 3A Step (Typical Values)

TYPICAL MEASURED VALUES			
C _{OUT1} VENDORS	PART NUMBER	C _{OUT2} VENDORS	PART NUMBER
TDK	C4532X5R0J107MZ (100UF, 6.3V)	SANYO POS CAP	6TPE330MIL (330μF, 6.3V)
TAIYO YUDEN	JMK432BJ107MU-T (100μF, 6.3V)	SANYO POS CAP	2R5TPE470M9 (470μF, 2.5V)
TAIYO YUDEN	JMK316BJ226ML-T501 (22μF, 6.3V)	SANYO POS CAP	4TPE470MCL (470μF, 4V)

V _{OUT} (V)	C _{IN} (CERAMIC)	C _{IN} (BULK)	C _{OUT1} (CERAMIC)	C _{OUT2} (BULK)	C _{COMP}	C3	V _{IN} (V)	DROOP (mV)	PEAK TO PEAK (mV)	RECOVERY TIME (μs)	LOAD STEP (A/μs)
1.2	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	5	30	60	25	3
1.2	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	5	30	60	20	3
1.2	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	5	25	54	20	3
1.2	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	5	25	55	20	3
1.2	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	12	30	60	25	3
1.2	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	12	25	54	20	3
1.2	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	12	25	56	20	3
1.2	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	12	25	55	20	3
1.5	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	5	25	50	25	3
1.5	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	5	25	54	20	3
1.5	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	5	25	59	20	3
1.5	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	5	26	59	20	3
1.5	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	12	25	55	25	3
1.5	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	12	25	54	20	3
1.5	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	12	28	59	20	3
1.5	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	12	26	59	20	3
1.8	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	5	25	54	30	3
1.8	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	5	25	50	20	3
1.8	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	5	25	50	20	3
1.8	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	5	29	60	20	3
1.8	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	100pF	12	25	50	30	3
1.8	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 2.5V	NONE	100pF	12	25	50	20	3
1.8	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	100pF	12	25	50	20	3
1.8	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	12	29	60	20	3
2.5	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 4V	NONE	220pF	5	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	220pF	5	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	220pF	5	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	220pF	5	25	50	25	3
2.5	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 4V	NONE	220pF	12	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	220pF	12	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	220pF	12	25	50	30	3
2.5	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	220pF	12	27	54	25	3
3.3	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	220pF	7	32	64	30	3
3.3	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 4V	NONE	220pF	7	30	60	30	3
3.3	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	220pF	7	30	60	35	3
3.3	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	220pF	7	32	64	25	3
3.3	2 × 10μF 25V	150μF 35V	1 × 100μF 6.3V	470μF 4V	NONE	220pF	12	38	58	30	3
3.3	2 × 10μF 25V	150μF 35V	3 × 22μF 6.3V	470μF 4V	NONE	220pF	12	30	60	35	3
3.3	2 × 10μF 25V	150μF 35V	2 × 100μF 6.3V	330μF 6.3V	NONE	220pF	12	30	60	30	3
3.3	2 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	220pF	12	32	64	25	3
5	1 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	15	80	160	25	3
5	1 × 10μF 25V	150μF 35V	4 × 100μF 6.3V	NONE	NONE	100pF	20	80	160	25	3

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After the controller has been started and given adequate time to charge up the output capacitor, C_{SS} is used as a short-circuit timer. After the RUN/SS pin charges above 4V, if the output voltage falls below 75% of its regulated value, then a short-circuit fault is assumed. A $1.8\mu\text{A}$ current then begins discharging C_{SS} . If the fault condition persists until the RUN/SS pin drops to 3.5V, then the controller turns off both power MOSFETs, shutting down the converter permanently. The RUN/SS pin must be actively pulled down to ground in order to restart operation.

The over-current protection timer requires the soft-start timing capacitor C_{SS} be made large enough to guarantee that the output is in regulation by the time C_{SS} has reached the 4V threshold. In general, this will depend upon the size of the output capacitance, output voltage and load current characteristic. A minimum external soft-start capacitor can be estimated from:

$$C_{SS_EXT} + 1000\text{pF} > C_{OUT} \cdot V_{OUT} (10^{-3} [\text{F} / \text{Vs}])$$

Generally $0.1\mu\text{F}$ is more than sufficient.

Since the load current is already limited by the current mode control and current foldback circuitry during a short circuit, overcurrent latchoff operation is NOT always needed or desired, especially if the output has large capacitance or the load draws high current during start-up. The latchoff feature can be overridden by a pull-up current greater than $5\mu\text{A}$ but less than $80\mu\text{A}$ to the RUN/SS pin. The additional current prevents the discharge of C_{SS} during a fault and also shortens the soft-start period. Using a resistor from RUN/SS pin to V_{IN} is a simple solution to defeat latchoff. Any pull-up network must be able to maintain RUN/SS above

4V maximum latchoff threshold and overcome the $4\mu\text{A}$ maximum discharge current. Figure 3 shows a conceptual drawing of $V_{RUN/SS}$ during startup and short circuit.

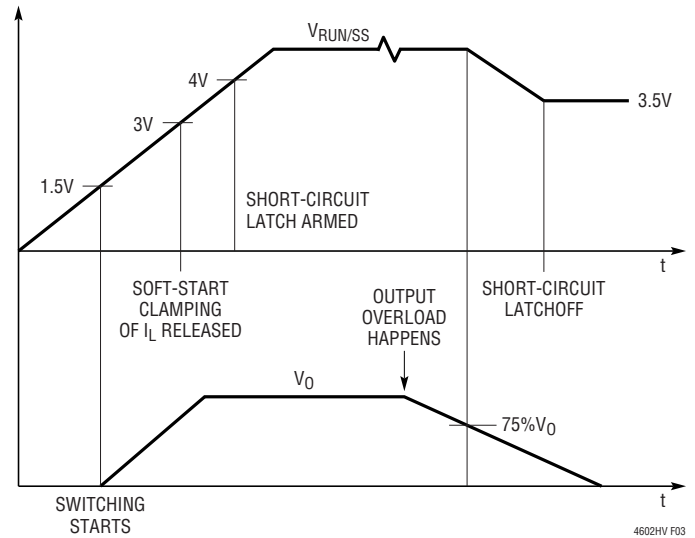


Figure 3. RUN/SS Pin Voltage During Startup and Short-Circuit Protection

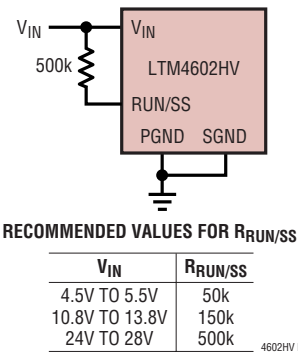


Figure 4. Defeat Short-Circuit Latchoff with a Pull-Up Resistor to V_{IN}

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Enable

The RUN/SS pin can be driven from logic as shown in Figure 5. This function allows the LTM4602HV to be turned on or off remotely. The $\overline{\text{ON}}$ signal can also control the sequence of the output voltage.

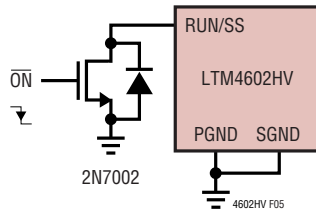


Figure 5. Enable Circuit with External Logic

Output Voltage Tracking

For the applications that require output voltage tracking, several LTM4602HV modules can be programmed by the power supply tracking controller such as the LTC2923. Figure 6 shows a typical schematic with LTC2923. Coincident, ratiometric and offset tracking for V_O rising and falling can be implemented with different sets of resistor values. See the LTC2923 data sheet for more details.

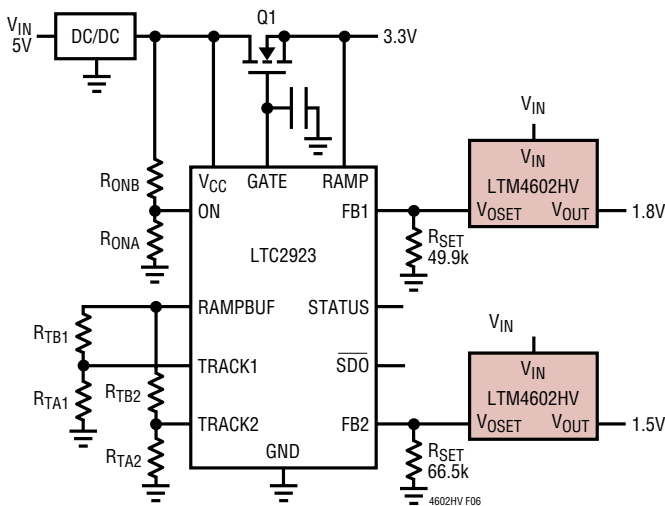


Figure 6. Output Voltage Tracking with the LTC2923 Controller

EXTV_{CC} Connection

An internal low dropout regulator produces an internal 5V supply that powers the control circuitry and FET drivers. Therefore, if the system does not have a 5V power rail, the LTM4602HV can be directly powered by V_{IN} . The gate driver current through LDO is about 16mA. The internal LDO power dissipation can be calculated as:

$$P_{LDO_LOSS} = 16\text{mA} \cdot (V_{IN} - 5\text{V})$$

The LTM4602HV also provides an external gate driver voltage pin EXTV_{CC} . If there is a 5V rail in the system, it is recommended to connect EXTV_{CC} pin to the external 5V rail. Whenever the EXTV_{CC} pin is above 4.7V, the internal 5V LDO is shut off and an internal 50mA P-channel switch connects the EXTV_{CC} to internal 5V. Internal 5V is supplied from EXTV_{CC} until this pin drops below 4.5V. Do not apply more than 6V to the EXTV_{CC} pin and ensure that $\text{EXTV}_{CC} < V_{IN}$. The following list summarizes the possible connections for EXTV_{CC} :

1. EXTV_{CC} grounded. Internal 5V LDO is always powered from the internal 5V regulator.
2. EXTV_{CC} connected to an external supply. Internal LDO is shut off. A high efficiency supply compatible with the MOSFET gate drive requirements (typically 5V) can improve overall efficiency. With this connection, it is always required that the EXTV_{CC} voltage can not be higher than V_{IN} pin voltage.

Discontinuous Operation and FCB Pin

The FCB pin determines whether the internal bottom MOSFET remains on when the inductor current reverses. There is an internal 10k pulling down resistor connecting this pin to ground. The default light load operation mode is forced continuous (PWM) current mode. This mode provides minimum output voltage ripple.

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In the application where the light load efficiency is important, tying the FCB pin above 0.6V threshold enables discontinuous operation where the bottom MOSFET turns off when inductor current reverses. Therefore, the conduction loss is minimized and light load efficiency is improved. The penalty is that the controller may skip cycle and the output voltage ripple increases at light load.

Paralleling Operation with Load Sharing

Two or more LTM4602HV modules can be paralleled to provide higher than 6A output current. Figure 7 shows the necessary interconnection between two paralleled modules. The OPTI-LOOP™ current mode control ensures good current sharing among modules to balance the thermal stress. The new feedback equation for two or more LTM4602HVs in parallel is:

$$V_{OUT} = 0.6V \cdot \frac{100k}{N} + R_{SET}$$

where N is the number of LTM4602HVs in parallel.

Thermal Considerations and Output Current Derating

The power loss curves in Figures 8 and 15 can be used in coordination with the load current derating curves in Figures 9 to 14, and Figures 16 to 19 for calculating an

approximate θ_{JA} for the module with various heatsinking methods. Thermal models are derived from several temperature measurements at the bench, and thermal modeling analysis. Application Note 103 provides a detailed explanation of the analysis for the thermal models, and the derating curves. Tables 3 and 4 provide a summary of the equivalent θ_{JA} for the noted conditions. These equivalent θ_{JA} parameters are correlated to the measure values, and improved with air-flow. The case temperature is maintained at 100°C or below for the derating curves. This allows for 4W maximum power dissipation in the total module with top and bottom heatsinking, and 2W power dissipation through the top of the module with an approximate θ_{JC} between 6°C/W to 9°C/W. This equates to a total of 124°C at the junction of the device. The θ_{JA} values in Tables 3 and 4 can be used to derive the derating curves for other output voltages.

Safety Considerations

The LTM4602HV modules do not provide isolation from V_{IN} to V_{OUT} . There is no internal fuse. If required, a slow blow fuse with a rating twice the maximum input current should be provided to protect each unit from catastrophic failure.

OPTI-LOOP is a trademark of Linear Technology Corporation.

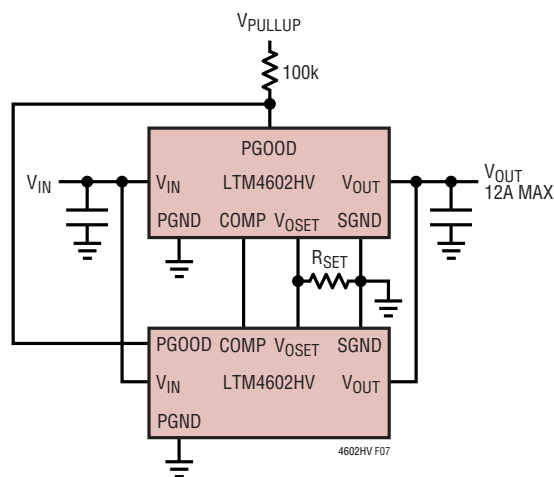
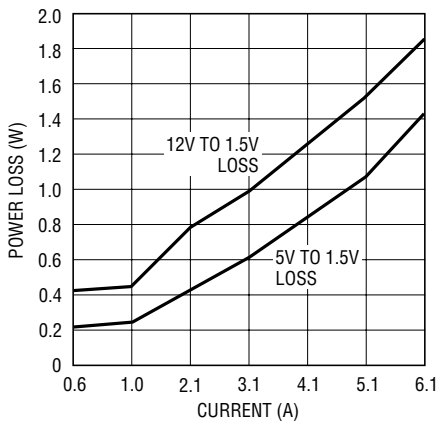


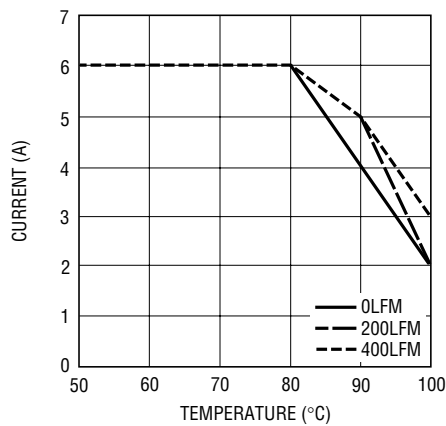
Figure 7. Parallel Two μ Modules with Load Sharing

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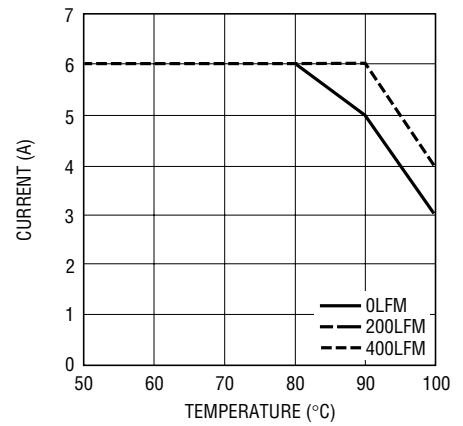
4602HV F08

Figure 8. 1.5V Power Loss Curves vs Load Current



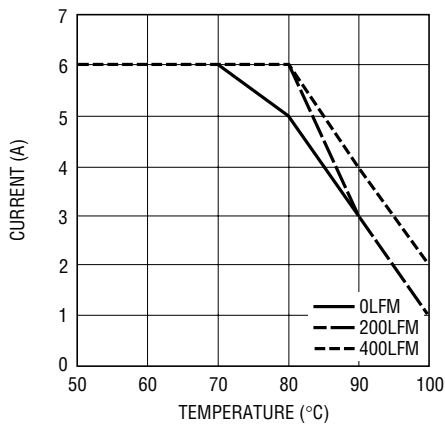
4602HV F09

Figure 9. 5V to 1.5V, No Heatsink



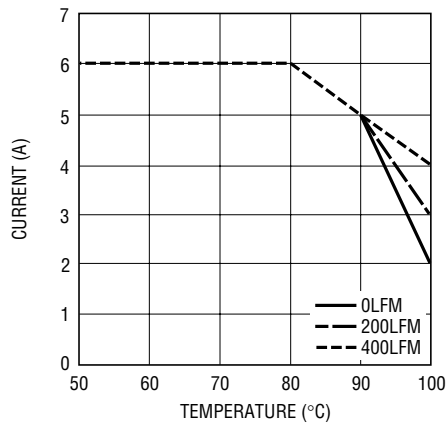
4602HV F10

Figure 10. 5V to 1.5V, BGA Heatsink



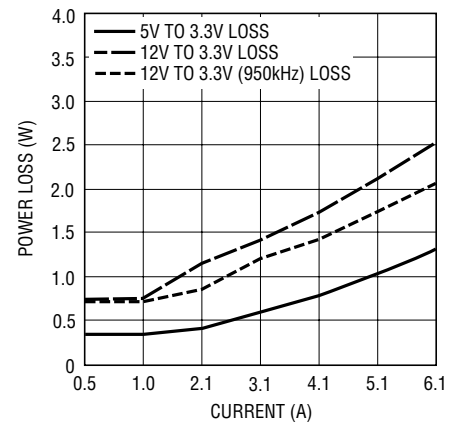
4602HV F11

Figure 11. 12V to 1.5V, No Heatsink



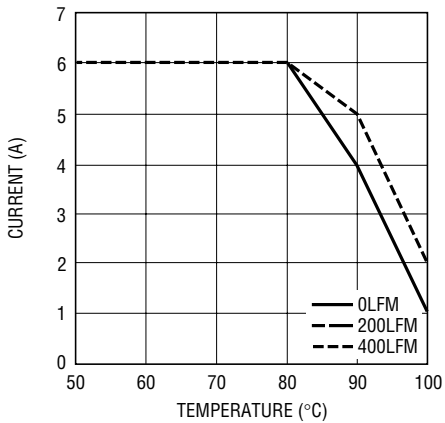
4602HV F09

Figure 12. 12V to 1.5V, BGA Heatsink



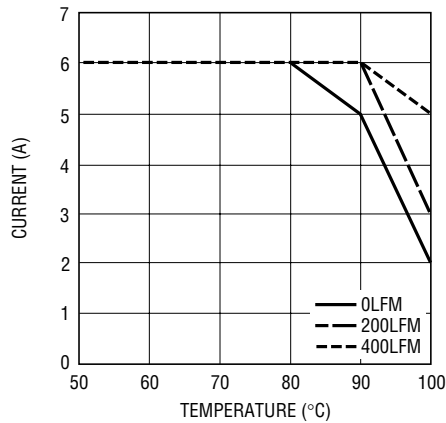
4602HV F13

Figure 13. 3.3V Power Loss



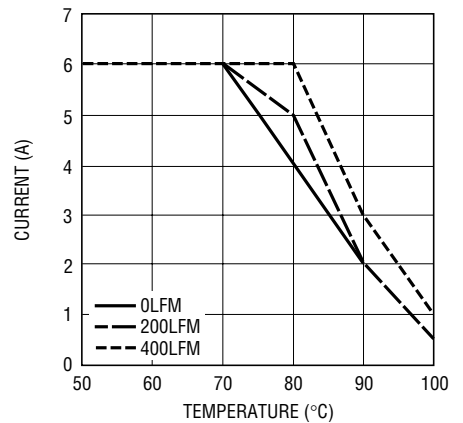
4602HV F14

Figure 14. 5V to 3.3V, No Heatsink



4602HV F15

Figure 15. 5V to 3.3V, BGA Heatsink



4602HV F16

Figure 16. 12V to 3.3V (950kHz), No Heatsink

APPLICATIONS INFORMATION

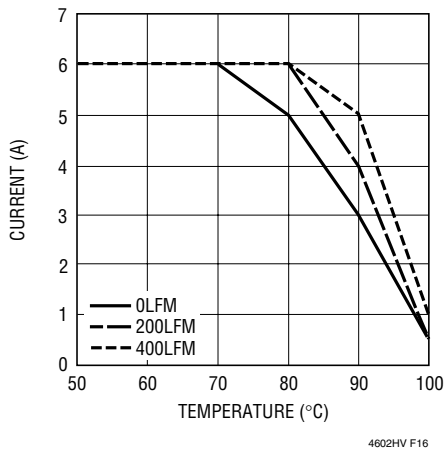


Figure 17. 12V to 3.3V (950kHz), BGA Heatsink

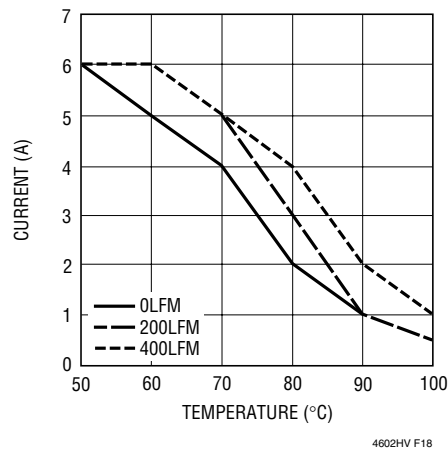


Figure 18. 24V to 3.3V, No Heatsink

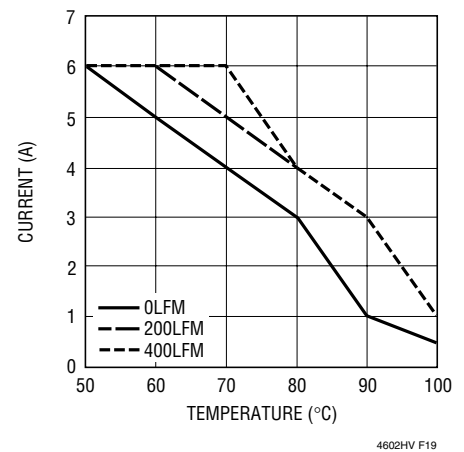


Figure 19. 24V to 3.3V, BGA Heatsink

Table 3. 1.5V Output

AIR FLOW (LFM)	HEATSINK	θ_{JA} (°C/W)
0	None	15.2
200	None	14
400	None	12
0	BGA Heatsink	13.9
200	BGA Heatsink	11.3
400	BGA Heatsink	10.25

Table 4. 3.3V Output

AIR FLOW (LFM)	HEATSINK	θ_{JA} (°C/W)
0	None	15.2
200	None	14.6
400	None	13.4
0	BGA Heatsink	13.9
200	BGA Heatsink	11.1
400	BGA Heatsink	10.5

Layout Checklist/Example

The high integration of the LTM4602HV makes the PCB board layout very simple and easy. However, to optimize its electrical and thermal performance, some layout considerations are still necessary.

- Use large PCB copper areas for high current path, including V_{IN} , PGND and V_{OUT} . It helps to minimize the PCB conduction loss and thermal stress
- Place high frequency ceramic input and output capacitors next to the V_{IN} , PGND and V_{OUT} pins to minimize high frequency noise
- Place a dedicated power ground layer underneath the unit
- To minimize the via conduction loss and reduce module thermal stress, use multiple vias for interconnection between top layer and other power layers

- Do not put via directly on pad
- Use a separated SGND ground copper area for components connected to signal pins. Connect the SGND to PGND underneath the unit

Figure 20 gives a good example of the recommended layout.

LTM4602 Frequency Adjustment

The LTM4602HV is designed to typically operate at 850kHz across most input and output conditions. The control architecture is constant on time valley mode current control. The f_{ADJ} pin is typically left open or decoupled with an optional 1000pF capacitor. The switching frequency has been optimized to maintain constant output ripple over the operating conditions. The equations for setting the operating frequency are set around a programmable constant on time. This on time is developed by a programmable

4602hvf

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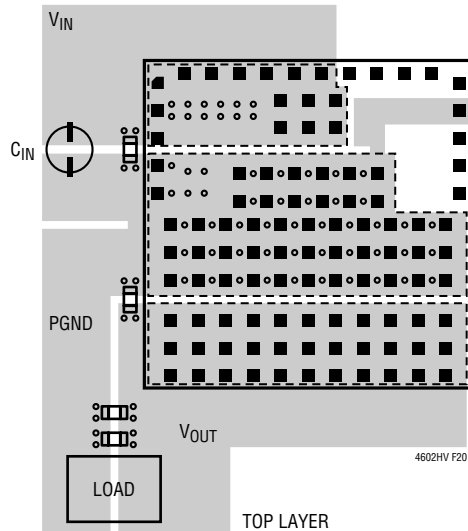


Figure 20. Recommended PCB Layout

current into an on board 10pF capacitor that establishes a ramp that is compared to a voltage threshold that is equal to the output voltage up to a 2.4V clamp. This I_{ON} current is equal to: $I_{ON} = (V_{IN} - 0.7V)/110k$, with the 110k onboard resistor from V_{IN} to f_{ADJ} . The on time is equal to $t_{ON} = (V_{OUT}/I_{ON}) \cdot 10pF$ and $t_{OFF} = t_s - t_{ON}$. The frequency is equal to: $Freq. = DC/t_{ON}$. The I_{ON} current is proportional to V_{IN} , and the regulator duty cycle is inversely proportional to V_{IN} , therefore the step-down regulator will remain relatively constant frequency as the duty cycle adjustment takes place with lowering V_{IN} . The on time is proportional to V_{OUT} up to a 2.4V clamp. This will hold frequency relatively constant with different output voltages up to 2.4V. The regulator switching period is comprised of the on time and off time as depicted in Figure 21. The on time is equal to $t_{ON} = (V_{OUT}/I_{ON}) \cdot 10pF$ and $t_{OFF} = t_s - t_{ON}$. The frequency is equal to: $Frequency = DC/t_{ON}$.

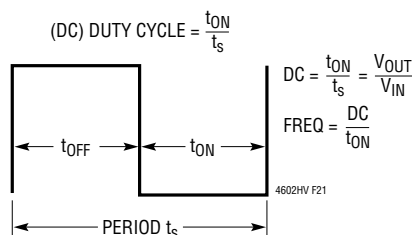


Figure 21

The LTM4602 has a minimum (t_{ON}) on time of 100 nanoseconds and a minimum (t_{OFF}) off time of 400 nanoseconds. The 2.4V clamp on the ramp threshold as a function of V_{OUT} will cause the switching frequency to increase by the ratio of $V_{OUT}/2.4V$ for 3.3V and 5V outputs. This is due to the fact the on time will not increase as V_{OUT} increases past 2.4V. Therefore, if the nominal switching frequency is 850kHz, then the switching frequency will increase to ~1.2MHz for 3.3V, and ~1.7MHz for 5V outputs due to $Frequency = (DC/t_{ON})$. When the switching frequency increases to 1.2MHz, then the time period t_s is reduced to ~833 nanoseconds and at 1.7MHz the switching period reduces to ~588 nanoseconds. When higher duty cycle conversions like 5V to 3.3V and 12V to 5V need to be accommodated, then the switching frequency can be lowered to alleviate the violation of the 400ns minimum off time. Since the total switching period is $t = t_{ON} + t_{OFF}$, t_{OFF} will be below the 400ns minimum off time. A resistor from the f_{ADJ} pin to ground can shunt current away from the on time generator, thus allowing for a longer on time and a lower switching frequency. 12V to 5V and 5V to 3.3V derivations are explained in the data sheet to lower switching frequency and accommodate these step-down conversions.

Equations for setting frequency: $V_{OUT} = 5V$

$$I_{ON} = (V_{IN} - 0.7V)/110k; \text{ for } 12V \text{ input, } I_{ON} = 103\mu A$$

$$frequency = (I_{ON}/[2.4V \cdot 10pF]) \cdot (DC) = 1.79MHz;$$

$$DC = \text{duty cycle, duty cycle is } (V_{OUT}/V_{IN})$$

$$t = t_{ON} + t_{OFF}, t_{ON} = \text{on-time, } t_{OFF} = \text{off-time of the switching period; } t = 1/\text{frequency}$$

t_{OFF} must be greater than 400ns, or $t - t_{ON} > 400ns$.

$$t_{ON} = DC \cdot t$$

1MHz frequency or 1 μs period is chosen.

$$t_{ON} = 0.41 \cdot 1\mu s \approx 410ns$$

$$t_{OFF} = 1\mu s - 410ns \approx 590ns$$

t_{ON} and t_{OFF} are above the minimums with adequate guard band.

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Using the frequency = $(I_{ON}/[2.4V \cdot 10pF]) \cdot (DC)$, solve for $I_{ON} = (1MHz \cdot 2.4V \cdot 10pF) \cdot (1/0.41) \cong 58\mu A$. I_{ON} current calculated from 12V input was $103\mu A$, so a resistor from f_{ADJ} to ground = $(0.7V/15k) = 46\mu A$. $103\mu A - 46\mu A = 57\mu A$, sets the adequate I_{ON} current for proper frequency range for the higher duty cycle conversion of 12V to 5V. Input voltage range is limited to 8V to 16V. Higher input voltages can be used without the 15k on f_{ADJ} . The inductor ripple current gets too high above 16V or below 8V.

Equations for setting frequency: $V_{OUT} = 3.3V$

$$I_{ON} = (V_{IN} - 0.7V)/110k; \text{ for } 5V \text{ input, } I_{ON} = 39\mu A$$

$$\text{frequency} = (I_{ON}/[2.4V \cdot 10pF]) \cdot (DC) = 1.07MHz;$$

DC = duty cycle, duty cycle is (V_{OUT}/V_{IN})

$$t = t_{ON} + t_{OFF}, t_{ON} = \text{on-time, } t_{OFF} = \text{off-time of the switching period; } t = 1/\text{frequency}$$

t_{OFF} must be greater than 400ns, or $t - t_{ON} > 400ns$.

$$t_{ON} = DC \cdot t$$

~450kHz frequency or 2.22 μs period is chosen. Frequency range is about 450kHz to 650kHz from 4.5V to 7V input.

$$t_{ON} = 0.66 \cdot 2.22\mu s \cong 1.46\mu s$$

$$t_{OFF} = 2.22\mu s - 1.46\mu s \cong 760ns$$

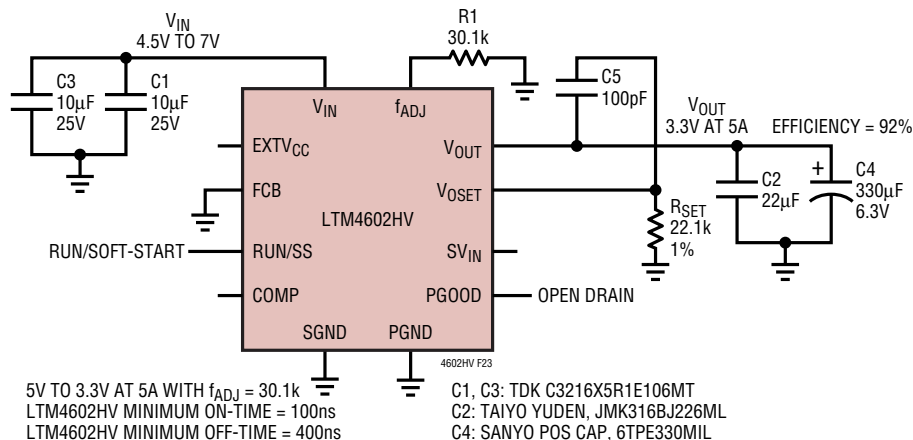
t_{ON} and t_{OFF} are above the minimums with adequate guard band.

Using the frequency = $(I_{ON}/[2.4V \cdot 10pF]) \cdot (DC)$, solve for $I_{ON} = (450kHz \cdot 2.4V \cdot 10pF) \cdot (1/0.66) \cong 16\mu A$. I_{ON} current calculated from 5V input was $39\mu A$, so a resistor from f_{ADJ} to ground = $(0.7V/30.1k) = 23\mu A$. $39\mu A - 23\mu A = 16\mu A$, sets the adequate I_{ON} current for proper frequency range for the higher duty cycle conversion of 5V to 3.3V. Input voltage range is limited to 4.5V to 7V. Higher input voltages can be used without the 30.1k on f_{ADJ} . The inductor ripple current gets too high above 7V, and the 400ns minimum off-time is limited below 4.5V.

Therefore, at 3.3V output, a 30.1k resistor is recommended to add from pin f_{ADJ} to ground when the input voltage is between 4.5V to 7V. However, this resistor needs to be removed to avoid high inductor ripple current when the input voltage is more than 7V. Similarly, for 5V output, a 15k resistor is recommended to adjust the frequency when the input voltage is between 8V to 16V. This 15k resistor is removed when the input voltage becomes higher than 16V. Please refer to the Typical Performance curve V_{IN} to V_{OUT} Step-Down Ratio.

In 12V to 3.3V and 24V to 3.3V applications, if a 35k resistor is added from the f_{ADJ} pin to ground, then a 2% efficiency gain will be achieved as shown in the 12V and 24V efficiency graphs shown in the Typical Characteristics. This is due to lowering the transition losses in the power MOSFETs by reducing the switching frequency from 1.3MHz to 1MHz.

5V to 3.3V at 5A



APPLICATIONS INFORMATION

12V to 5V at 5A

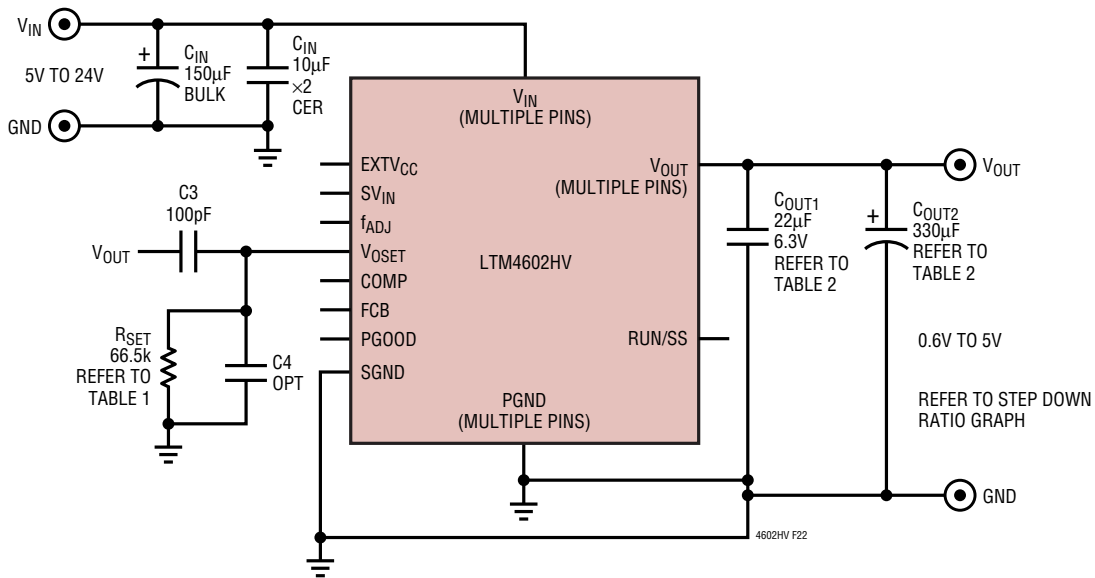
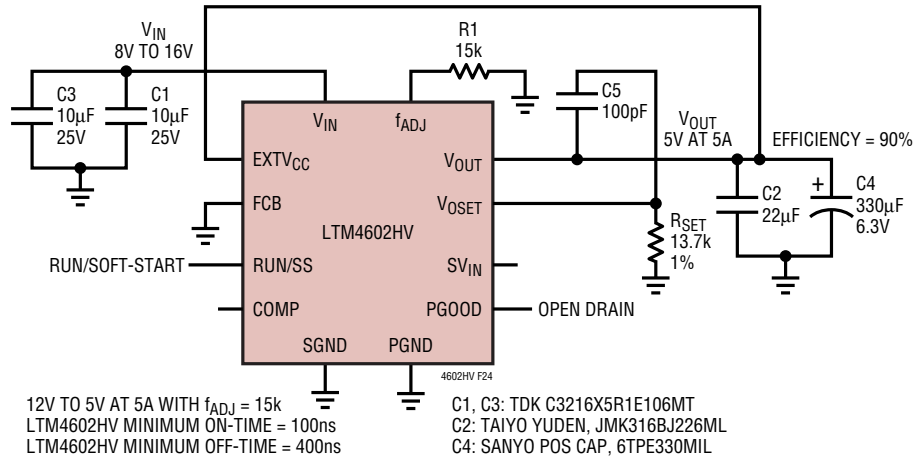
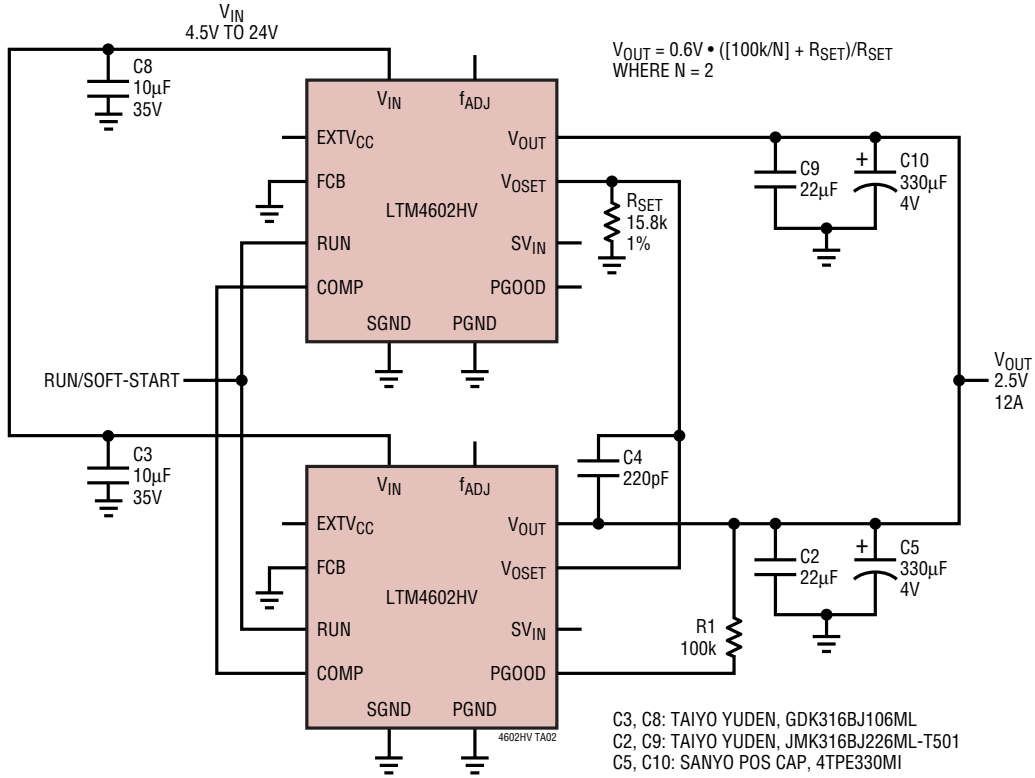


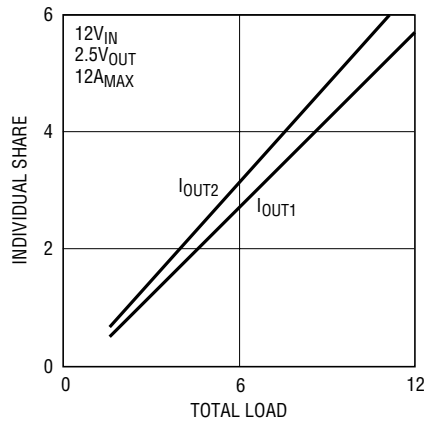
Figure 22. Typical Application, 5V to 24V Input, 0.6V to 6V Output, 6A Max

TYPICAL APPLICATION

Parallel Operation and Load Sharing

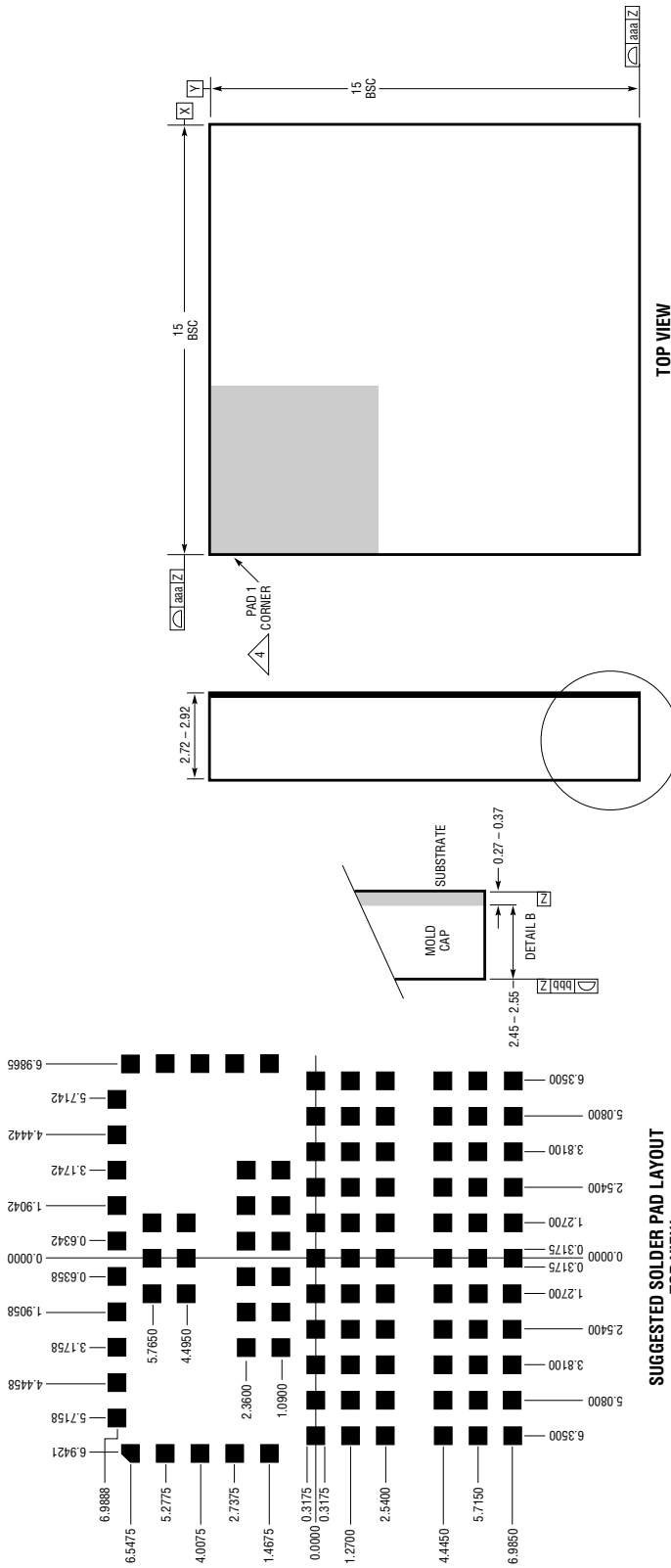


Current Sharing Between Two LTM4602HV Modules



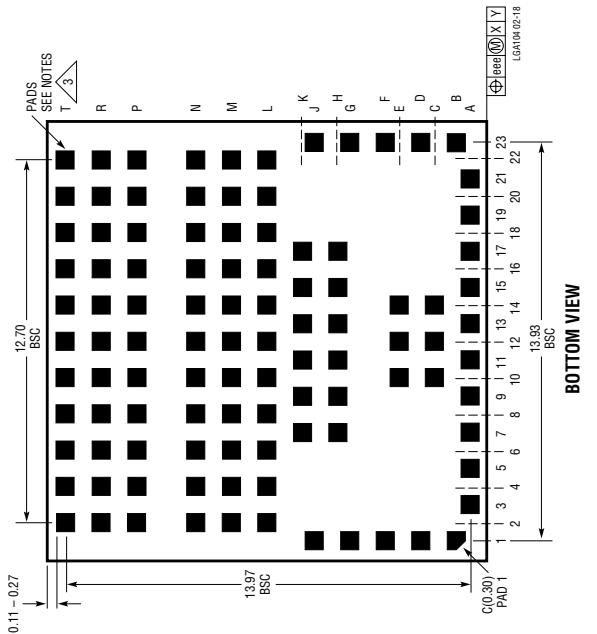
PACKAGE DESCRIPTION

LGA Package
104-Lead (15mm x 15mm)
 (Reference LTM DWG # 05-05-1800)



- NOTES:**
1. DIMENSIONING AND TOLERANCING PER ASME Y14.5M-1994
 2. ALL DIMENSIONS ARE IN MILLIMETERS
 3. LAND DESIGNATION PER JEDEC MO-222, SPP-010
 4. DETAILS OF PAD #1 IDENTIFIER ARE OPTIONAL, BUT MUST BE LOCATED WITHIN THE ZONE INDICATED. THE PAD #1 IDENTIFIER IS A MARKED FEATURE OR A NOTCHED BEVELED PAD
 5. PRIMARY DATUM - Z - IS SEATING PLANE
 6. THE TOTAL NUMBER OF PADS: 104

SYMBOL	TOLERANCE
aaa	0.15
bbb	0.10
eee	0.15



PACKAGE DESCRIPTION

Pin Assignment Tables
(Arranged by Pin Number)

PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME
A1 -	B1 V_{IN}	C1 -	D1 V_{IN}	E1 -	F1 V_{IN}	G1 PGND	H1 -
A2 -	B2 -	C2 -	D2 -	E2 -	F2 -	G2 -	H2 -
A3 V_{IN}	B3 -	C3 -	D3 -	E3 -	F3 -	G3 -	H3 -
A4 -	B4 -	C4 -	D4 -	E4 -	F4 -	G4 -	H4 -
A5 V_{IN}	B5 -	C5 -	D5 -	E5 -	F5 -	G5 -	H5 -
A6 -	B6 -	C6 -	D6 -	E6 -	F6 -	G6 -	H6 -
A7 V_{IN}	B7 -	C7 -	D7 -	E7 -	F7 -	G7 -	H7 PGND
A8 -	B8 -	C8 -	D8 -	E8 -	F8 -	G8 -	H8 -
A9 V_{IN}	B9 -	C9 -	D9 -	E9 -	F9 -	G9 -	H9 PGND
A10 -	B10 -	C10 V_{IN}	D10 -	E10 V_{IN}	F10 -	G10 -	H10 -
A11 V_{IN}	B11 -	C11 -	D11 -	E11 -	F11 -	G11 -	H11 PGND
A12 -	B12 -	C12 V_{IN}	D12 -	E12 V_{IN}	F12 -	G12 -	H12 -
A13 V_{IN}	B13 -	C13 -	D13 -	E13 -	F13 -	G13 -	H13 PGND
A14 -	B14 -	C14 V_{IN}	D14 -	E14 V_{IN}	F14 -	G14 -	H14 -
A15 f_{ADJ}	B15 -	C15 -	D15 -	E15 -	F15 -	G15 -	H15 PGND
A16 -	B16 -	C16 -	D16 -	E16 -	F16 -	G16 -	H16 -
A17 SV_{IN}	B17 -	C17 -	D17 -	E17 -	F17 -	G17 -	H17 PGND
A18 -	B18 -	C18 -	D18 -	E18 -	F18 -	G18 -	H18 -
A19 $EXTV_{CC}$	B19 -	C19 -	D19 -	E19 -	F19 -	G19 -	H19 -
A20 -	B20 -	C20 -	D20 -	E20 -	F20 -	G20 -	H20 -
A21 V_{OSET}	B21 -	C21 -	D21 -	E21 -	F21 -	G21 -	H21 -
A22 -	B22 -	C22 -	D22 -	E22 -	F22 -	G22 -	H22 -
A23 -	B23 COMP	C23 -	D23 SGND	E23 -	F23 RUN/SS	G23 FCB	H23 -

PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME
J1 PGND	K1 -	L1 -	M1 -	N1 -	P1 -	R1 -	T1 -
J2 -	K2 -	L2 PGND	M2 PGND	N2 PGND	P2 V_{OUT}	R2 V_{OUT}	T2 V_{OUT}
J3 -	K3 -	L3 -	M3 -	N3 -	P3 -	R3 -	T3 -
J4 -	K4 -	L4 PGND	M4 PGND	N4 PGND	P4 V_{OUT}	R4 V_{OUT}	T4 V_{OUT}
J5 -	K5 -	L5 -	M5 -	N5 -	P5 -	R5 -	T5 -
J6 -	K6 -	L6 PGND	M6 PGND	N6 PGND	P6 V_{OUT}	R6 V_{OUT}	T6 V_{OUT}
J7 -	K7 PGND	L7 -	M7 -	N7 -	P7 -	R7 -	T7 -
J8 -	K8 -	L8 PGND	M8 PGND	N8 PGND	P8 V_{OUT}	R8 V_{OUT}	T8 V_{OUT}
J9 -	K9 PGND	L9 -	M9 -	N9 -	P9 -	R9 -	T9 -
J10 -	K10 -	L10 PGND	M10 PGND	N10 PGND	P10 V_{OUT}	R10 V_{OUT}	T10 V_{OUT}
J11 -	K11 PGND	L11 -	M11 -	N11 -	P11 -	R11 -	T11 -
J12 -	K12 -	L12 PGND	M12 PGND	N12 PGND	P12 V_{OUT}	R12 V_{OUT}	T12 V_{OUT}
J13 -	K13 PGND	L13 -	M13 -	N13 -	P13 -	R13 -	T13 -
J14 -	K14 -	L14 PGND	M14 PGND	N14 PGND	P14 V_{OUT}	R14 V_{OUT}	T14 V_{OUT}
J15 -	K15 PGND	L15 -	M15 -	N15 -	P15 -	R15 -	T15 -
J16 -	K16 -	L16 PGND	M16 PGND	N16 PGND	P16 V_{OUT}	R16 V_{OUT}	T16 V_{OUT}
J17 -	K17 PGND	L17 -	M17 -	N17 -	P17 -	R17 -	T17 -
J18 -	K18 -	L18 PGND	M18 PGND	N18 PGND	P18 V_{OUT}	R18 V_{OUT}	T18 V_{OUT}
J19 -	K19 -	L19 -	M19 -	N19 -	P19 -	R19 -	T19 -
J20 -	K20 -	L20 PGND	M20 PGND	N20 PGND	P20 V_{OUT}	R20 V_{OUT}	T20 V_{OUT}
J21 -	K21 -	L21 -	M21 -	N21 -	P21 -	R21 -	T21 -
J22 -	K22 -	L22 PGND	M22 PGND	N22 PGND	P22 V_{OUT}	R22 V_{OUT}	T22 V_{OUT}
J23 PGOOD	K23 -	L23 -	M23 -	N23 -	P23 -	R23 -	T23 -

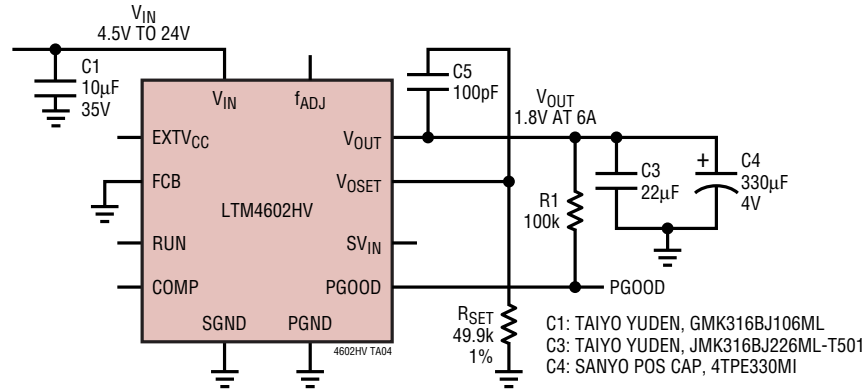
PACKAGE DESCRIPTION

Pin Assignment Tables
(Arranged by Pin Number)

PIN NAME		PIN NAME		PIN NAME		PIN NAME	
G1	PGND	P2	V _{OUT}	A3	V _{IN}	A15	f _{ADJ}
H7	PGND	P4	V _{OUT}	A5	V _{IN}	A17	SV _{IN}
H9	PGND	P6	V _{OUT}	A7	V _{IN}	A19	EXTV _{CC}
H11	PGND	P8	V _{OUT}	A9	V _{IN}	A21	V _{OSET}
H13	PGND	P10	V _{OUT}	A11	V _{IN}	B23	COMP
H15	PGND	P12	V _{OUT}	A13	V _{IN}	D23	SGND
H17	PGND	P14	V _{OUT}	B1	V _{IN}	F23	RUN/SS
J1	PGND	P16	V _{OUT}	C10	V _{IN}	G23	FCB
K7	PGND	P18	V _{OUT}	C12	V _{IN}	J23	PGOOD
K9	PGND	P20	V _{OUT}	C14	V _{IN}		
K11	PGND	P22	V _{OUT}	D1	V _{IN}		
K13	PGND	R2	V _{OUT}	E10	V _{IN}		
K15	PGND	R4	V _{OUT}	E12	V _{IN}		
K17	PGND	R6	V _{OUT}	E14	V _{IN}		
L2	PGND	R8	V _{OUT}	F1	V _{IN}		
L4	PGND	R10	V _{OUT}				
L6	PGND	R12	V _{OUT}				
L8	PGND	R14	V _{OUT}				
L10	PGND	R16	V _{OUT}				
L12	PGND	R18	V _{OUT}				
L14	PGND	R20	V _{OUT}				
L16	PGND	R22	V _{OUT}				
L18	PGND	T2	V _{OUT}				
L20	PGND	T4	V _{OUT}				
L22	PGND	T6	V _{OUT}				
M2	PGND	T8	V _{OUT}				
M4	PGND	T10	V _{OUT}				
M6	PGND	T12	V _{OUT}				
M8	PGND	T14	V _{OUT}				
M10	PGND	T16	V _{OUT}				
M12	PGND	T18	V _{OUT}				
M14	PGND	T20	V _{OUT}				
M16	PGND	T22	V _{OUT}				
M18	PGND						
M20	PGND						
M22	PGND						
N2	PGND						
N4	PGND						
N6	PGND						
N8	PGND						
N10	PGND						
N12	PGND						
N14	PGND						
N16	PGND						
N18	PGND						
N20	PGND						
N22	PGND						

TYPICAL APPLICATION

1.8V, 5A Regulator



RELATED PARTS

PART NUMBER	DESCRIPTION	COMMENTS
LTC2900	Quad Supply Monitor with Adjustable Reset Timer	Monitors Four Supplies; Adjustable Reset Timer
LTC2923	Power Supply Tracking Controller	Tracks Both Up and Down; Power Supply Sequencing
LT3825/LT3837	Synchronous Isolated Flyback Controllers	No Optocoupler Required; 3.3V, 12A Output; Simple Design
LTM4600	10A DC/DC µModule	10A Basic DC/DC µModule
LTM4601	12A DC/DC µModule with PLL, Output Tracking/Margining and Remote Sensing	Synchronizable, PolyPhase® Operation to 48A, LTM4601-1 Version has no Remote Sensing, Fast Transient Response
LTM4603	6A DC/DC µModule with PLL and Output Tracking/Margining and Remote Sensing	Synchronizable, PolyPhase Operation, LTM4603-1 Version has no Remote Sensing, Fast Transient Response

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